

# Timing and Synchronization

**A. Gallo**



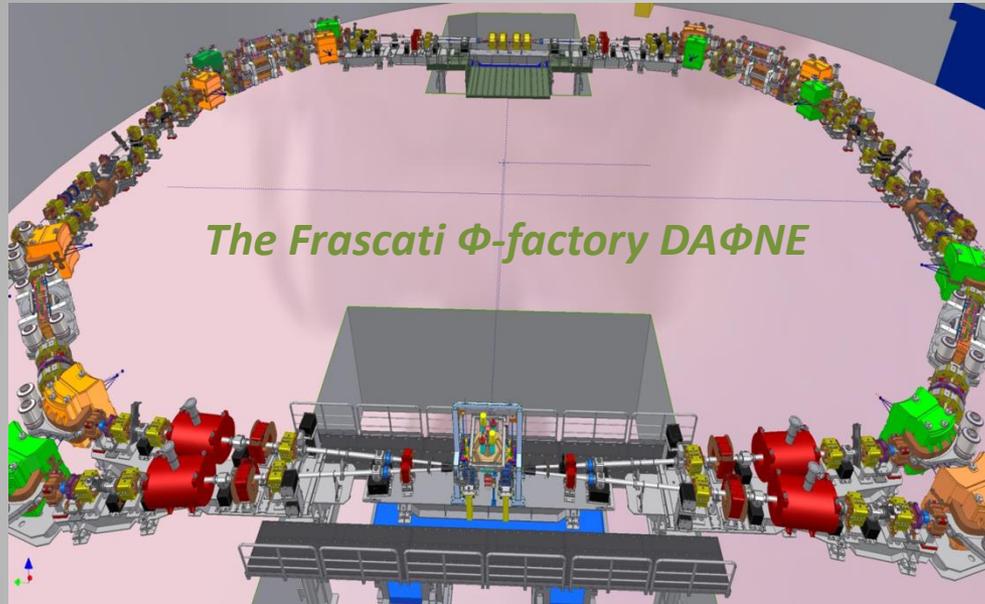
***Istituto Nazionale di Fisica Nucleare  
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## 10<sup>th</sup> International Accelerator School for Linear Colliders

December 8–19, 2016, at Mt. Fuji, Japan



- **MOTIVATIONS**
  - ✓ Why accelerators need synchronization, and at what precision level
- **DEFINITIONS AND BASICS**
  - ✓ Synchronization, Synchronization vs. Timing, Drift vs. Jitter, Master Oscillator
  - ✓ Fourier and Laplace Transforms, Random processes, Phase noise in Oscillators
  - ✓ Phase detectors, Phase Locked Loops
- **SYNCRONIZATION ARCHITECTURE AND PERFORMANCES**
  - ✓ Phase lock of synchronization clients (RF systems, Lasers, Diagnostics, ...)
  - ✓ Residual absolute and relative phase jitter
  - ✓ Reference distribution – actively stabilized links
- **BEAM ARRIVAL TIME FLUCTUATIONS**
  - ✓ Beam synchronization
  - ✓ Bunch arrival time measurement techniques
- **TIMING**
  - ✓ Trigger generation and distribution
  - ✓ Example of event sequence
- **CONCLUSIONS AND REFERENCES**

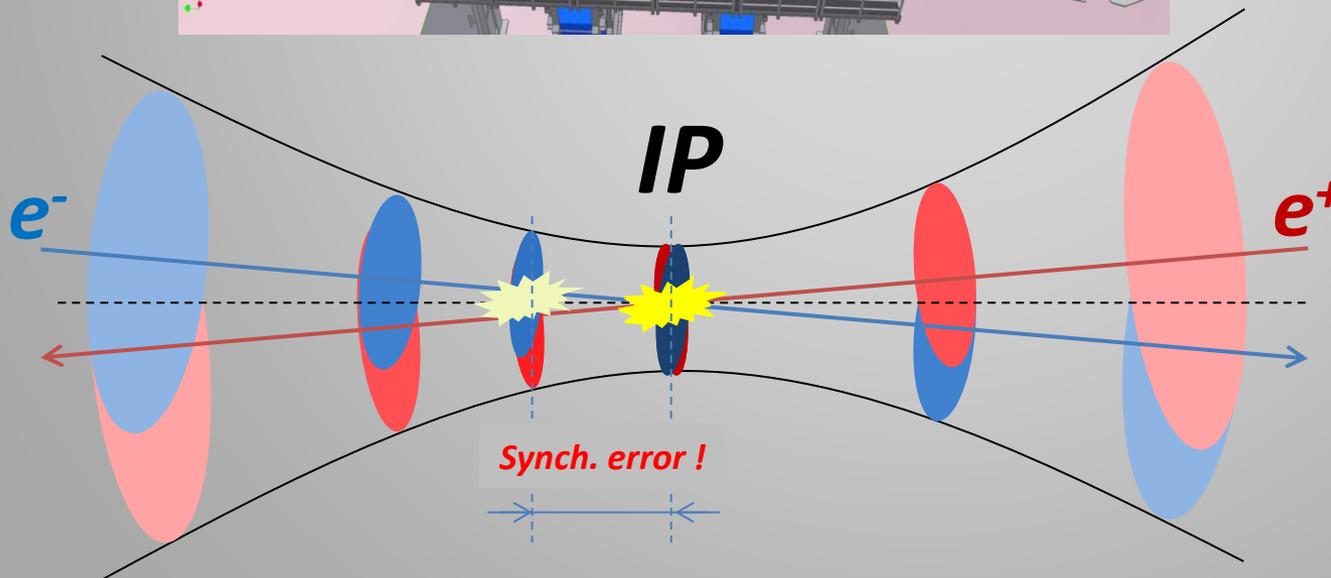


Bunches of the 2 colliding beams need to **arrive** at the **Interaction Point** (max vertical focalization) at the same time.

Waist length  $\approx \beta_y \approx \sigma_z$   
(hourglass effect)

**Synchronization requirement:**

$$\Delta t \ll \sigma_{t_{bunch}} = \frac{1}{c} \cdot \sigma_{z_{bunch}}$$



**CIRCULAR COLLIDERS:**

$$\sigma_z \approx 1 \text{ cm} \rightarrow \Delta t < 10 \text{ ps}$$

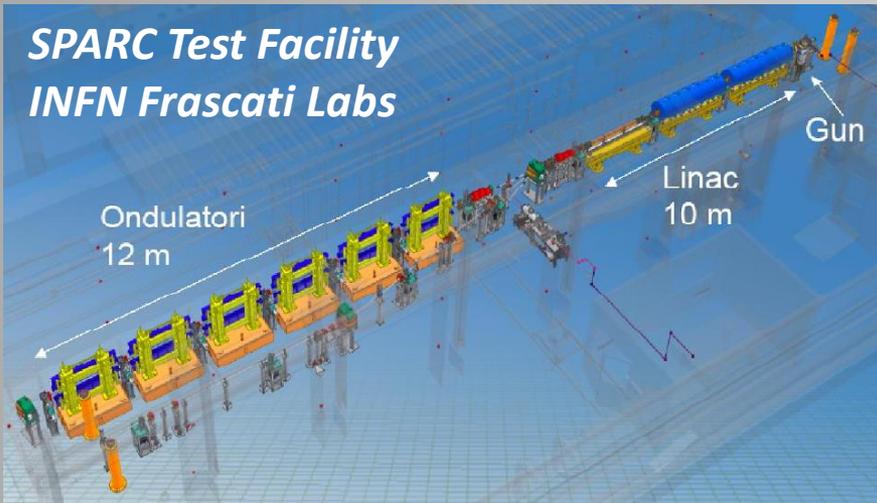
**LINEAR COLLIDER (ILC):**

$$\sigma_z < 1 \text{ mm} \rightarrow \Delta t < 1 \text{ ps}$$

**RF Stability spec**

A. Gallo, *Timing and Synchronization, Mt. Fuji (Japan), Dec. 8 – 19 2016*

## SPARC Test Facility INFN Frascati Labs



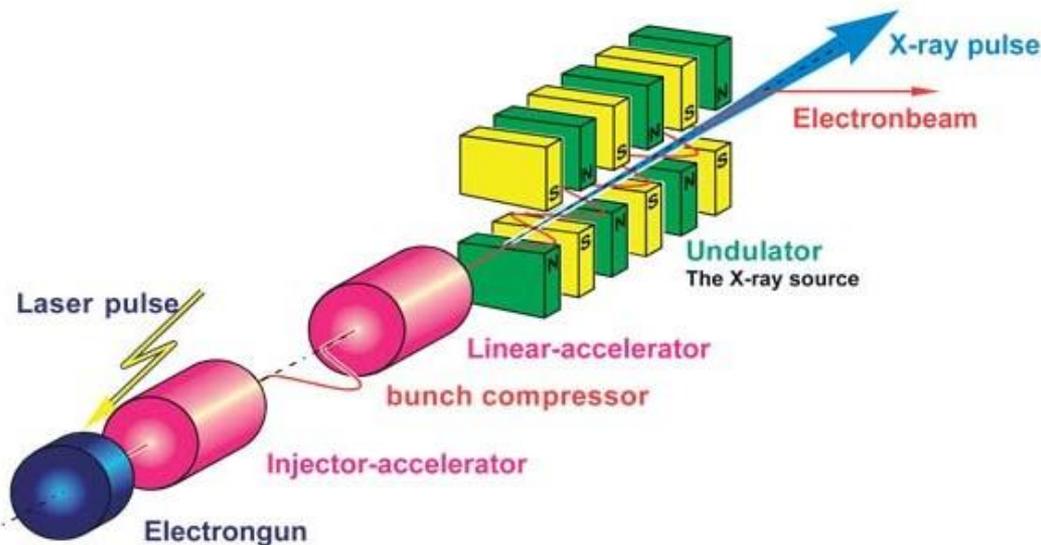
Free Electro Laser machines had a crucial role in pushing the accelerator synchronization requirements and techniques to a new frontier in the last  $\approx 15$  years.

The simplest FEL regime, the **SASE (Self-Amplified Spontaneous Emission)**, requires high-brightness bunches, being:

$$B \div \frac{I_{bunch}}{\epsilon_{\perp}^2}$$

**Large peak currents**  $I_{bunch}$  are typically obtained by **short laser pulses** illuminating a **photo-cathode** embedded in an RF Gun accelerating structure, and furtherly increased with **bunch compression** techniques.

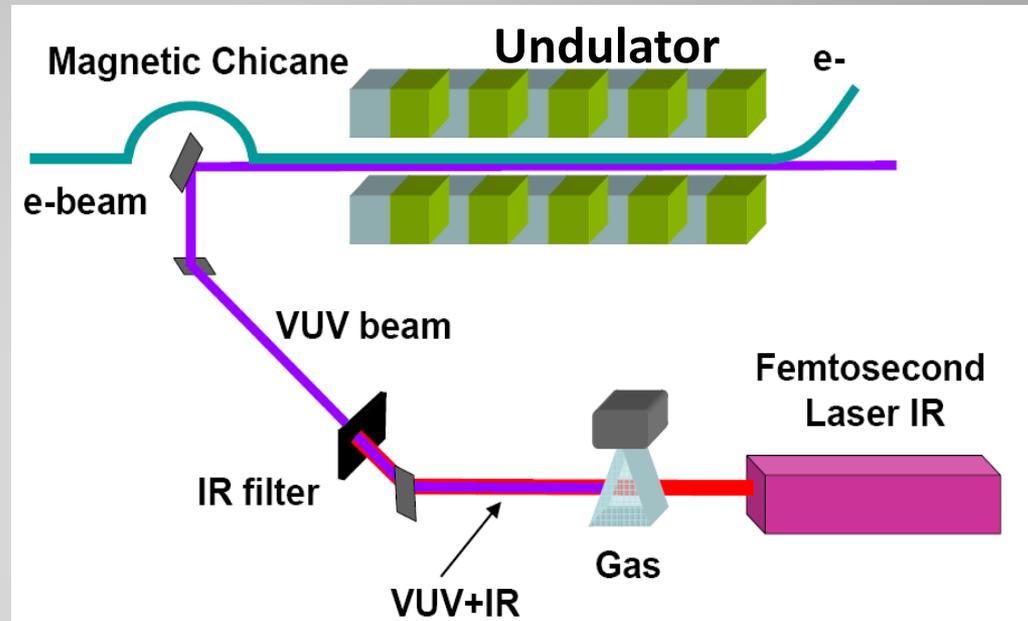
**Small transverse emittances**  $\epsilon_{\perp}$  can be obtained with **tight control** of the global machine WP, including amplitude and phase of the RF fields, magnetic focusing, laser arrival time, ...



**Global Synchronization requirements: < 500 fs rms**

In a simple SASE configuration the **micro-bunching process**, which is the base of the FEL radiation production, starts from **noise**. Characteristics such as radiation intensity and envelope profile can vary considerably from shot to shot.

A better control of the radiation properties resulting in more **uniform** and **reproducible** shot to shot pulse characteristics can be achieved in the “**seeded**” FEL configuration.



To “trigger” and guide the avalanche process generating the exponentially-growing radiation intensity, the **high brightness bunch** is made to interact with a **VUV** short and intense **pulse** obtained by HHG (High Harmonic Generation) in gas driven by an IR pulse generated by a dedicated high power laser system (typically TiSa). The presence of the external radiation since the beginning of the micro-bunching process inside the magnetic undulators seeds and drives the FEL radiation growth in a steady, repeatable configuration. The **electron bunch** and the **VUV pulse**, both **very short**, must constantly **overlap** in **space** and **time** shot to shot.

**Synchronization requirements (e- bunch vs TiSa IR pulse): < 100 fs rms**

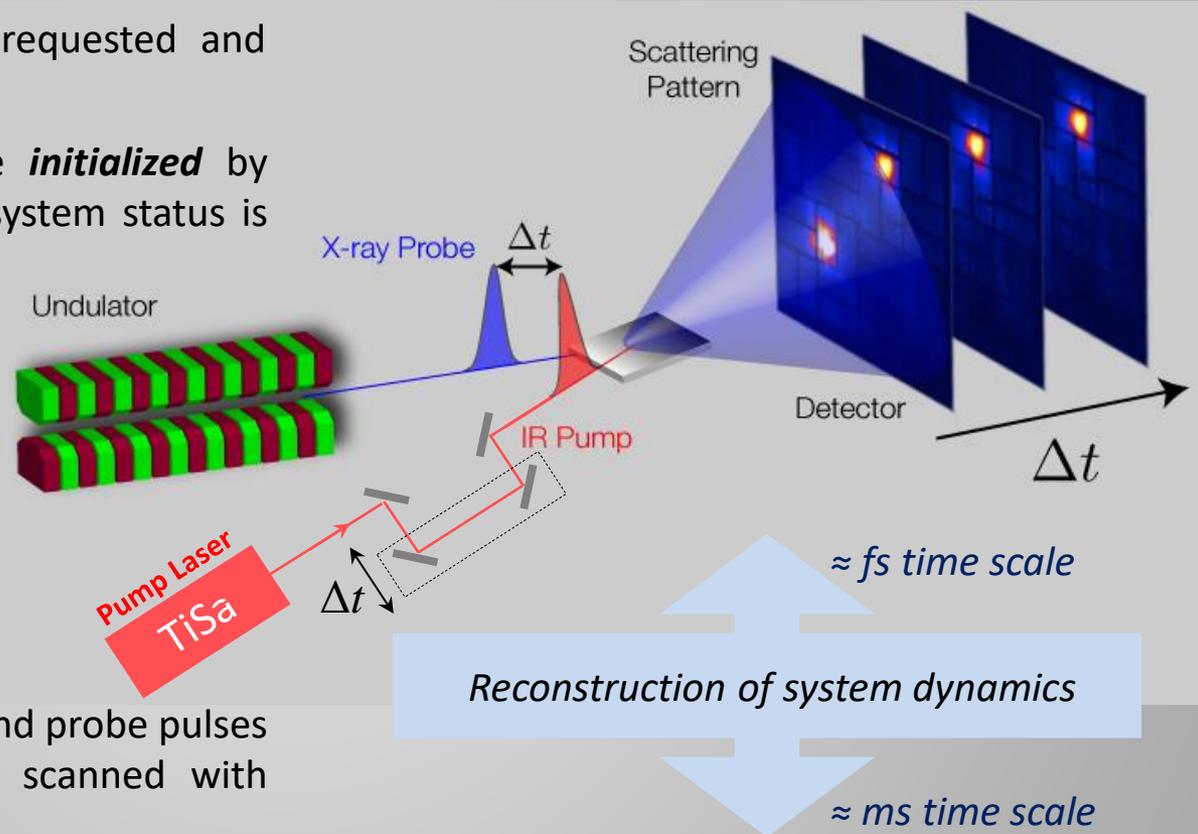
Pump-probe technique is widely requested and applied by user experimentalists.

Physical / chemical processes are **initialized** by ultra-short **laser pulses**, then the system status is **probed** by **FEL radiation**.

The dynamics of the process under study is captured and stored in a “snapshots” record.

Pump laser and FEL pulses need to be **synchronized** at level of the **time-resolution** required by the experiments (down to  $\approx 10$  fs).

The relative delay between pump and probe pulses needs to be finely and precisely scanned with proper time-resolution.

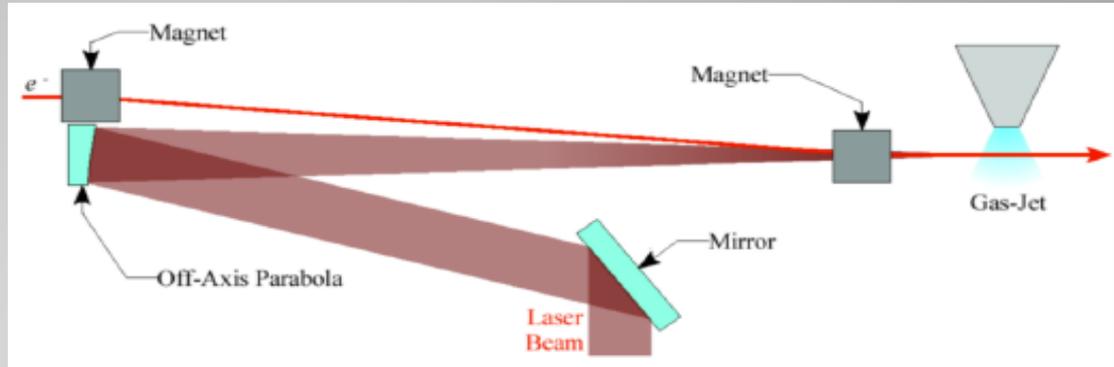


**Synchronization requirements  
(FEL vs Pump Laser pulses):  
 $\approx 10$  fs rms**



Plasma acceleration is the new frontier in accelerator physics, to overcome the gradient limits of the RF technology in the way to compact, high energy machines.

Wakefield Laser-Plasma Acceleration (WLPA) is a technique using an extremely intense laser pulse on a gas jet to generate a plasma wave with large accelerating gradients ( many GV/m).

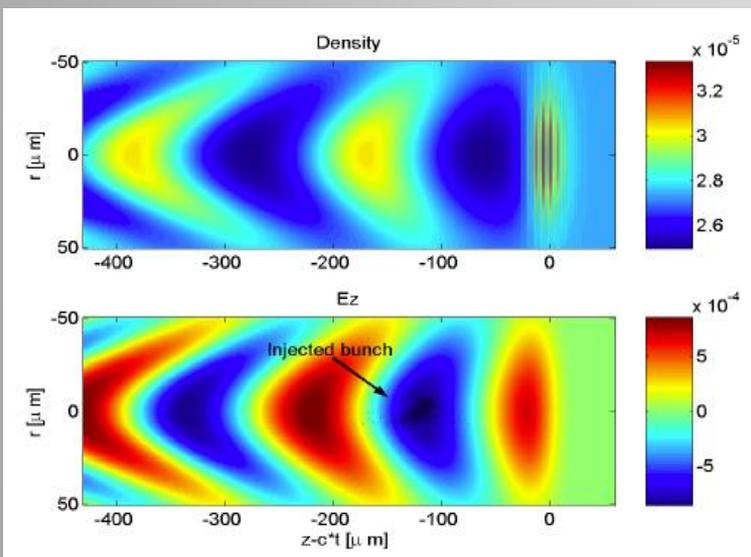


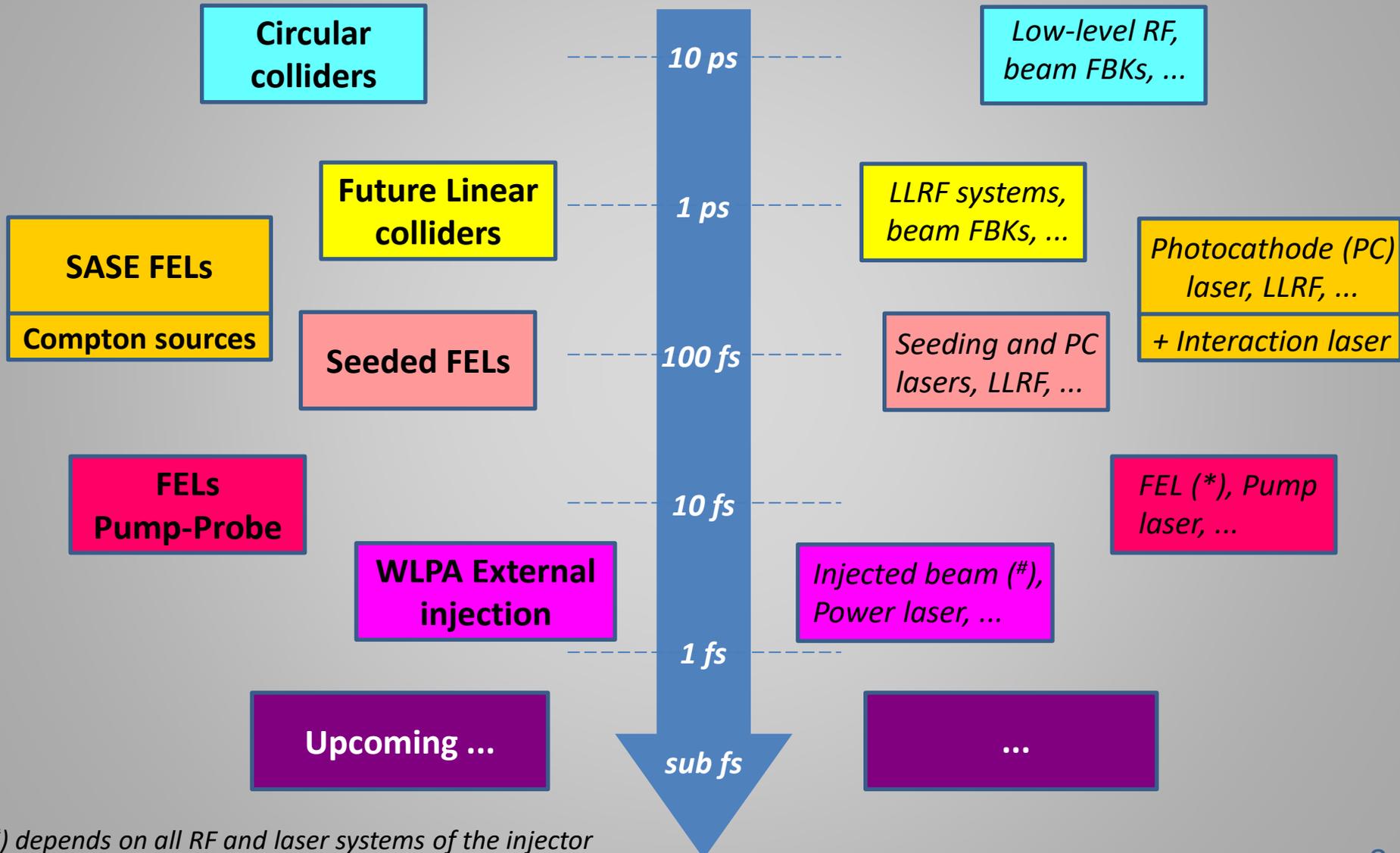
To produce good quality beams external bunches have to be injected in the plasma wave. The “accelerating buckets” in the plasma wave are typically few 100  $\mu\text{m}$  long.

The injected bunches have to be very short to limit the energy spread after acceleration, and ideally need to be injected constantly in the same position of the plasma wave to avoid shot-to-shot energy fluctuations.

This requires synchronization at the level of a small fraction of the plasma wave period.

***Synchronization requirements  
(external bunch vs laser pulse):  
< 10 fs rms***





(#) depends on all RF and laser systems of the injector

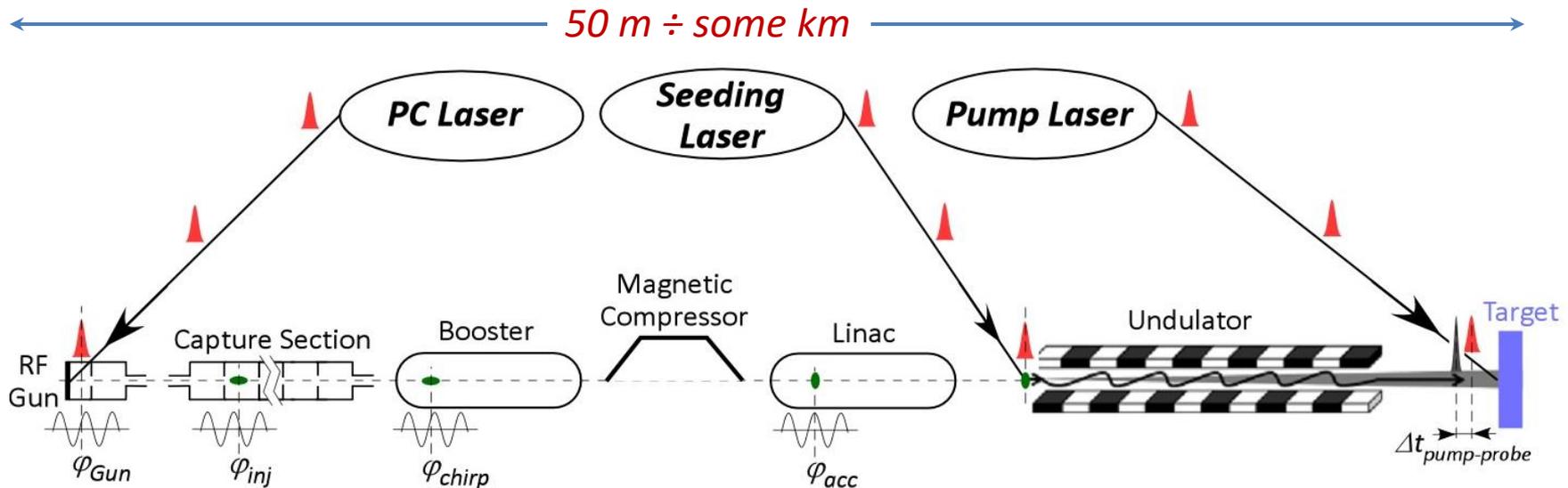
(\*) depends on beam (LLRFs + PC laser) and laser seed (if any)

# ***DEFINITIONS***

According to the previous examples, the synchronization of a facility based on a particle accelerator is a **time domain concept**.

Every accelerator is built to produce a **specific physical process** (shots of bullet particles, nuclear and sub-nuclear reactions, synchrotron radiation, FEL radiation, Compton photons, ...).

It turns out that a **necessary condition** for an efficient and reproducible event production is the **relative temporal alignment** (i.e. the **synchronization**) of **all the accelerator sub-systems** impacting the beam longitudinal phase-space and time-of-arrival (such as RF fields, PC laser system, ...), and of the **beam bunches** with **any other system they have to interact with** during and after the acceleration (such as seeding lasers, pump lasers, interaction lasers, ...).



In general the sub systems of an accelerator based facility need temporal alignments over different time scales:

- A. A fine temporal alignment, down to the fs scale, among all the relevant sub-systems presenting fundamental time structures in their internal mechanisms and in their physical outputs (main topic discussed so far).
- B. A set of digital signals – triggers - with proper relative delays to start (or enable, gate, etc. ...) a number of processes such as: firing injection/extraction kickers, RF pulse forming, switch on RF klystron HV, open/close Pockels cells in laser system, start acquisition in digitizer boards, start image acquisition with gated cameras, ... Time resolution and stability of the trigger signals is way more relaxed (< 1 ns often sufficient,  $\approx 10$  ps more than adequate)

**Synchronization**

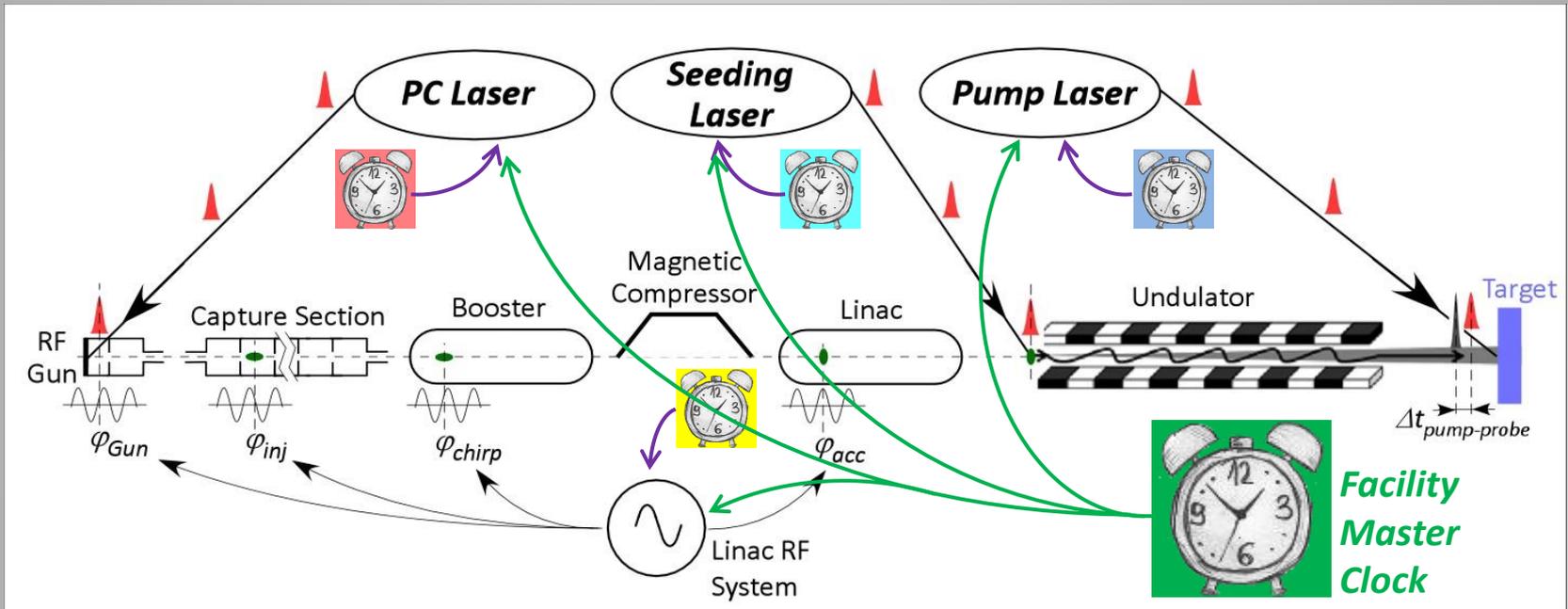
**Timing**

The task A is accomplished by the machine “**Synchronization system**”. It deals with **transporting** the **reference signal** all over the facility with constant delay and **minimal drifts**, and **locking** all the **clients** (i.e. the relevant sub-systems) to it with the **lowest residual jitter**. The main object of the present lecture is the introduction to this kind of systems.

The task B is accomplished by the machine “**Timing system**” or “**Trigger managing system**”. This is not in the femtosecond business, but it is still an interesting topic that will be covered in this lecture.

However, sometimes the words “Timing” and “Synchronization” are taken as synonyms, or used together - “Timing and Synchronization” – to indicate activities related to task A.

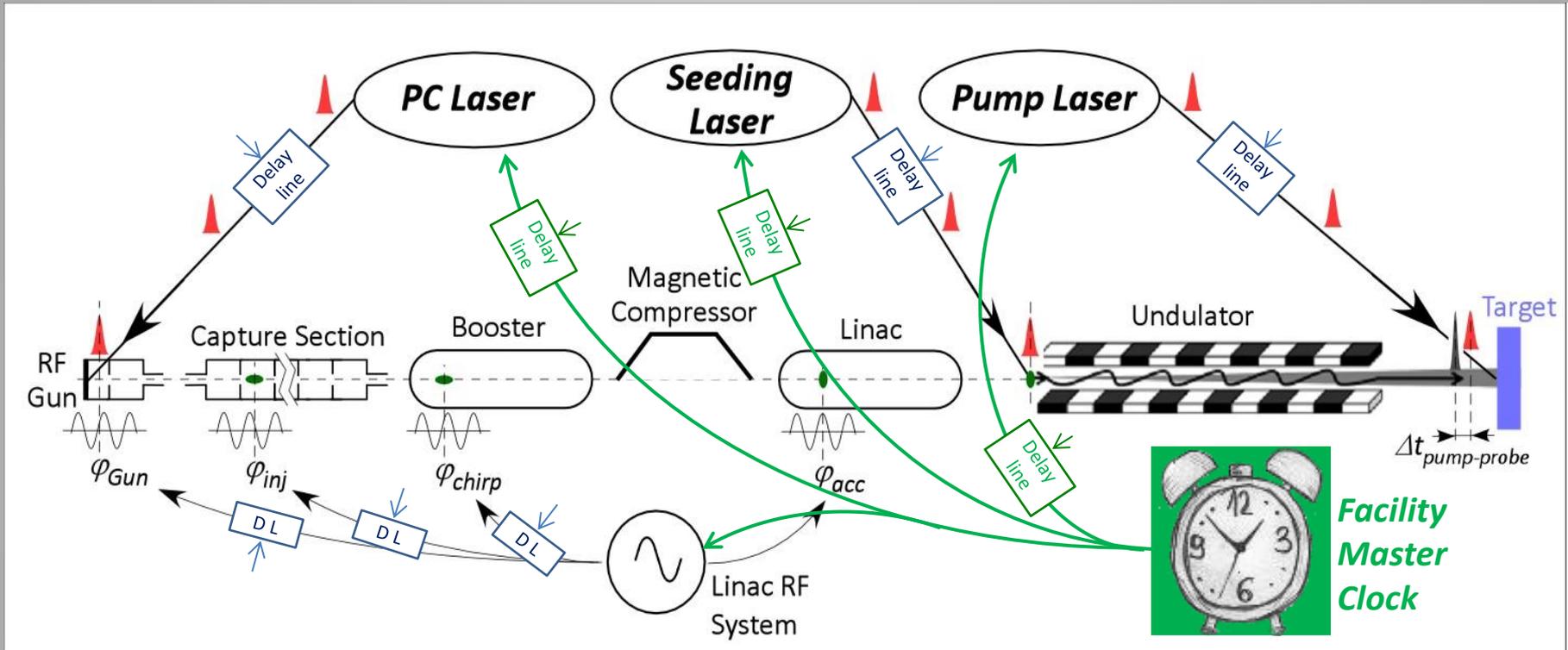
Naive approach: can each sub-system be synchronized to a local high-stability clock to have a global good synchronization of the whole facility ?



**Best optical clocks**  $\rightarrow \Delta\omega/\omega \approx 10^{-18} \rightarrow \Delta T/T \approx 10^{-18} \rightarrow T \approx 10 \text{ fs}/10^{-18} \approx \mathbf{3 \text{ hours !!!}}$

It is impossible to preserve a tight phase relation over long time scales even with the state-of-the-art technology.

All sub-systems need to be **continuously re-synchronized** by a **common master clock** that has to be distributed to the all "clients" spread over the facility with a star network architecture.



Once the local oscillators have been locked to the reference, they can be shifted in time by means of delay lines of various types – translation stages with mirrors for lasers, trombone-lines or electrical phase shifters for RF signals. This allows setting, correcting, optimizing and changing the working point of the facility synchronization.

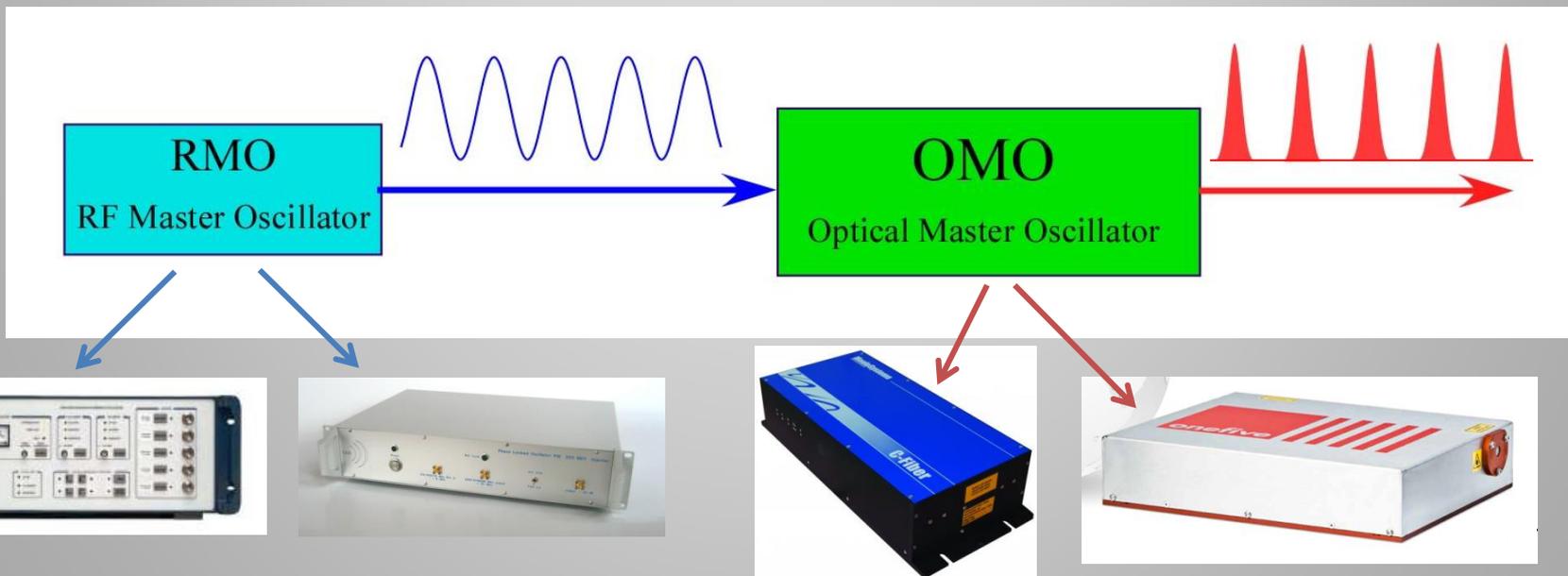
Delay lines can be placed either downstream the oscillators or on the reference signal on its path to the client oscillator. The function accomplished is exactly the same.

For simplicity, in most of the following sketches the presence of the delay line will be omitted

The **Master Oscillator** of a facility based on particle accelerators is typically a **good(\*)**, **low phase noise**  $\mu$ -wave generator acting as timing reference for the machine sub-systems. It is often indicated as the **RMO (RF Master Oscillator)**.

The timing reference signal can be distributed straightforwardly as a pure sine-wave voltage through coaxial cables, or firstly encoded in the repetition rate of a pulsed laser (or sometimes in the amplitude modulation of a CW laser), and then distributed through optical-fiber links.

**Optical fibers** provide **less signal attenuation** and **larger bandwidths**, so optical technology is definitely preferred for synchronization reference distribution, at least for large facilities.



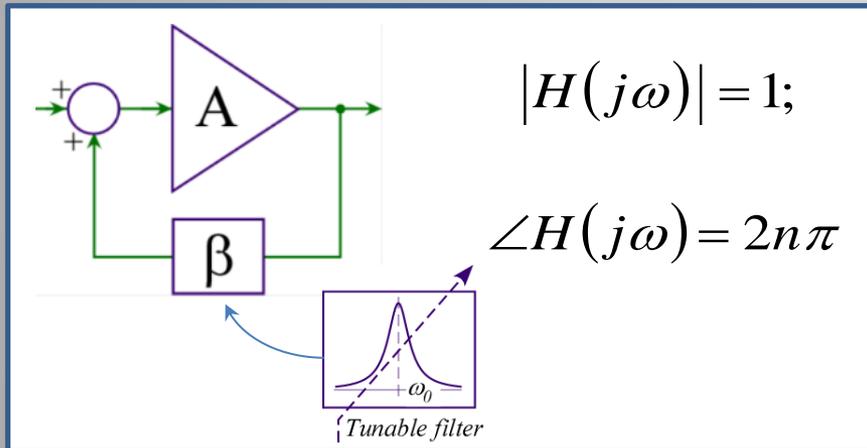
(\*) the role of the phase purity of the reference will be discussed later

## RF

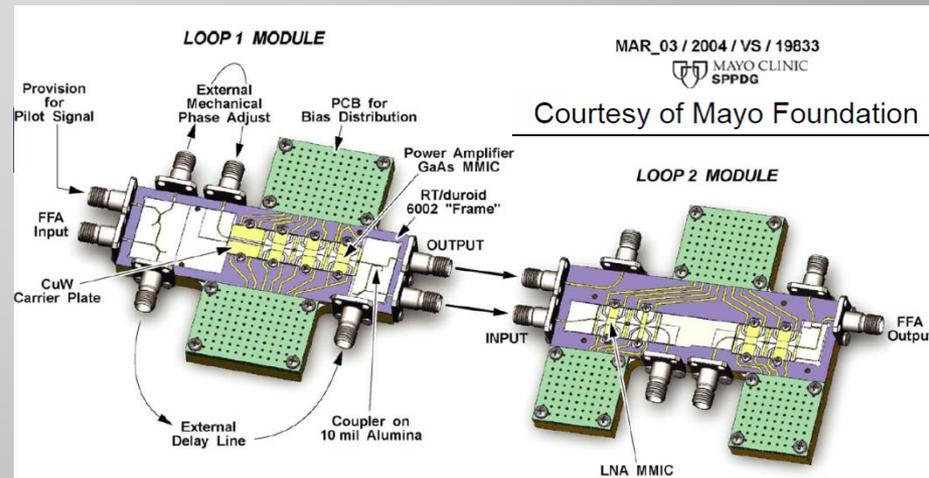
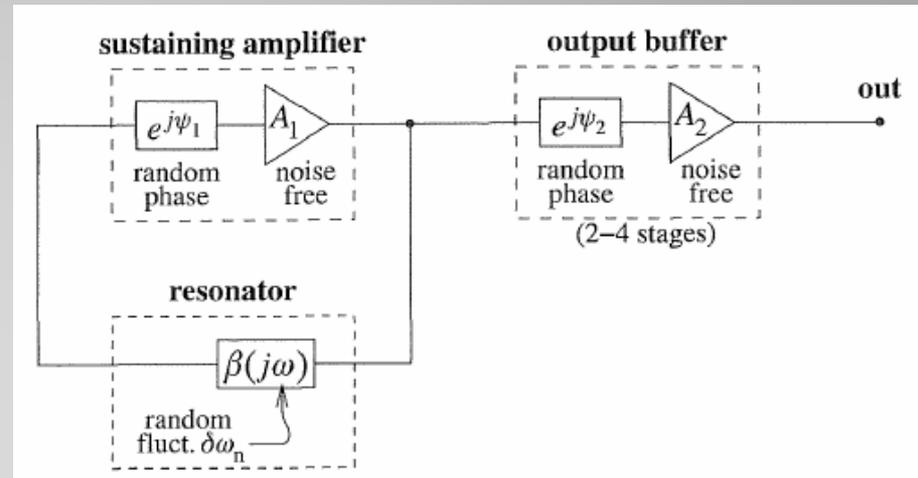
RF reference oscillator are typically based on positive-feedback network.

### Barkhausen Criterion:

Systems breaks into oscillations at frequencies where the loop gain  $H = A\beta$  is such that:



Noise present at various stages (sustaining and output amplifiers, frequency selection filter, ...) needs to be minimized by proper choice of components, layout, shielding, etc. ... Good RF oscillators may exhibit low phase noise density in the lower side of the spectrum ( $f < 1\text{kHz}$ ).

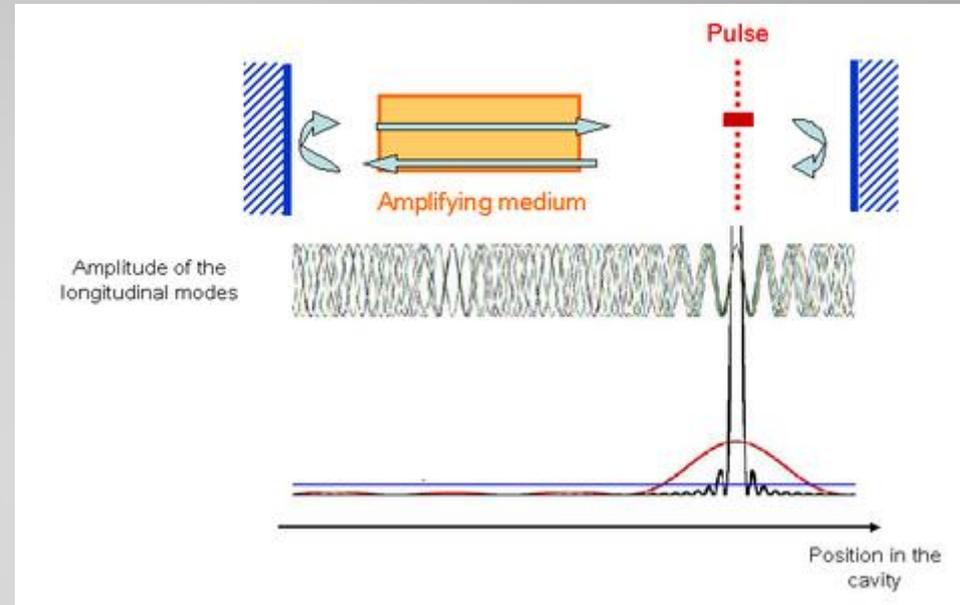


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## Optical: mode-locked lasers

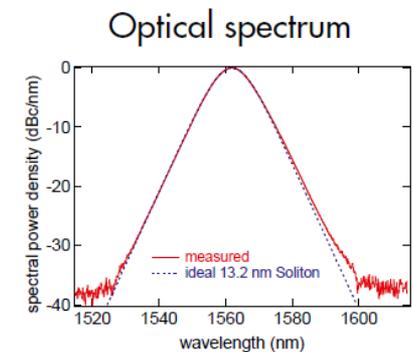
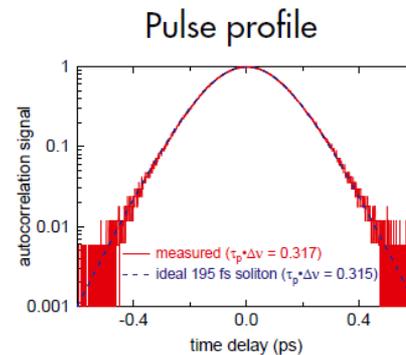
A **mode-locked laser** consists in an **optical cavity** hosting an active (amplifying) medium capable of sustaining **a large number of longitudinal modes** with frequencies  $\nu_k = k\nu_0 = kc/L$  within the bandwidth of the active medium, being  $L$  the cavity round trip length and  $k$  integer. If the modes are forced to **oscillate in phase** and the medium emission BW is wide, and a **very short pulse** ( $\approx 100$  fs) travels forth and back in the cavity and a sample is coupled out through a leaking mirror.



## Origami

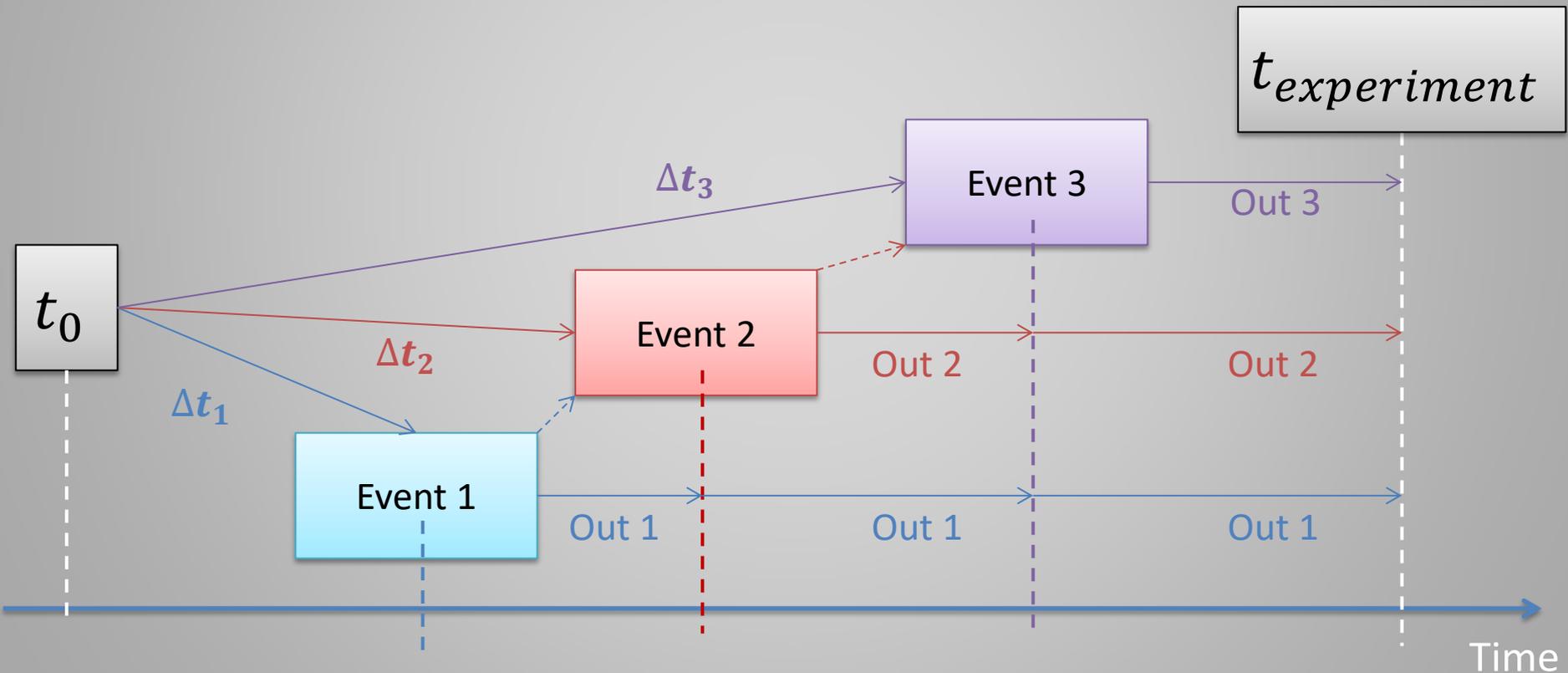


Laser specifications	Origami-05	Origami-08	Origami-10	Origami-15
Center wavelength	513 – 535 nm	765 – 785 nm	1025 – 1070 nm	1530 – 1586 nm
Pulse Duration <sup>1,2</sup>	<100 – 230 fs	<60 – 200 fs	<70 – 400 fs	<80 – 500 fs
Avg. output power (up to) <sup>2</sup>	100 mW	30 mW	250 mW	120 mW
Pulse energy (up to) <sup>2</sup>	1.2 nJ	0.7 nJ	5 nJ	2 nJ
Peak power (up to) <sup>2</sup>	10 kW	4.5 kW	30 kW	15 kW
Pulse repetition rate <sup>2</sup>	20 MHz – 1.3 GHz			
Spectral bandwidth	transform-limited ( $\tau_p \cdot \Delta\nu \sim 0.32$ ) $\rightarrow 1/\pi$			
Beam quality	$M^2 < 1.1$ , TEM <sub>00</sub>			
PER	> 23 dB			
Amplitude noise (24 h)	< 0.2% rms, < 0.5% pk-pk			
Center wavelength drift	< 0.1 nm pk-pk			
Laser output	collimated free space (fiber output optional)			



<http://www.onefive.com/ds/Datasheet%20Origami%20LP.pdf>

Once all the physical outputs of sub-systems are made coherent, the **timing system** decides the chain of events that are necessary to realize an experiment.



The synchronization error of a client with respect to the reference is identified as **jitter** or **drift** depending on the **time scale** of the involved phenomena.

**Jitter** = fast variations, caused by inherent residual lack of coherency between oscillators, even if they are locked at the best;

**Drift** = slow variations, mainly caused by modifications of the environment conditions, such as temperature (primarily) but also humidity, materials and components aging, ...

The boundary between the 2 categories is somehow arbitrary. For instance, synchronization errors due to mechanical vibrations can be classified in either category:

Acoustic waves → Jitter

Infrasounds → Drift

For pulsed accelerators, where the beam is produced in the form of a sequence of bunch trains with a certain repetition rate (10 Hz ÷ 120 Hz typically), the **rep. rate value** itself can be taken as a reasonable definition of the **boundary** between **jitters** and **drifts**.

In this respect, **drifts** are phenomena significantly **slower** than **rep. rate** and will produced effects on the beam that can be **monitored** and **corrected** pulse-to-pulse.

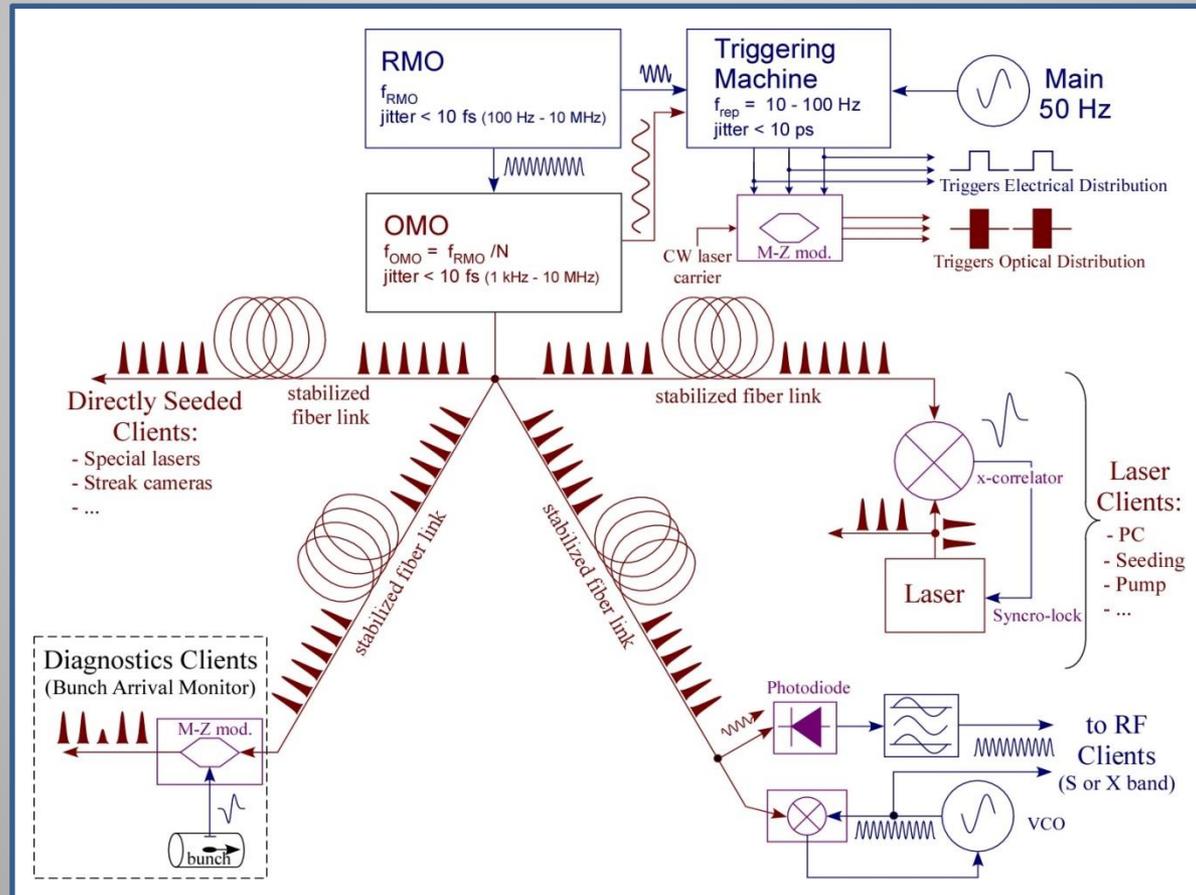
On the contrary, **jitters** are **faster** than **rep. rate** and will result in a pulse-to-pulse **chaotic scatter** of the beam characteristics that has to be minimized but that **can not** be actively **corrected**.

Drift → Nasty

Jitter → Killer

## Tasks of a Synchronization system:

- ✓ Generate and transport the reference signal to any client local position with constant delay and minimal drifts;
- ✓ Lock the client (laser, RF, ...) fundamental frequency to the reference with minimal residual jitter;
- ✓ Monitor clients and beam, and apply delay corrections to compensate residual drifts.



# ***BASICS***

- ***Fourier and Laplace Transforms***
- ***Random Processes***
- ***Phase Noise in Oscillators***

## Transforms summary

Transforms	Fourier - $\mathcal{F}$	Laplace - $\mathcal{L}$
Definition	$X(j\omega) = \int_{-\infty}^{+\infty} x(t) e^{-j\omega t} dt$	$X(s) = \int_0^{+\infty} x(t) e^{-st} dt$
Inverse transform	$x(t) = \frac{1}{2\pi} \int_{-\infty}^{+\infty} X(j\omega) e^{j\omega t} d\omega$	$x(t) = \frac{1}{2\pi i} \int_{\gamma-j\cdot\infty}^{\gamma+j\cdot\infty} X(s) e^{st} ds$
Transformability conditions	$\int_{-\infty}^{+\infty}  x(t) ^2 dt \neq \infty$	$x(t) = 0 \text{ if } t < 0; \quad x(t) \cdot e^{-\sigma t} \xrightarrow{t \rightarrow +\infty} 0$
Linearity	$\mathcal{F} [a x(t) + b y(t)] = aX(\omega) + bY(\omega)$	$\mathcal{L} [a x(t) + b y(t)] = aX(s) + bY(s)$
Convolution product	$(x * y)(t) \stackrel{\text{def}}{=} \int_{-\infty}^{+\infty} x(t + \tau) \cdot y(\tau) d\tau$ $\mathcal{F} [(x * y)(t)] = X^*(\omega) \cdot Y(\omega)$	$(x * y)(t) \stackrel{\text{def}}{=} \int_0^t x(t + \tau) \cdot y(\tau) d\tau$ $\mathcal{L} [(x * y)(t)] = X^*(s) \cdot Y(s)$
Derivative	$\mathcal{F} \left[ \frac{dx}{dt} \right] = j\omega \cdot X(\omega)$	$\mathcal{L} \left[ \frac{dx}{dt} \right] = s \cdot X(s)$
Delay	$\mathcal{F} [x(t - \tau)] = X(\omega) e^{-j\omega\tau}$	$\mathcal{L} [x(t - \tau)] = X(s) e^{-s\tau}$

## Random process summary

- Stationary process: statistical properties invariant for a  $t'$  time shift  $x(t) \rightarrow x(t + t')$
- Ergodic process: statistical properties can be estimated by a single process realization
- Uncorrelation: if  $x(t)$  and  $y(t)$  are 2 random variables completely uncorrelated (statistically independent), then:

$$\sigma_{x+y}^2 = \sigma_x^2 + \sigma_y^2 \quad \text{with} \quad \sigma_x^2 \stackrel{\text{def}}{=} \overline{x^2} - \bar{x}^2$$

### Power spectrum:

rms and standard deviation of a random variable  $x(t)$  can be computed on the basis of its Fourier transform. Strictly speaking, a function of time  $x(t)$  with  $x_{rms} \neq 0$  cannot be Fourier transformed since it does not satisfy the transformability necessary condition.

$$\int_{-\infty}^{+\infty} |x(t)|^2 dt = A \neq \infty \quad \xrightarrow{\text{would imply}} \quad x_{rms}^2 = \lim_{T \rightarrow \infty} \frac{1}{T} \int_{-T/2}^{+T/2} |x(t)|^2 dt = 0$$

If  $x(t)$  represents a current or a voltage signal, it can be Fourier transformed provided that it carries a **finite quantity of energy**. But we might be interested in treating random (noise) signals characterized by a **non-zero average power** ( $x_{rms}^2 \neq 0$ ) carrying an unlimited amount of energy.

## Random process summary

However, for practical reasons, we are only interested in observations of the random variable  $x(t)$  for a **finite time**  $\Delta T$ . So we may truncate the function outside the interval  $[-\Delta T/2, \Delta T/2]$  and remove any possible limitation in the function transformability. We also assume  $x(t)$  real.

$$x_{\Delta T}(t) = \begin{cases} x(t) & -\Delta T/2 \leq t \leq \Delta T/2 \\ 0 & \text{elsewhere} \end{cases}$$

The truncated function  $x_{\Delta T}(t)$  is Fourier transformable. Let  $X_{\Delta T}(f)$  be its Fourier transform. We have:

$$x_{rms}^2 = \lim_{\Delta T \rightarrow \infty} x_{\Delta T, rms}^2 = \lim_{\Delta T \rightarrow \infty} \frac{1}{\Delta T} \int_{-\infty}^{+\infty} x_{\Delta T}^2(t) dt \stackrel{\text{Parseval's theorem}}{=} \lim_{\Delta T \rightarrow \infty} \frac{1}{\Delta T} \int_{-\infty}^{+\infty} |X_{\Delta T}(f)|^2 df \stackrel{\text{def}}{=} \int_0^{+\infty} S_x(f) df$$

with  $S_x(f) \stackrel{\text{def}}{=} \lim_{\Delta T \rightarrow \infty} 2 \cdot \frac{|X_{\Delta T}(f)|^2}{\Delta T}$

The function  $S_x(f)$  is called “**power spectrum**” or “**power spectral density**” of the random variable  $x(t)$ . The time duration of the variable observation  $\Delta T$  sets the minimum frequency  $f_{min} \approx 1/\Delta T$  containing meaningful information in the spectrum of  $x_{\Delta T}(t)$ .

## Random process summary

**Important to underline!** If  $x(t)$  is a stationary process, we can consider different observations of duration  $\Delta T$  centered at different times  $k\Delta T$  ( $k$  any integer):

$$x_{k\Delta T}(t) = \begin{cases} x(t) & k\Delta T - \frac{\Delta T}{2} \leq t \leq k\Delta T + \Delta T/2 \\ 0 & \text{elsewhere} \end{cases}$$

And if  $x(t)$  is ergodic too, we may consider different realizations  $x_i(t)$  of the process, and observe them in slices of duration  $\Delta T$ :

$$x_{i,k\Delta T}(t) = \begin{cases} x_i(t) & k\Delta T - \frac{\Delta T}{2} \leq t \leq k\Delta T + \Delta T/2 \\ 0 & \text{elsewhere} \end{cases}$$

The functions  $x_{i,k\Delta T}(t)$  are all different, but statistically equivalent, in the sense that statistical properties of the process  $x(t)$  (including  $x_{rms}$  and  $\sigma_x$ ) can be extracted from each of them.

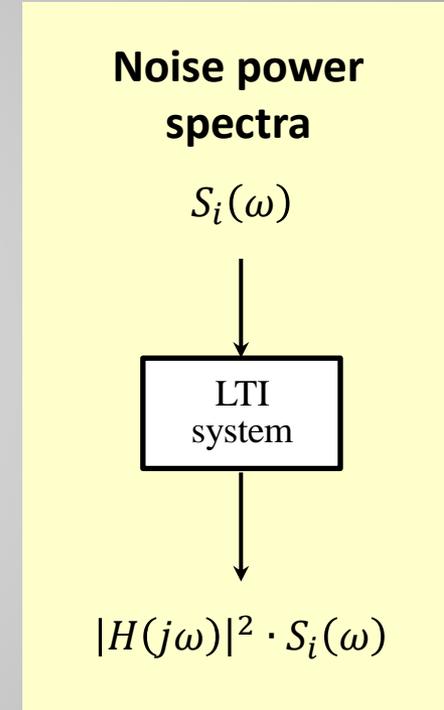
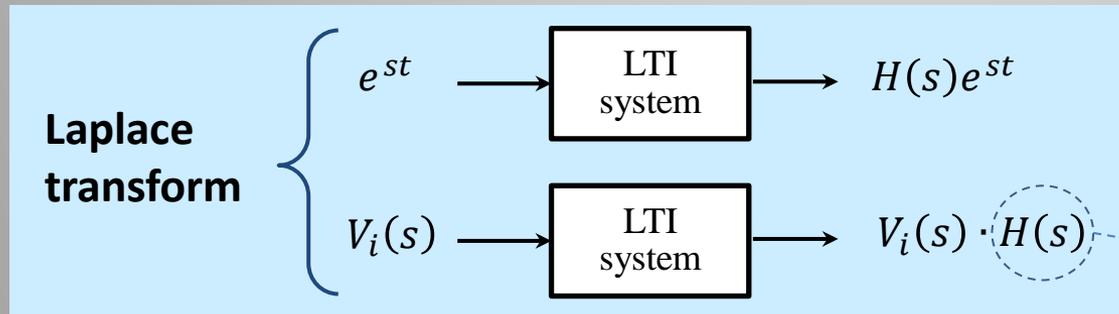
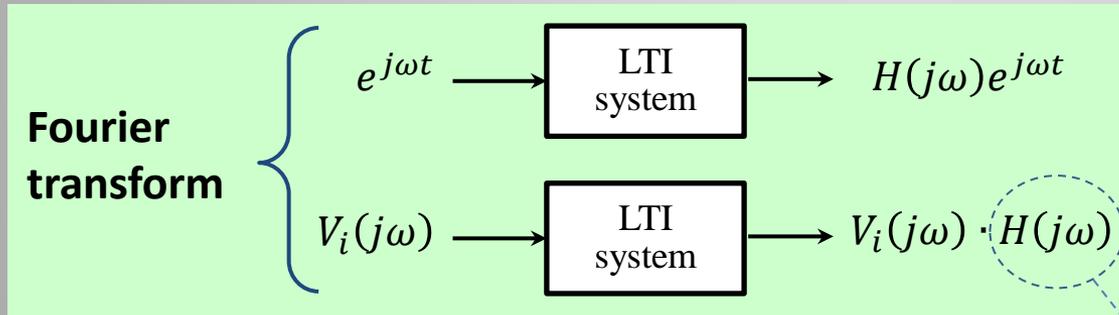
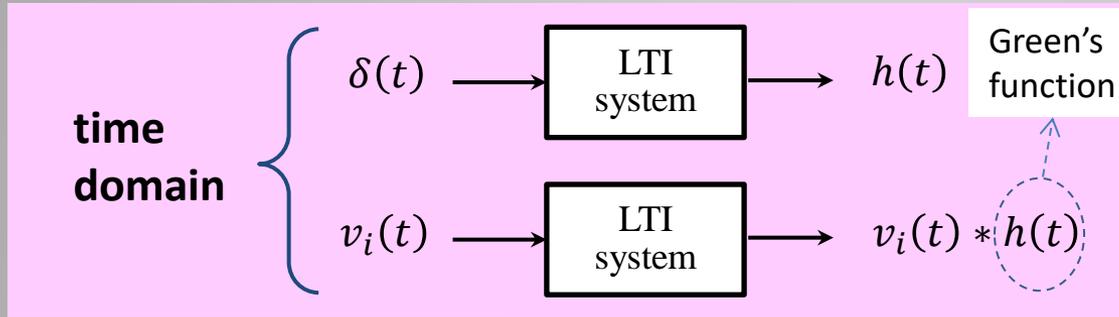
This means  $|X_{i,k\Delta T}(\omega)| = |X_{\Delta T}(\omega)|$  independently on the observed realization and temporal slice.

**The module of the Fourier transform of all  $x_{i,k\Delta T}(t)$  functions is the same.** So, in what they differ?

As matter of fact, they only differ in the phase  $\Phi_{i,k\Delta T}(\omega) = \text{Arg}[X_{i,k\Delta T}(\omega)]$  of they Fourier transform:

$$\mathcal{F}[x_{i,k\Delta T}(t)] = |X_{\Delta T}(\omega)| \cdot e^{j\Phi_{i,k\Delta T}(\omega)}$$

Fourier and Laplace transforms are used to compute the response of **Linear Time Invariant (LTI)** systems:

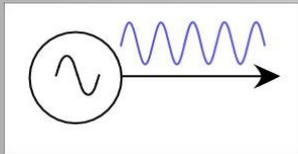


LTI system  
Transfer functions

The most important task of a Synchronization system is to **lock firmly** each **client** to the **reference** in order to minimize the residual jitter. In fact each client can be described as a local oscillator (electrical for RF systems, optical for laser systems) whose main frequency can be changed by applying a voltage to a control port.

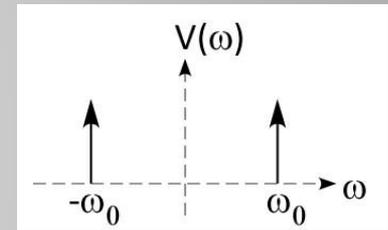
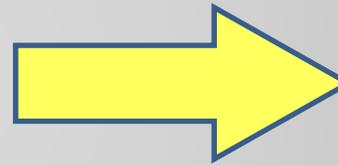
Before discussing the lock schematics and performances, it is worth introducing some **basic concepts** on **phase noise in real oscillators**.

## Ideal oscillator

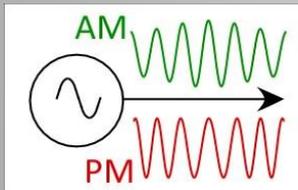


$$V(t) = V_0 \cdot \cos(\omega_0 t + \varphi_0)$$

## Ideal Spectrum

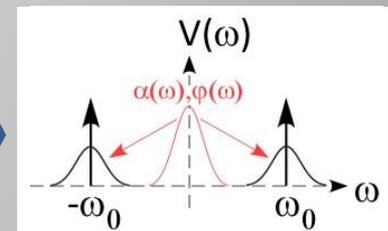


## Real oscillator



$$V(t) = V_0 \cdot [1 + \alpha(t)] \cdot \cos[\omega_0 t + \varphi(t)]$$

## Real Spectrum



In real oscillators the amplitude and phase will always fluctuate in time by a certain amount because of the unavoidable presence of noise. However, by common sense, a well behaving real oscillator has to satisfy the following conditions:

$$|\alpha(t)| \ll 1; \quad \left| \frac{d\varphi}{dt} \right| \ll \omega_0$$

A real oscillator signal can be also represented in **Cartesian Coordinates**  $(\alpha, \varphi) \rightarrow (v_I, v_Q)$ :

$$V(t) = V_0 \cdot \cos(\omega_0 t) + v_I(t) \cdot \cos(\omega_0 t) - v_Q(t) \cdot \sin(\omega_0 t)$$

if  $v_I(t), v_Q(t) \ll V_0$   $\rightarrow$   $\alpha(t) = v_I(t)/V_0, \quad \varphi(t) = v_Q(t)/V_0 \ll 1$

*Cartesian representation only holds for small PM depth*

Real oscillator outputs are **amplitude (AM)** and **phase (PM) modulated** carrier signals. In general it turns out that **close to the carrier** frequency the contribution of the **PM noise** to the signal spectrum **dominates** the contribution of the **AM noise**. For this reason the lecture will be focused on phase noise. However, amplitude noise in RF systems directly reflects in energy modulation of the bunches, that may cause bunch arrival time jitter when beam travels through dispersive and bended paths (i.e. when  $R_{56} \neq 0$  as in magnetic chicanes).

Let's consider a real oscillator and neglect the AM component:

$$V(t) = V_0 \cdot \cos[\omega_0 t + \varphi(t)] = V_0 \cdot \cos[\omega_0(t + \tau(t))] \quad \text{with} \quad \tau(t) \equiv \varphi(t)/\omega_0$$

The statistical properties of  $\varphi(t)$  and  $\tau(t)$  qualify the oscillator, primarily the values of the standard deviations  $\sigma_\varphi$  and  $\sigma_\tau$  (or equivalently  $\varphi_{rms}$  and  $\tau_{rms}$  since we may assume a zero average value). As for every noise phenomena they can be computed through the **phase noise power spectral density**  $S_\varphi(f)$  of the random variable  $\varphi(t)$ .

Again, for practical reasons, we are only interested in observations of the random variable  $\varphi(t)$  for a finite time  $\Delta T$ . So we may truncate the function outside the interval  $[-\Delta T/2, \Delta T/2]$  to recover the function transformability.

$$\varphi_{\Delta T}(t) = \begin{cases} \varphi(t) & -\Delta T/2 \leq t \leq \Delta T/2 \\ 0 & \text{elsewhere} \end{cases}$$

Let  $\Phi_{\Delta T}(f)$  be the Fourier transform of the truncated function  $\varphi_{\Delta T}(t)$ . We have:

$$\varphi_{\Delta T rms}^2 = \frac{1}{\Delta T} \int_{-\infty}^{+\infty} \varphi_{\Delta T}^2(t) dt = \frac{1}{\Delta T} \int_{-\infty}^{+\infty} |\Phi_{\Delta T}(f)|^2 df = \int_{f_{min}}^{+\infty} S_{\varphi}(f) df \text{ with } S_{\varphi}(f) \stackrel{\text{def}}{=} 2 \frac{|\Phi_{\Delta T}(f)|^2}{\Delta T}$$

$S_{\varphi}(f)$  is the **phase noise power spectral density**, whose dimensions are  $rad^2/Hz$ .

Again, the time duration of the variable observation  $\Delta T$  sets the minimum frequency  $f_{min} \approx 1/\Delta T$  containing meaningful information on the spectrum  $\Phi_{\Delta T}(f)$  of the phase noise  $\varphi_{\Delta T}(t)$ .

**IMPORTANT:**

we might still write

$$\varphi_{rms}^2 = \lim_{\Delta T \rightarrow \infty} \varphi_{\Delta T rms}^2 = \int_0^{+\infty} \left( 2 \cdot \lim_{\Delta T \rightarrow \infty} \frac{|\Phi_{\Delta T}(f)|^2}{\Delta T} \right) df = \int_0^{+\infty} S_{\varphi}(f) df$$

but we must be aware that  $\varphi_{rms}$  in some case **might diverge**. This is physically possible since the **power** in the carrier does only **depend** on **amplitude** and **not** on **phase**. In these cases the rms value can only be specified for a given observation time  $\Delta T$  or equivalently for a frequency range of integration  $[f_1, f_2]$ .

We have:

$$\varphi_{rms}^2 \Big|_{\Delta T} = 2 \cdot \int_{f_{min}}^{+\infty} \mathcal{L}(f) df \quad \text{with} \quad \mathcal{L}(f) = \begin{cases} \frac{|\Phi_{\Delta T}(f)|^2}{\Delta T} & f \geq 0 \\ 0 & f < 0 \end{cases}$$

The function  $\mathcal{L}(f)$  is defined as the “Single Sideband Power Spectral Density” and is called “script-L”

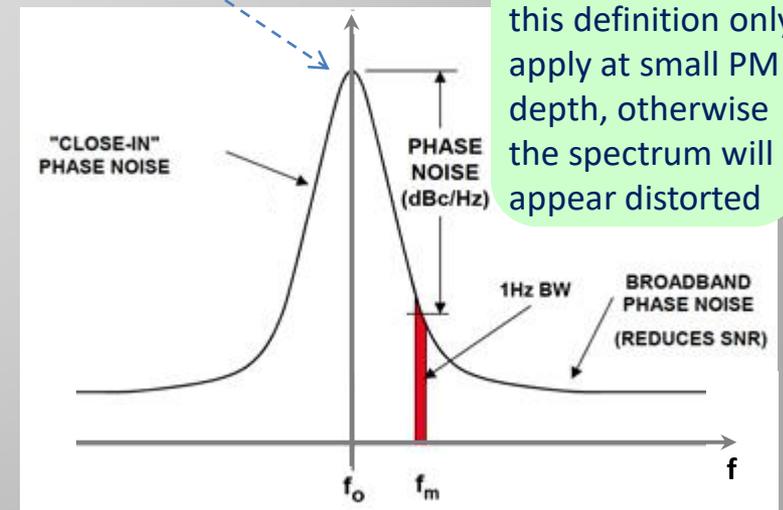
$$\mathcal{L}(f) = \frac{\text{power in 1 Hz phase modulation single sideband}}{\text{total signal power}} = \frac{1}{2} S_{\varphi}(f) \leftarrow \text{IEEE standard 1139 – 1999}$$

Linear scale  $\rightarrow \mathcal{L}(f)$  units  $\equiv \text{Hz}^{-1}$  or  $\text{rad}^2/\text{Hz}$

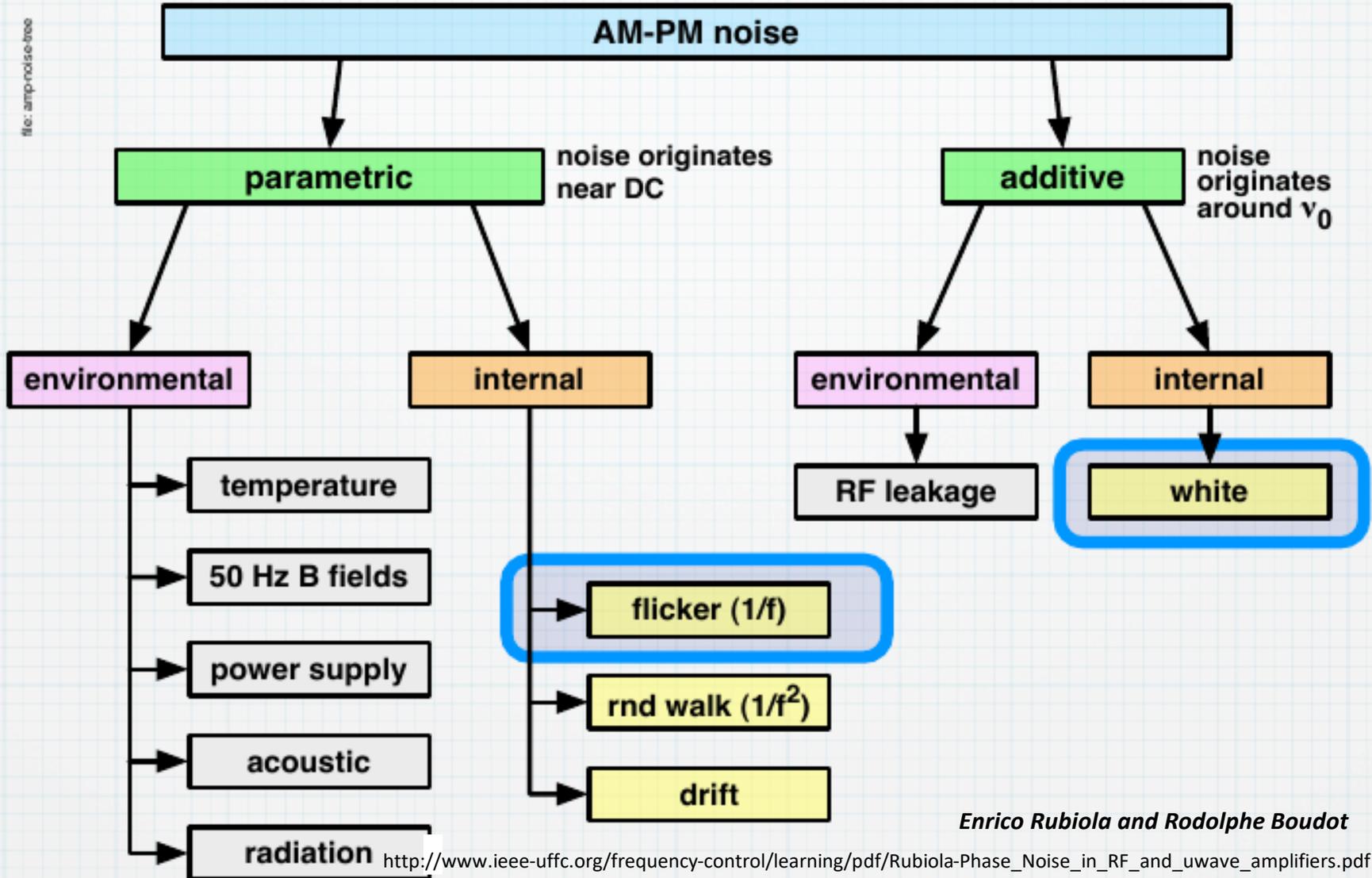
Log scale  $\rightarrow 10 \cdot \text{Log}[\mathcal{L}(f)]$  units  $\equiv \text{dBc}/\text{Hz}$

## CONCLUSIONS:

- ✓ Phase (and time) jitters can be computed from the spectrum of  $\varphi(t)$  through the  $\mathcal{L}(f)$  - or  $S_{\varphi}(f)$  - function;
- ✓ Computed values depend on the integration range, i.e. on the duration  $\Delta T$  of the observation. Criteria are needed for a proper choice (we will see ...).

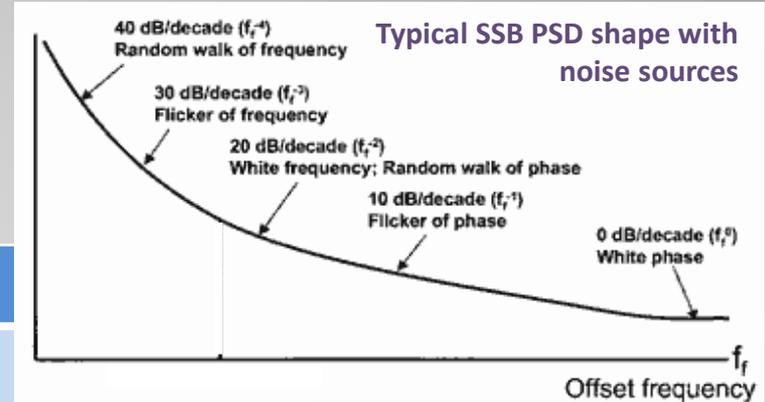


**Attention:**  
this definition only apply at small PM depth, otherwise the spectrum will appear distorted



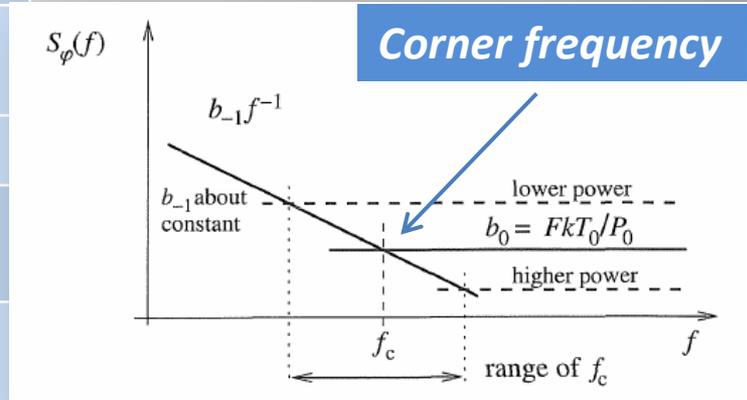
**Close-in phase noise:**  $S_{\varphi}(f) = \sum \frac{b_{-k}}{f^k} \quad k = 0,1,2,3, \dots$

$S_{FM}(f) \xrightarrow{\text{F or L transforms}} S_{PM}(f) = S_{FM}(f)/f^2$



	Type	Origin	$S_{\varphi}(f)$
$f^0$	White	Thermal noise of resistors	$(F) \cdot kT/P_0$
	Shot	Current quantization	$2q\bar{i}R/P_0$
$f^{-1}$	Flicker	Flicking PM	$b_{-1}/f$
$f^{-2}$	White FM	Thermal FM noise	$b_0^{FM} \cdot \frac{1}{f^2}$
	Random walk	Brownian motion	$b_{-2}/f^2$
$f^{-3}$	Flicker FM	Flicking FM	$\frac{b_{-1}^{FM}}{f} \cdot \frac{1}{f^2}$
$f^{-4}$	Random walk FM	Brownian motion $\rightarrow$ FM	$\frac{b_{-2}^{FM}}{f^2} \cdot \frac{1}{f^2}$
$f^{-n}$	...	high orders ...	

$F \stackrel{\text{def}}{=} SNR_{in}/SNR_{out}$



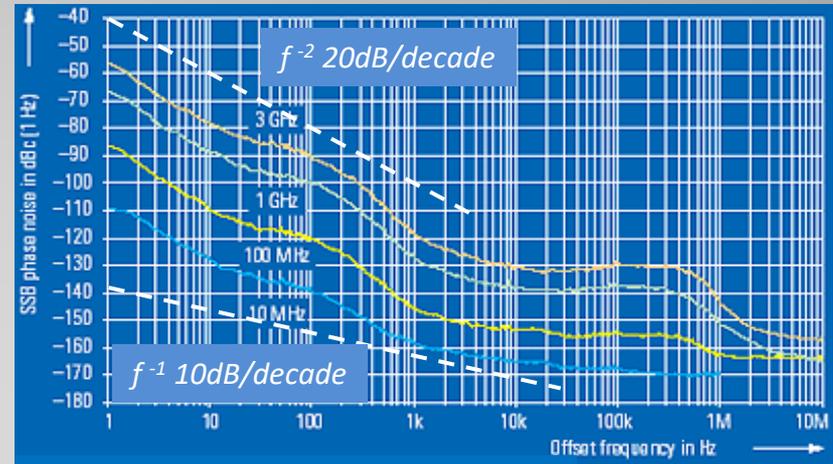
$[b_{-k}] = \text{rad}^2 \text{Hz}^{k-1}$

Time jitter can be computed according to:

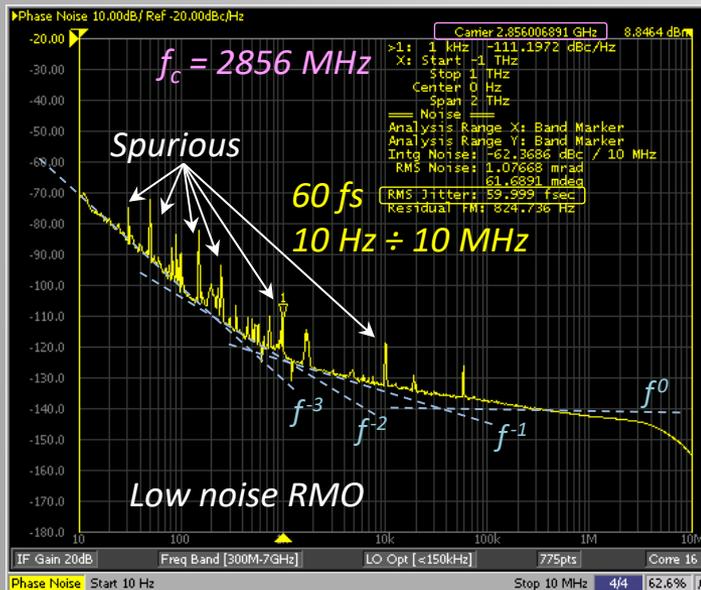
$$\sigma_t^2 = \frac{\varphi_{rms}^2}{\omega_c^2} = \frac{1}{\omega_c^2} \int_{f_{min}}^{+\infty} S_\varphi(f) df$$

same time jitter  $\rightarrow S_\varphi(f) \div \omega_c^2$

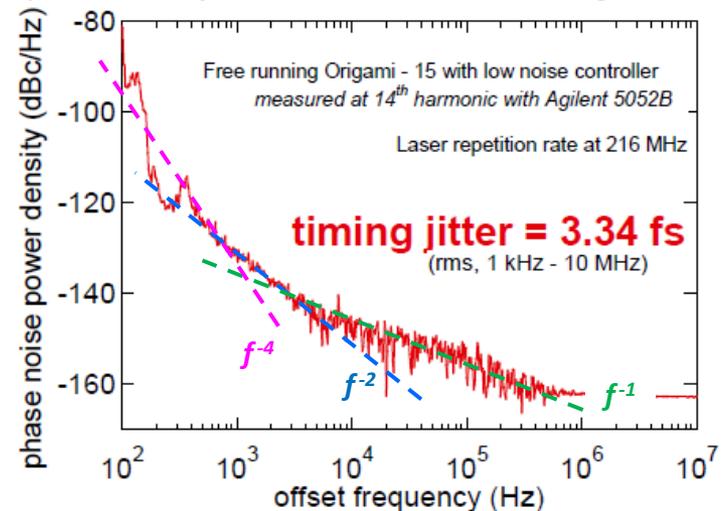
Phase noise spectral densities of different oscillators have to be compared at same carrier frequency  $\omega_c$  or scaled as  $\omega_c^{-2}$  before comparison.



Commercial frequency synthesizer



<http://www.onefive.com/ds/Datasheet%20Origami%20LP.pdf>



OMO – Mode-locked laser –  $f = 3024$  MHz

***GO TO  
EXERCISE #1***

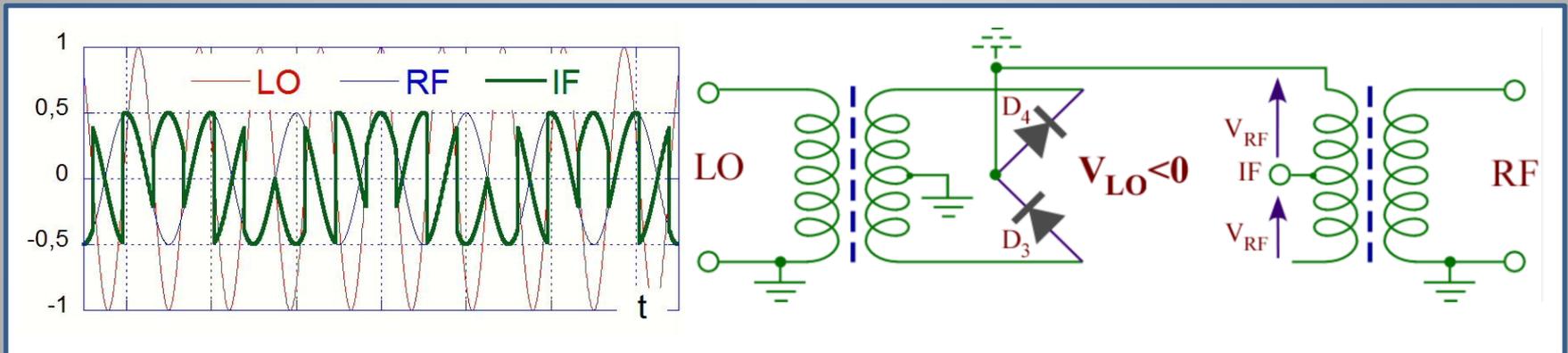
# ***BASICS***

- ***Phase Detectors***
- ***Phase Locked Loops***

## Phase detection on RF signals

The **Double Balanced Mixer** is the **most diffused RF device** for frequency translation (up/down conversion) and detection of the relative phase between 2 RF signals (LO and RF ports). The LO voltage is differentially applied on a diode bridge switching on/off alternatively the  $D_1$ - $D_2$  and  $D_3$ - $D_4$  pairs, so that the voltage at IF is:

$$V_{IF}(t) = V_{RF}(t) \cdot \text{sgn}[V_{LO}(t)]$$



$$V_{RF}(t) = V_{RF} \cdot \cos(\omega_{RF}t); \quad V_{LO}(t) = V_{LO} \cdot \cos(\omega_{LO}t)$$

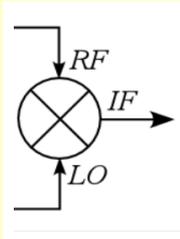
$$V_{RF} \ll V_{LO}$$

$$\begin{aligned} V_{IF}(t) &= V_{RF} \cos(\omega_{RF}t) \cdot \text{sgn}[\cos(\omega_{LO}t)] = V_{RF} \cos(\omega_{RF}t) \cdot \sum_{n=\text{odds}} \frac{4}{n\pi} \cos(n\omega_{LO}t) = \\ &= \frac{2}{\pi} V_{RF} [\cos((\omega_{LO} - \omega_{RF})t) + \cos((\omega_{LO} + \omega_{RF})t) + \text{intermod products}] \end{aligned}$$

## Phase detection on RF signals

If  $f_{LO} = f_{RF}$  the IF signal has a DC component given by:  $V_{IF}|_{DC} = \langle V_{IF}(t) \rangle = k_{CL} A_{RF} \cos \varphi$

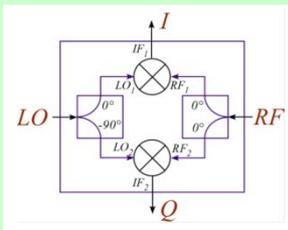
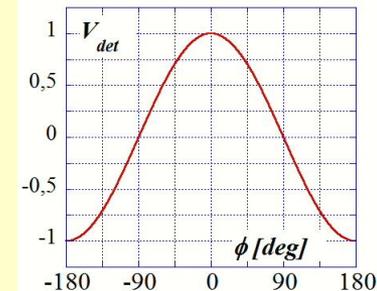
$$A_{RF} \cos(\omega t + \varphi)$$



$$A_{LO} \cos(\omega t)$$

$$V_{det} = V_{IF} = V(\varphi) + \text{high harm.}$$

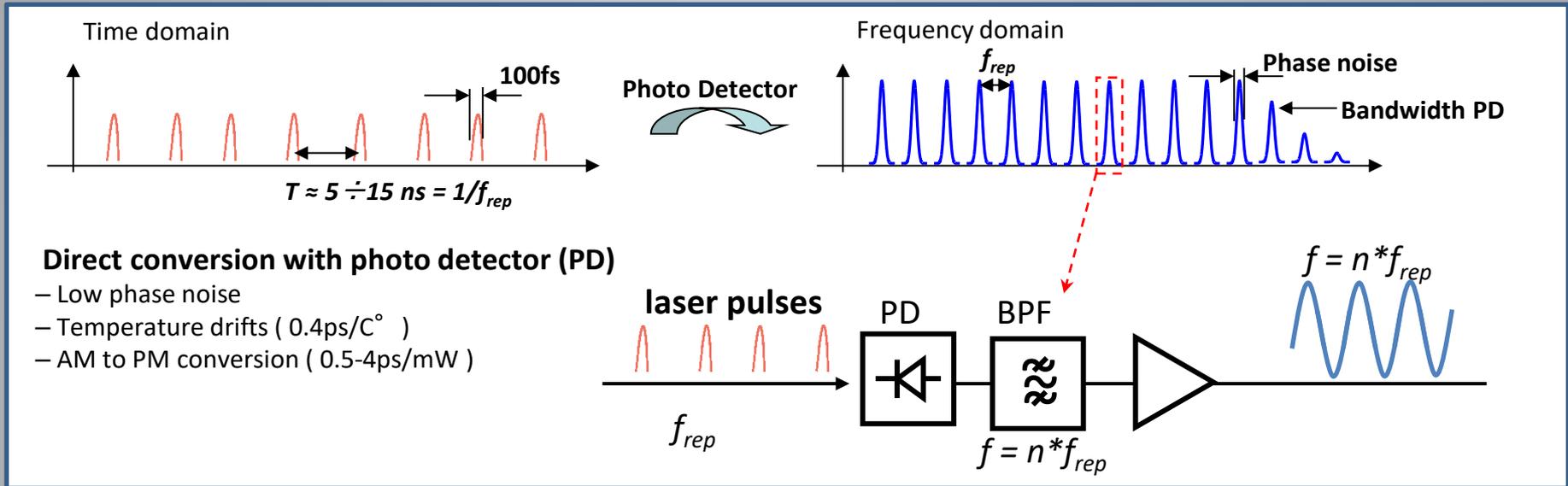
$$A_{RF} \ll A_{LO} \Rightarrow V_{det}(\varphi) = k_{CL} A_{RF} \cos \varphi$$



$$\begin{cases} V_I = k_{CL} A_{RF} \cos(\varphi) + \text{high harmonics} \\ V_Q = k_{CL} A_{RF} \sin(\varphi) + \text{high harmonics} \end{cases} \Rightarrow \begin{cases} A_{RF} \div \sqrt{V_I^2 + V_Q^2} \\ \varphi = \arctan(V_Q/V_I) + \frac{\pi}{2} [1 - \text{sgn}(V_I)] \end{cases}$$

$$\left. \frac{dV_{det}}{d\varphi} \right|_{\varphi=\pm\pi/2} = \mp k_{CL} A_{RF} \underset{A_{RF}=1V}{\underset{CL=6dB}{\approx}} 5 \div 10 \text{ mV/Deg} \underset{f_c=10GHz}{\approx} 15 \div 30 \text{ mV/ps}$$

- ✓ Passive
- ✓ Cheap, Robust
- ✓ Wideband
- ✓ Sensitivity proportional to level, AM → PM not fully rejected
- ✓ Noise figure  $F \approx CL$
- ✓ Good sensitivity but lower wrt optical devices



## Phase detection between RF and Laser – Sagnac Loop Interferometer or BOM-PD

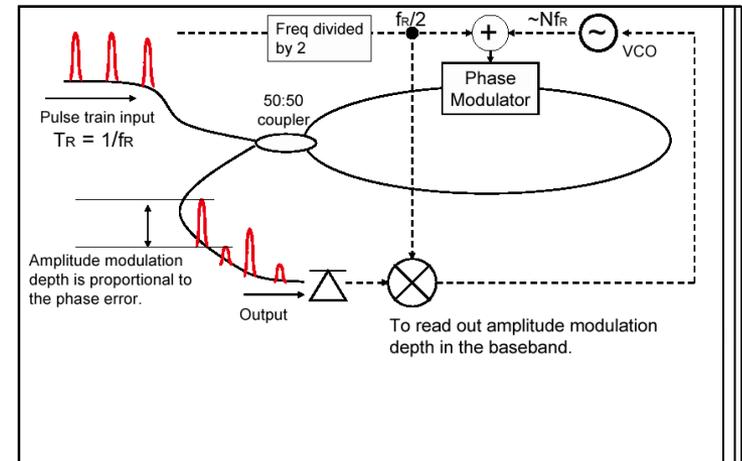
Recently ( $\approx 10$  years) special devices to perform direct measurements of the relative phase between an RF voltage and a train of short laser pulses have been developed

balanced optical mixer to lock RF osc.

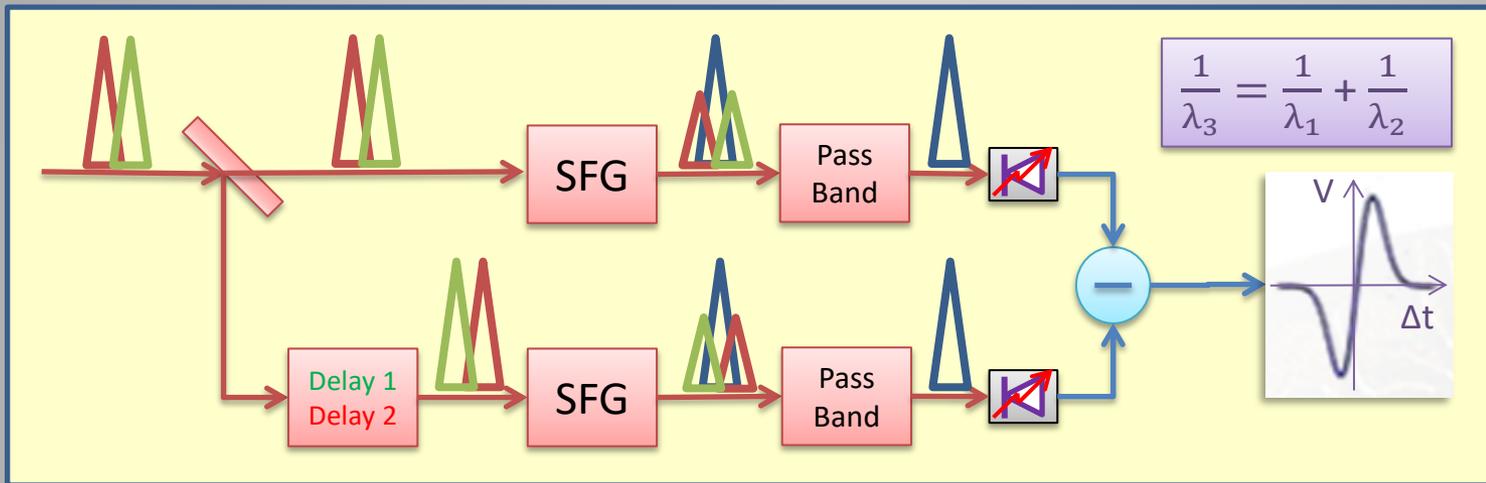
- insensitive against laser fluctuation
- Very low temperature drifts

### Results:

$f=1.3\text{GHz}$  jitter & drift  $< 10 \text{ fs rms}$  *limited by detection!*



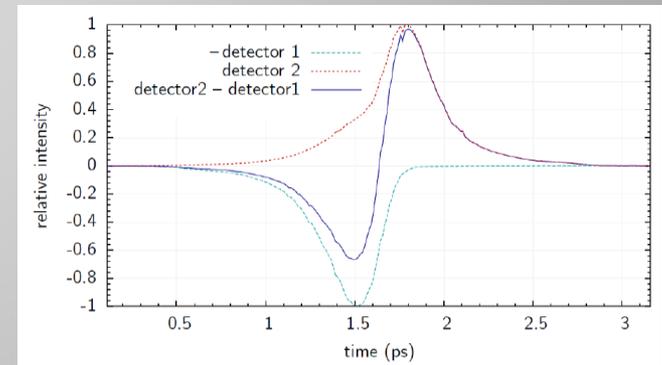
**Balanced cross correlation** of very short optical pulses ( $\sigma_t \approx 200$  fs) provides an **extremely sensitive** measurement of the **relative delay between 2 pulses**.



The two pulses have orthogonal polarization and generate a shorter wavelength pulse proportional to their time overlap in each branch by means of non-linear crystal.

In a second branch the two polarizations experience a differential delay  $\Delta T = T_1 - T_2 \approx \sigma_t$ . The amplitudes of the interaction radiation pulses are converted to voltages by photodiodes and their difference  $V_0$  is taken as the detector output  $V_0$ .

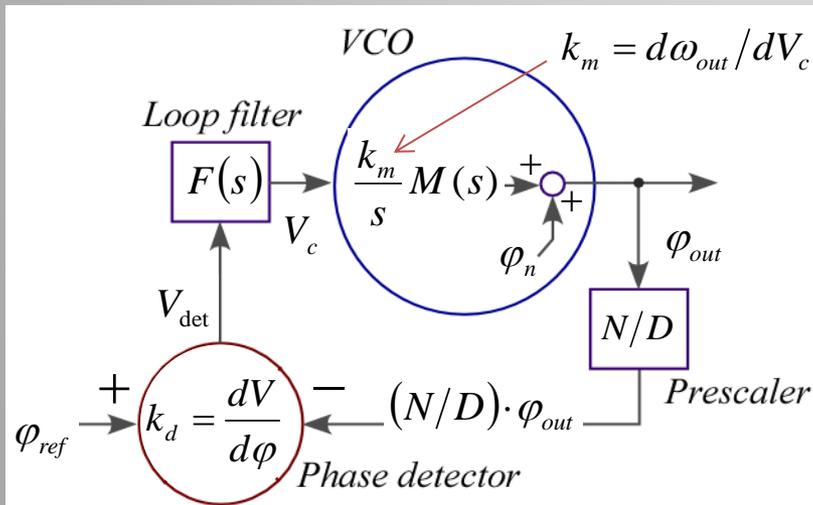
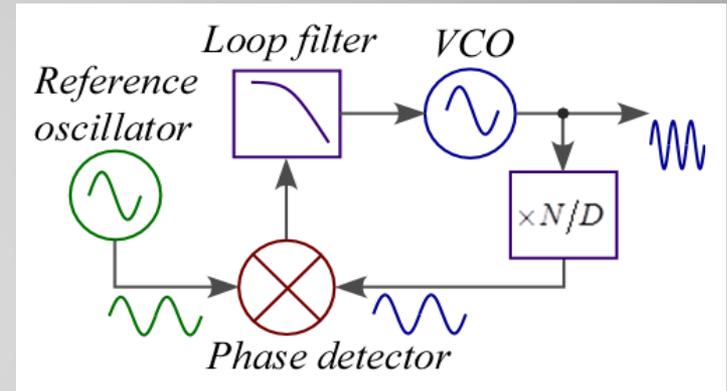
If the initial time delay between the pulses is exactly  $\Delta T/2$  then clearly  $V_0 \approx 0$  (balance), while it grows rapidly as soon as initial delay deviates.



Detection sensitivity up to 10 mV/fs achievable with ultra-short pulses!!!

PLLs are a very **general subject** in RF electronics, used to **synchronize oscillators** to a **common reference** or to **extract the carrier** from a **modulated signal** (FM tuning). In our context PLLs are used to **phase-lock the clients** of the synchronization system **to the master clock** (RMO or OMO). The building blocks are:

- A VCO, whose frequency range includes  $(D/N) f_{ref}$ ;
- A phase detector, to compare the scaled VCO phase to the reference;
- A loop filter, which sets the lock bandwidth;
- A prescalers or synthesizer ( $N/D$  frequency multiplier,  $N$  and  $D$  integers) if different frequencies are required.



**PLL linear model**

**PLL transfer function**

$$\varphi_{out}(s) = \frac{D}{N} \frac{H(s)}{1 + H(s)} \varphi_{ref}(s) + \frac{1}{1 + H(s)} \varphi_n(s)$$

*VCO noise*

$$\text{with } H(s) = \frac{N}{D} \frac{k_d k_m}{s} F(s) M(s)$$

*freq-to-phase conversion      loop filter      VCO mod. bandwidth*

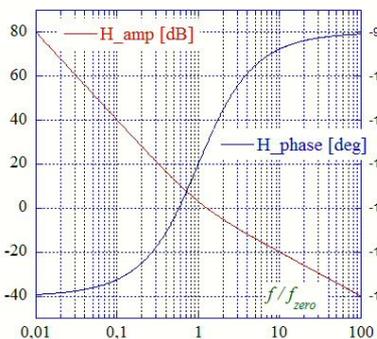
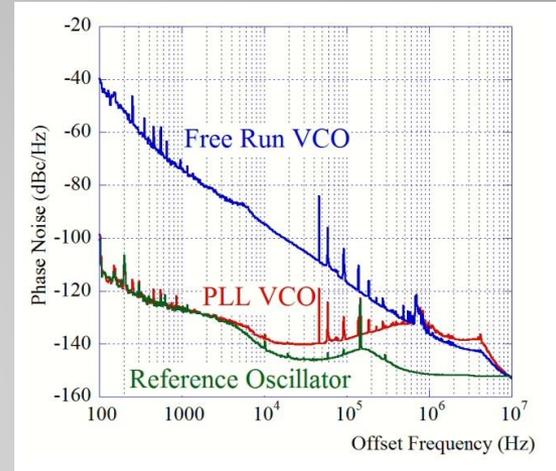
**Loop filters** provide **PLL stability**, tailoring the frequency response, and **set loop gain** and **cut-off frequency**.

The **output phase spectrum** is **locked** to the **reference** if  $|H(j\omega)| \gg 1$ , while it returns similar to the **free run VCO** if  $|H(j\omega)| < 1$ .

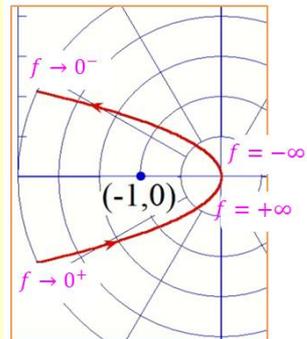
A flat-frequency response loop filter gives already a pure integrator loop transfer function thanks to a pole in the origin ( $f=0$ ) provided by the dc frequency control of the VCO.

Loop filters properly designed can improve the PLL performance:

- ✓ By furtherly increasing the low-frequency gain and remove phase offsets due to systematic VCO frequency errors, by means of extra poles in the origin (integrators) compensated by zeroes properly placed;
- ✓ By enlarging the PLL BW through equalization of the frequency response of the VCO modulation port.



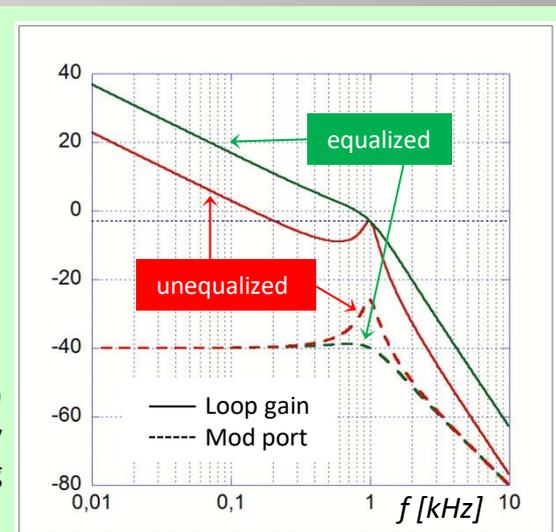
Bode plot of the PLL loop gain



Nyquist locus

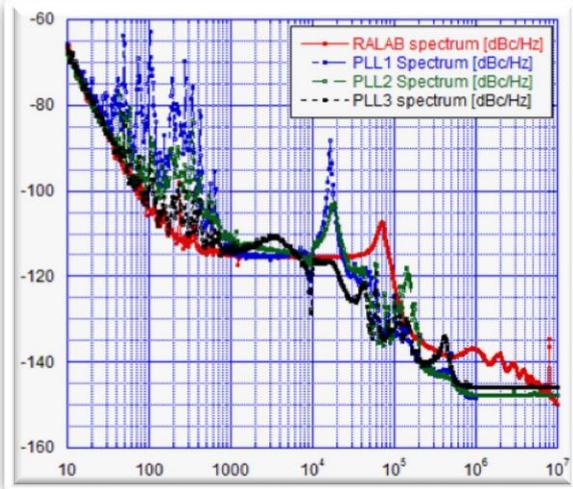
A very steep frequency response can be obtained (slope = 40 dB/decade) in stable conditions (see Nyquist plot).

Equalization of the VCO modulation port frequency response allows increasing the loop gain.



What is **peculiar** in **PLLs** for clients of a **stabilization system** of a Particle Accelerator facility ?

- ✓ Both the reference and client oscillators can be either RF VCOs or laser cavities. Phase detectors are chosen consequently;
- ✓ Laser oscillators behave as VCOs by trimming the cavity length through a piezo controlled mirror.
  - Limited modulation bandwidth ( $\approx$  few kHz typical);
  - Limited dynamic range ( $\Delta f/f \approx 10^{-6}$ ), overcome by adding motorized translational stages to enlarge the mirror positioning range;
  - At frequencies beyond PLL bandwidth ( $f > 1$  kHz) mode-locked lasers exhibit excellent low-phase noise spectrum.

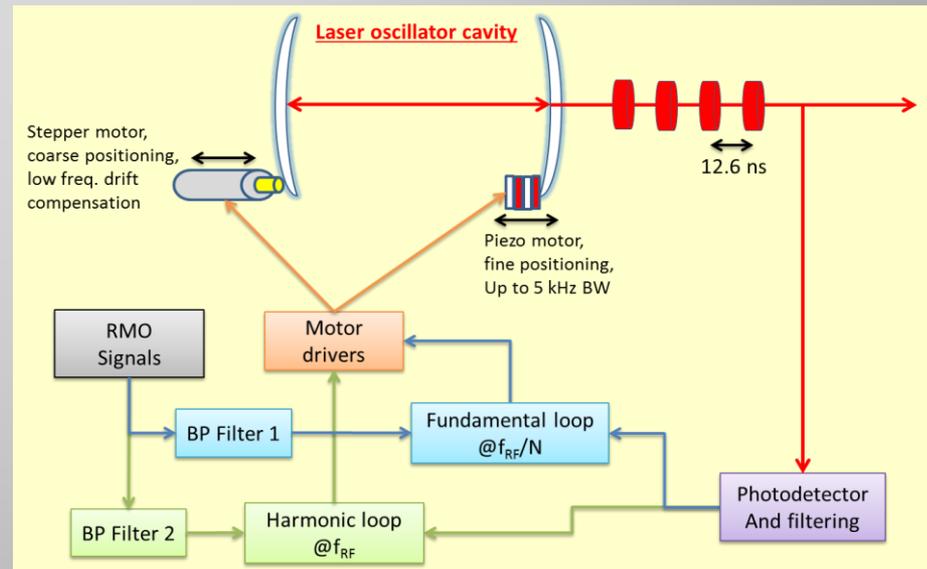


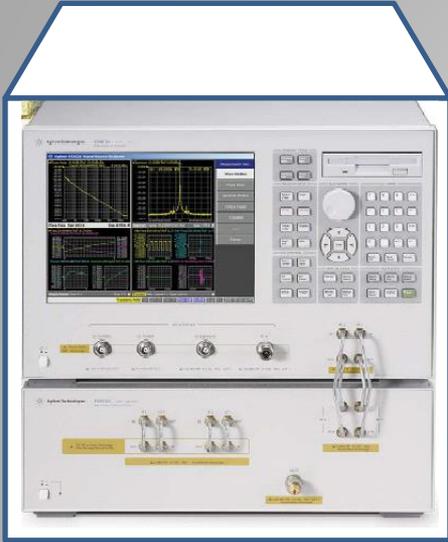
**RMO**  
 $\sigma_t \approx 85$  fs  
10 Hz – 10 MHz

**Laser:**

**PLL flat**  
 $\sigma_t \approx 230$  fs  
**PLL + 1 s=0 pole**  
 $\sigma_t \approx 85$  fs  
**PLL + 2 s=0 poles**  
 $\sigma_t \approx 70$  fs

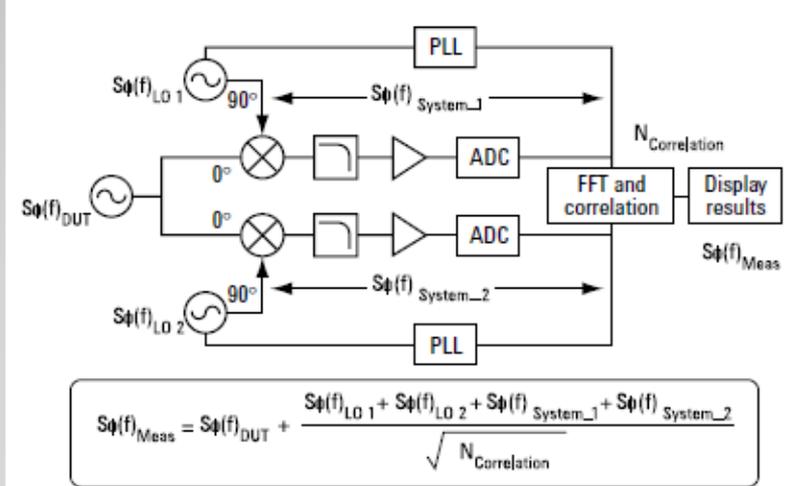
SSB phase noise of a locked OMO for different loop filters





**Signal Source Analyzers** SSA are dedicated instruments integrating an optimized set-up for precise phase noise measurements.

Two low noise LO oscillators are locked to the DUT signal. The instrument sets the cut-off frequency of the 2 PLLs well below the minimum frequency of the selected span.



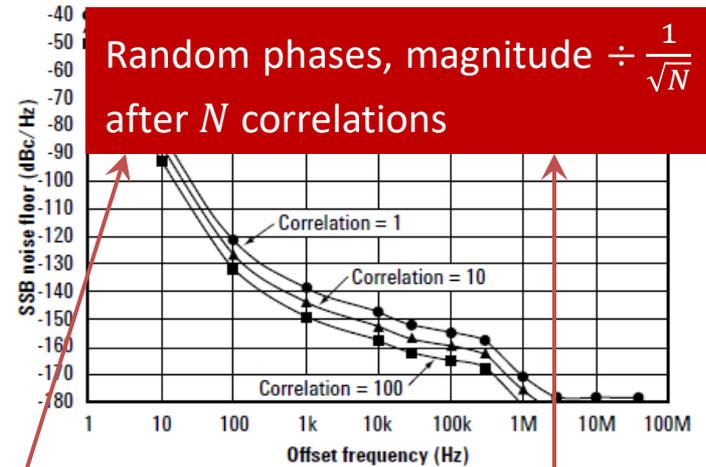
The phase noise of the DUT  $\varphi_{DUT}(t)$  is simultaneously measured wrt the 2 LOs:

$$\Delta\varphi_k(t) = \varphi_{DUT}(t) - \varphi_{LO,k}(t) \xrightarrow{\mathcal{F}\text{-trans}} \rightarrow \Delta\Phi_k(f) = \Phi_{DUT}(f) - \Phi_{LO,k}(f) \quad k = 1,2$$

The cross correlation function  $r(\tau)$  of  $\Delta\varphi_1(t)$  and  $\Delta\varphi_2(t)$ , and its Fourier transform  $R(f)$  are:

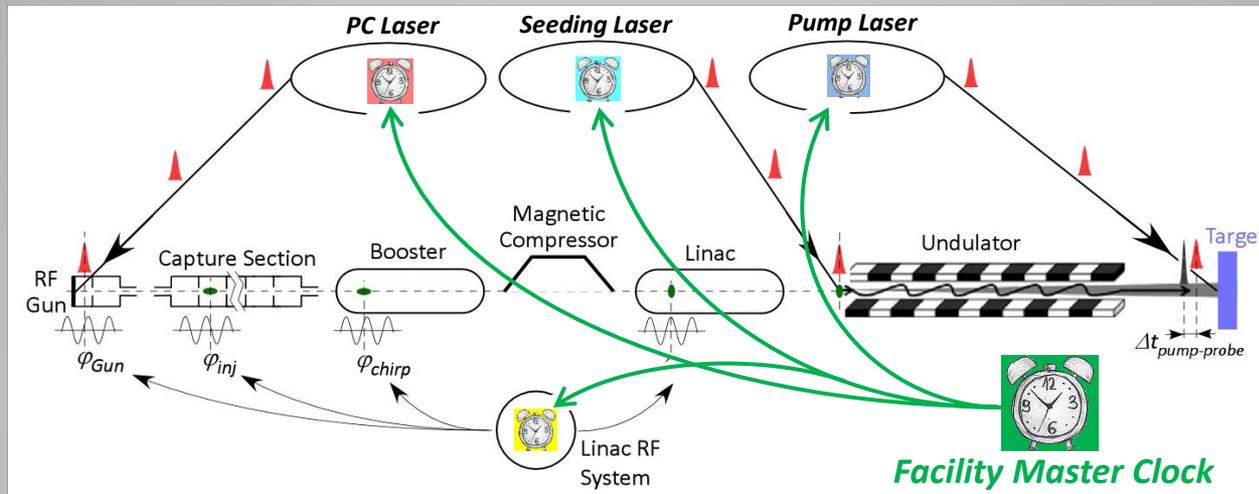
$$r(\tau) = \int_{-\infty}^{+\infty} \Delta\varphi_1(t) \cdot \Delta\varphi_2(t + \tau) dt$$

$$R(f) = \Delta\Phi_1^*(f) \cdot \Delta\Phi_2(f) = |\Phi_{DUT}(f)|^2 - \left( \Phi_{DUT}(f) \cdot \left( \Phi_{LO,1}^*(f) + \Phi_{LO,2}^*(f) \right) \right) + \left( \Phi_{LO,1}^*(f) \cdot \Phi_{LO,2}(f) \right)$$



## ***Performances of Synchronization Systems***

- ***Client Residual Jitter***
- ***Stabilized Reference Distribution***



A client with a free-run phase noise  $\varphi_{i_0}$  once being PLL locked to the reference with a loop gain  $H_i(j2\pi f)$  will show a residual phase jitter  $\varphi_i$  and a phase noise power spectrum  $S_i$  according to:

$$\varphi_i = \frac{H_i}{1 + H_i} \varphi_{ref} + \frac{1}{1 + H_i} \varphi_{i_0} \rightarrow S_i(f) = \frac{|H_i|^2}{|1 + H_i|^2} S_{ref}(f) + \frac{1}{|1 + H_i|^2} S_{i_0}(f)$$

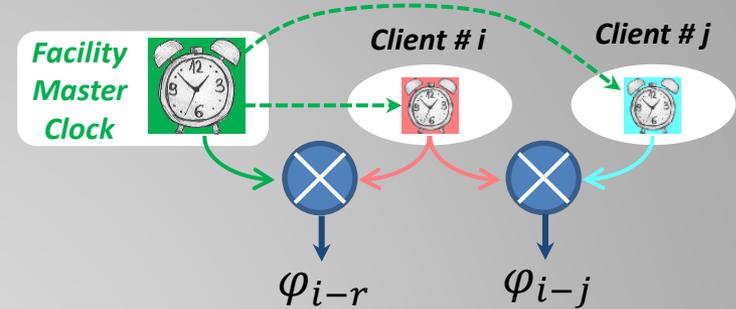
**Incoherent noise contributions**

Client absolute residual time jitter

$$\sigma_{t_i}^2 = \frac{1}{\omega_{ref}^2} \int_{f_{min}}^{+\infty} \frac{|H_i|^2 S_{ref}(f) + S_{i_0}(f)}{|1 + H_i|^2} df$$

But we are finally interested in relative jitter between clients and reference  $\varphi_{i-r} = \varphi_i - \varphi_{ref}$ , and among different clients  $\varphi_{i-j} = \varphi_i - \varphi_j$ :

$$\varphi_{i-r} = \frac{\varphi_{i_0} - \varphi_{ref}}{1 + H_i} \rightarrow S_{i-r}(f) = \frac{S_{i_0}(f) + S_{ref}(f)}{|1 + H_i|^2}$$



Client residual relative time jitter

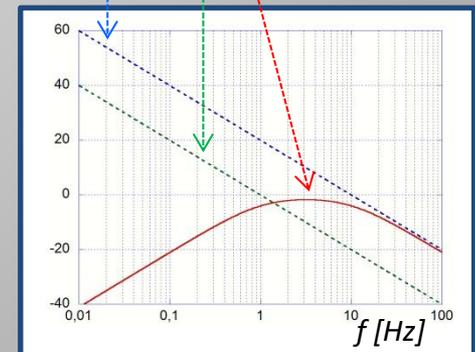
$$\sigma_{t_{i-r}}^2 = \frac{1}{\omega_{ref}^2} \int_{f_{min}}^{+\infty} \frac{S_{ref}(f) + S_{i_0}(f)}{|1 + H_i|^2} df$$

$$\varphi_{i-j} = \frac{\varphi_{i_0} - \varphi_{ref}}{1 + H_i} - \frac{\varphi_{j_0} - \varphi_{ref}}{1 + H_j} \rightarrow S_{i-j}(f) = \frac{S_{i_0}(f)}{|1 + H_i|^2} + \frac{S_{j_0}(f)}{|1 + H_j|^2} + \left[ \frac{H_i - H_j}{(1 + H_i)(1 + H_j)} \right]^2 S_{ref}(f)$$

$$\sigma_{t_{i-j}}^2 = \frac{1}{\omega_{ref}^2} \int_{f_{min}}^{+\infty} S_{i-j}(f) df$$

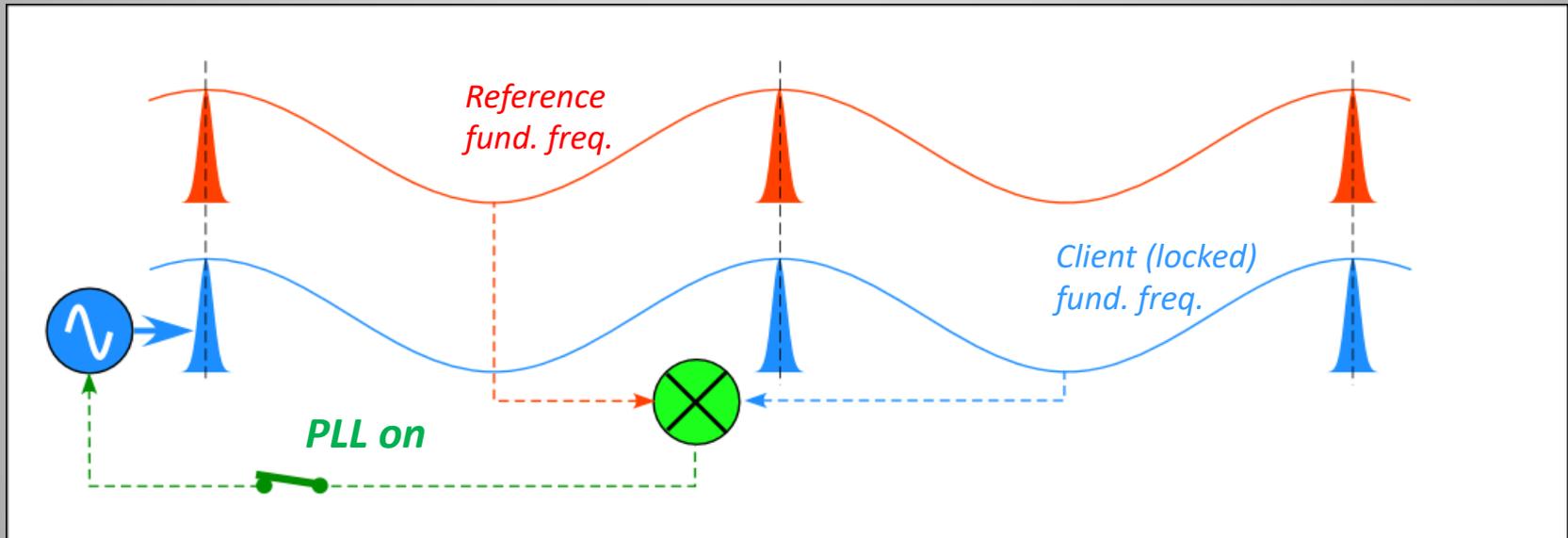
Residual relative time jitter between clients i-j

If  $H_i \neq H_j$  there is a **direct contribution** of the **master clock phase noise**  $S_{ref}(f)$  to the **relative jitter** between clients  $i$  and  $j$  in the region between the cutoff frequencies of the 2 PLLs. That's why a **very low RMO phase noise** is specified in a **wide spectral region** including the cut-off frequencies of all the client PLLs (0.1÷100 kHz typical).



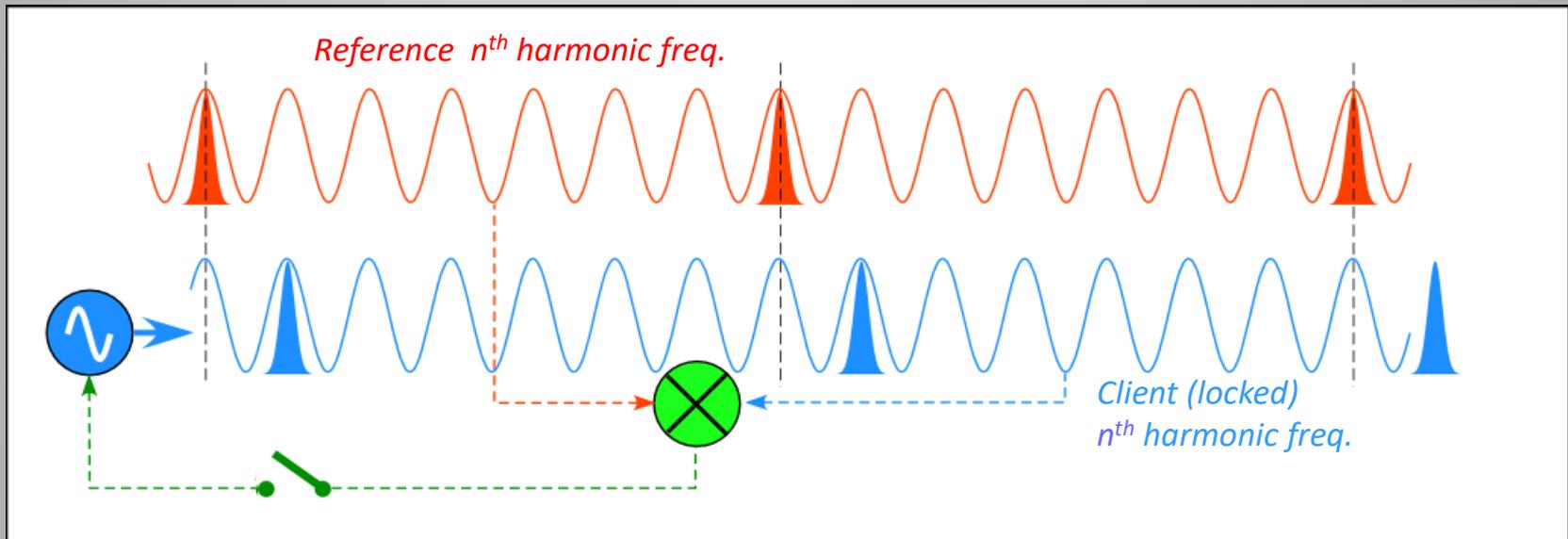
***GO TO  
EXERCISE #2***

- Sometimes synchronization systems need to deal with relatively low rep rate client oscillators. This is the case of laser oscillators ( $f_{rep} \approx 100 \text{ MHz}$ ,  $T \approx 10 \text{ ns}$  typically).
- The synchronization PLL can work on the fundamental frequency extracted from the client output. The reference itself, especially when encoded in pulsed Optical Master Oscillators, may present a low rep rate, typically the same or a rational fraction of the client to be synchronized.



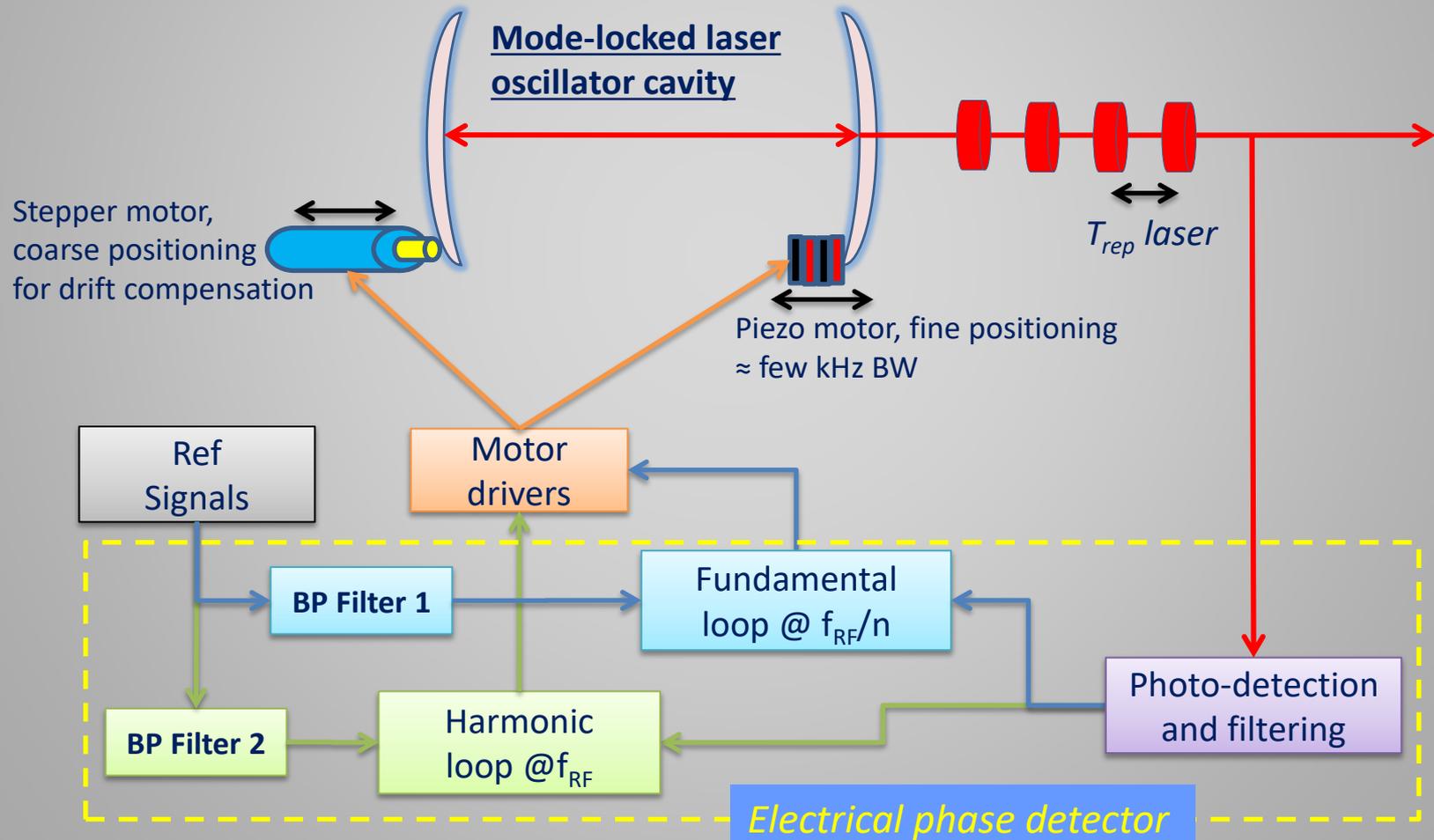
- Although this scheme can decently work, the phase detection sensitivity is quite poor ( $1 \text{ Deg} \approx 10 \div 100 \text{ ps @ fund. freq.}$ ), limiting the achievable performances in terms of phase noise reduction.

- Phase detection sensitivity can be improved by a factor “n” by extracting and locking from both reference and client the  $n^{\text{th}}$  harmonic of the fundamental frequency. This approach is particularly suitable for mode-locked lasers that provide extremely short pulses and large bandwidths.

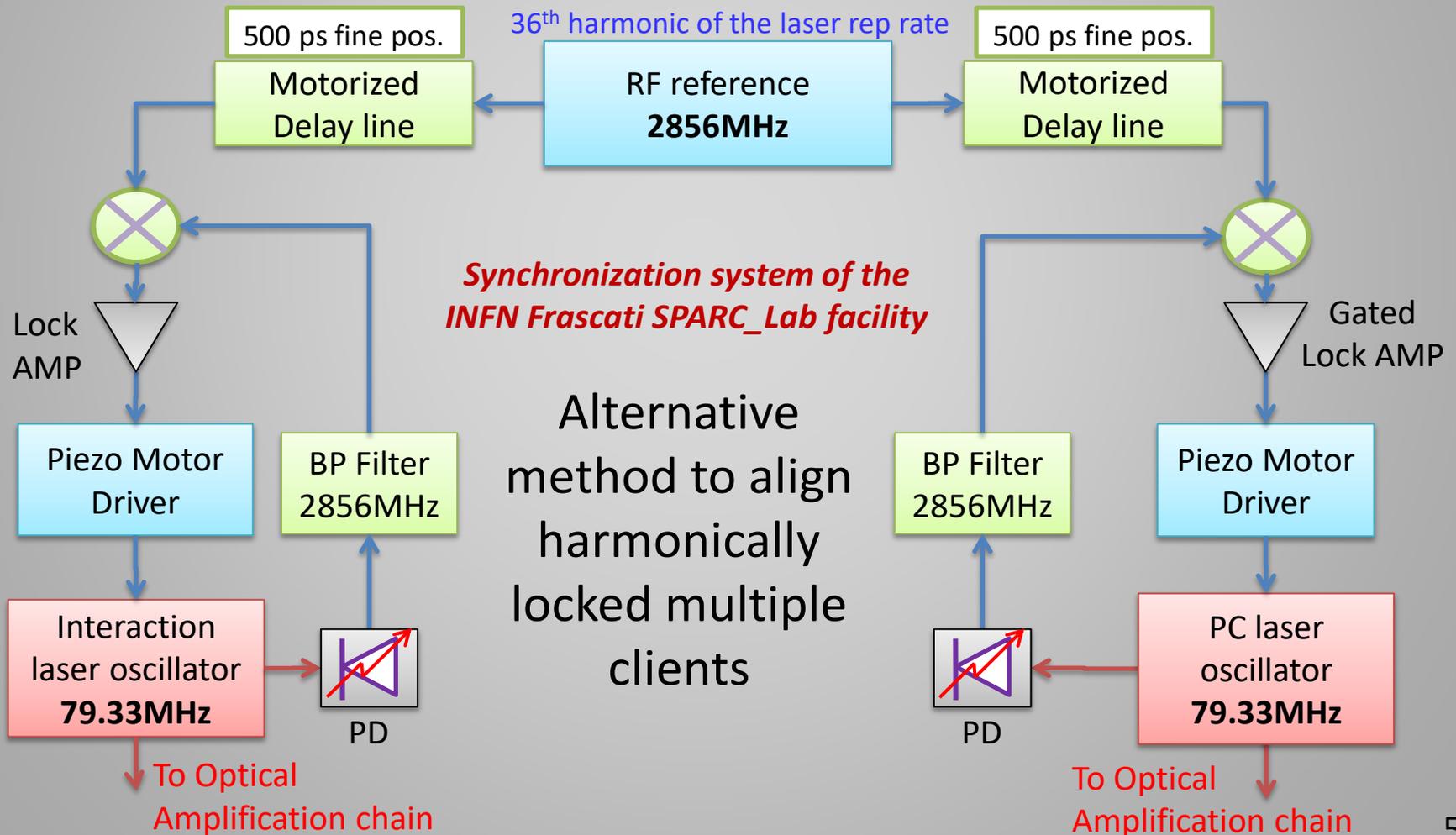


- But a PLL based on a  $\mu$ -wave mixer can only lock the input sine waves. There are “n” possible relative positions of the client compatible with the harmonic locking, and the client will randomly jumps from one to another every time the lock is reinitialized or it is recovered after a temporary failure due to some disturbance.

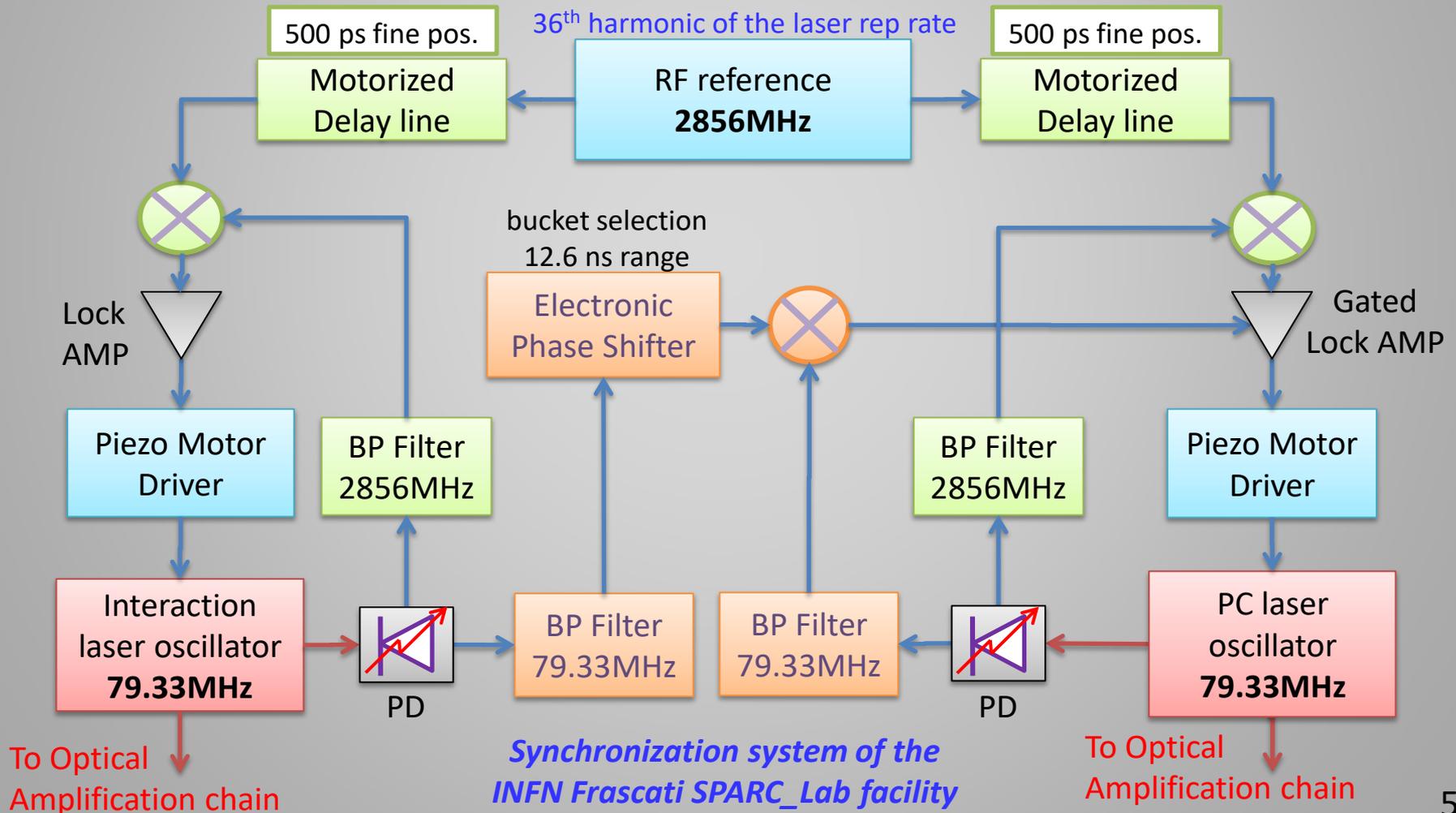
To remove the uncertainty among the  $n$  equivalent lock positions one possibility is to have both fundamental and harmonic loops in operation, always starting with the fundamental one for univocal positioning before activating the harmonic one to improve detection sensitivity.



Another way around to remove the positioning uncertainty of the harmonic lock that no requires the activation of a parallel fundamental loop is to gate the loop error amplifier with a signal derived from a phase comparison at fundamental frequency.

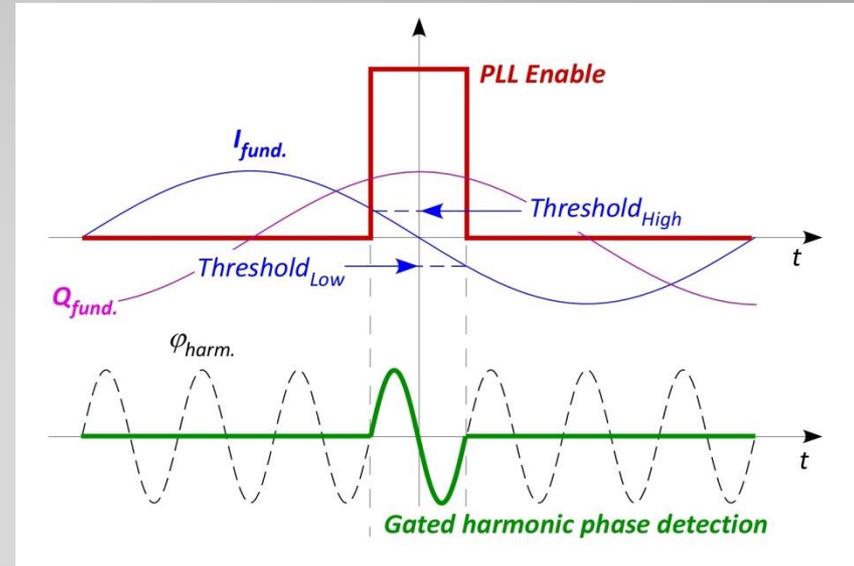
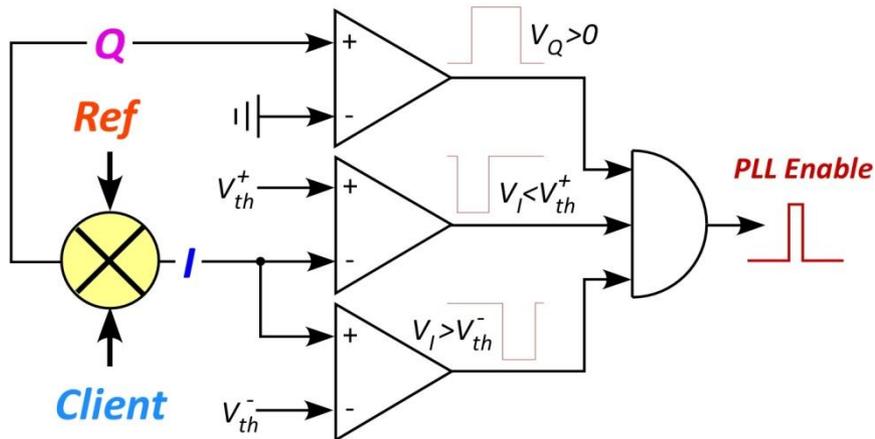


The error amp of one PLL is enabled only under the condition that the relative phase between the 2 lasers measured at the fundamental frequency is within a narrow range corresponding to 1 single period of the phase measured at the harmonic frequency.



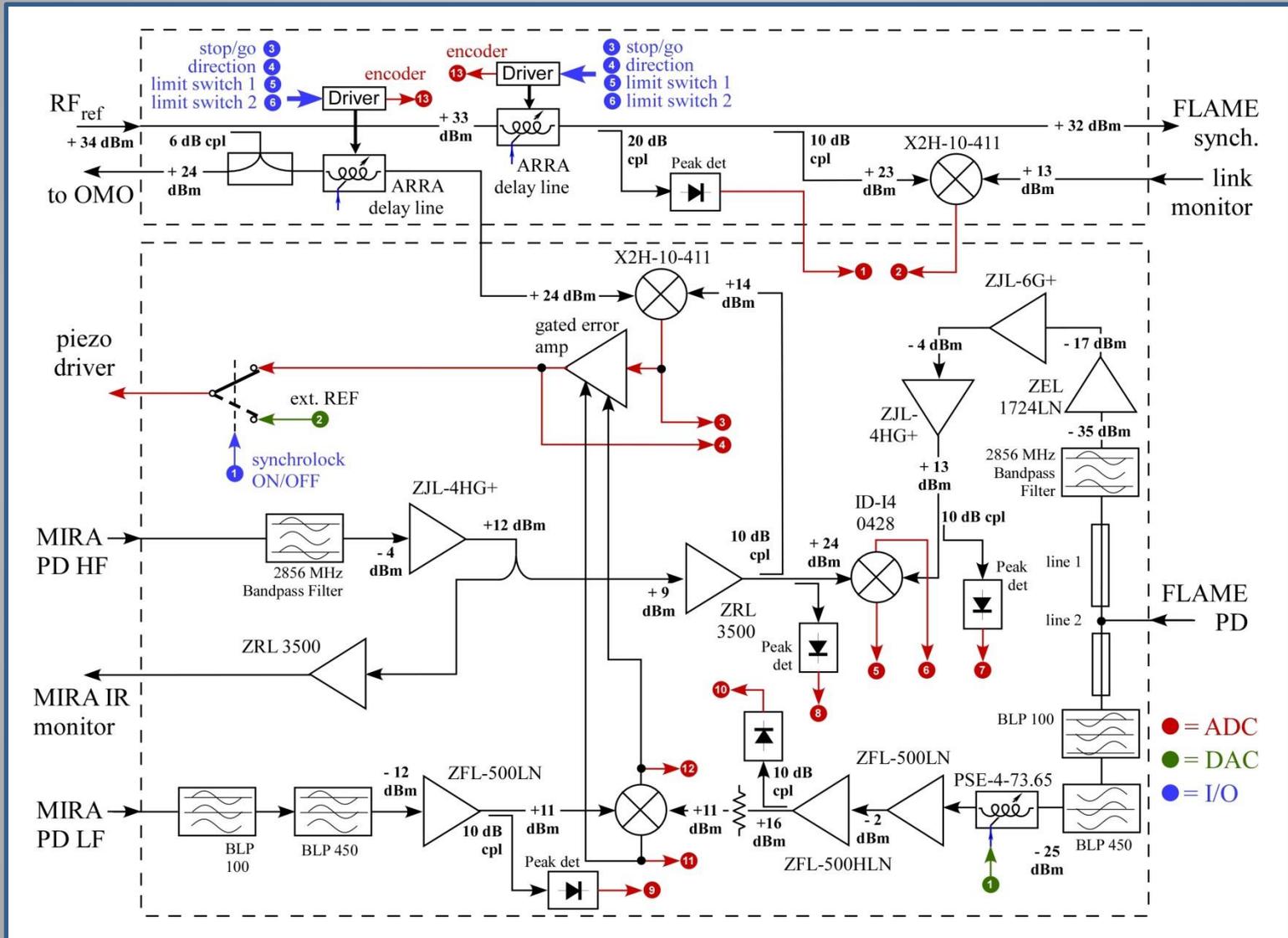
## How is the gate/enable signal generated?

To isolate and select a unique zero in the harmonic phase response, a gate corresponding to 1/n of the fundamental period have to be generated starting from I and Q signals obtained by demodulation at the client fundamental frequency.

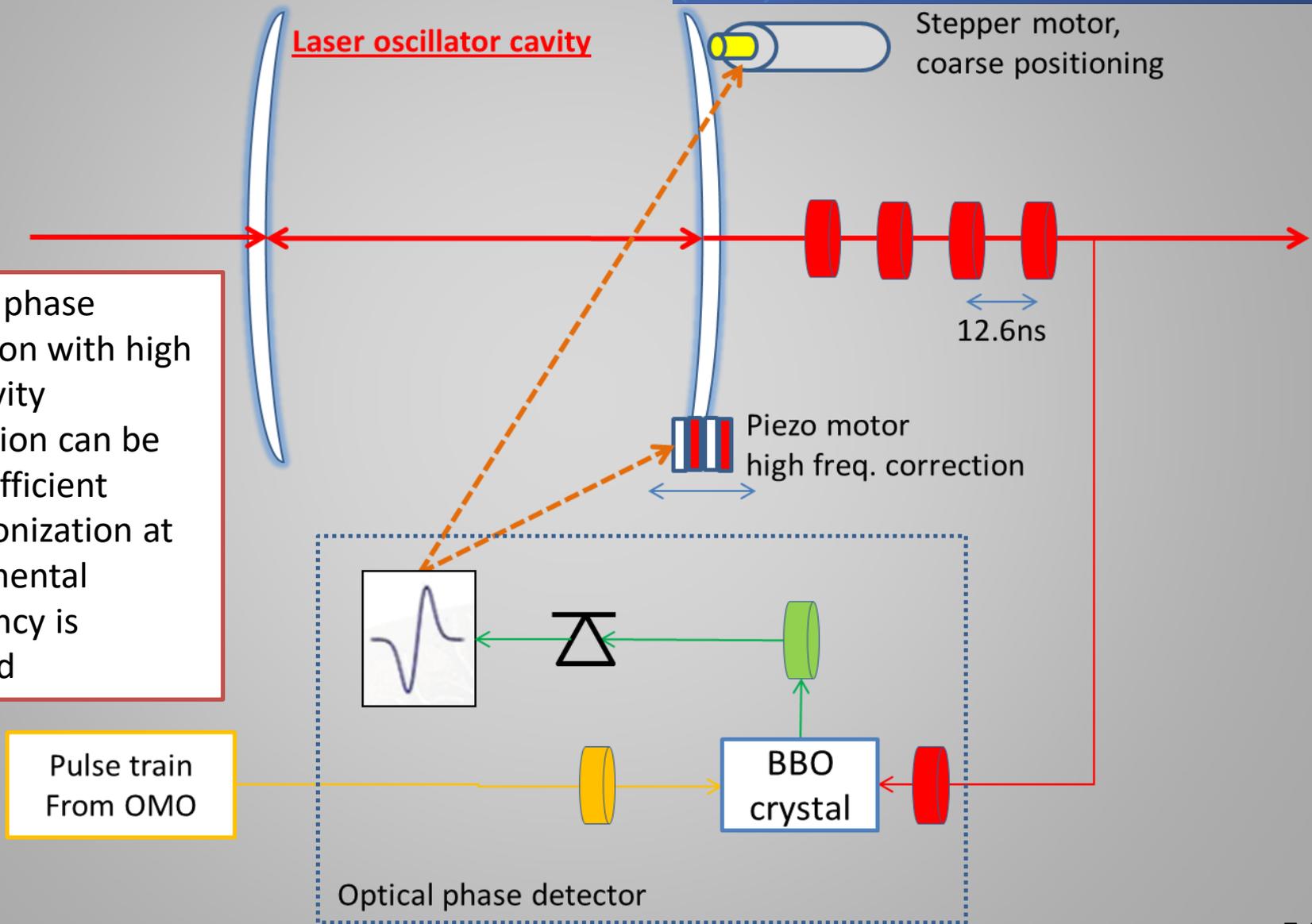


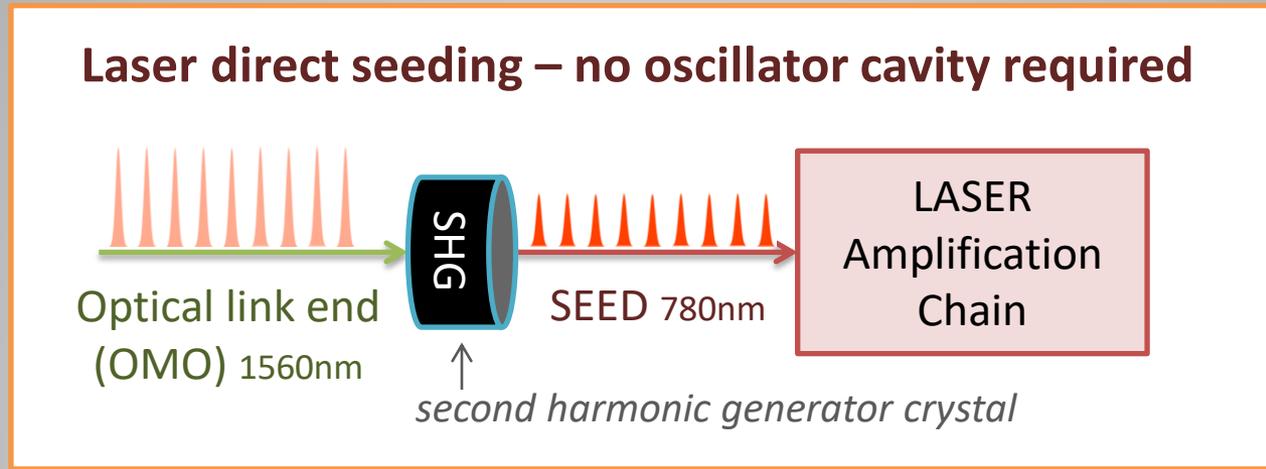
The correct gate aperture is obtained by proper setting a voltage range defined by 2 threshold levels and by imposing the conditions that one of the Cartesian component has a value inside the range while the other has a well defined polarity (either positive or negative).

Simple electronic discriminators are used for this task. The shape of the phase detection characteristics obtained by an harmonic detector followed by a gated PLL error amplifier resembles those featured by optical x-correlators, with a high sensitive response limited to a very narrow portion of the period of the client rep rate.



- optical phase detection with high sensitivity
- correction can be more efficient
- synchronization at fundamental frequency is ensured



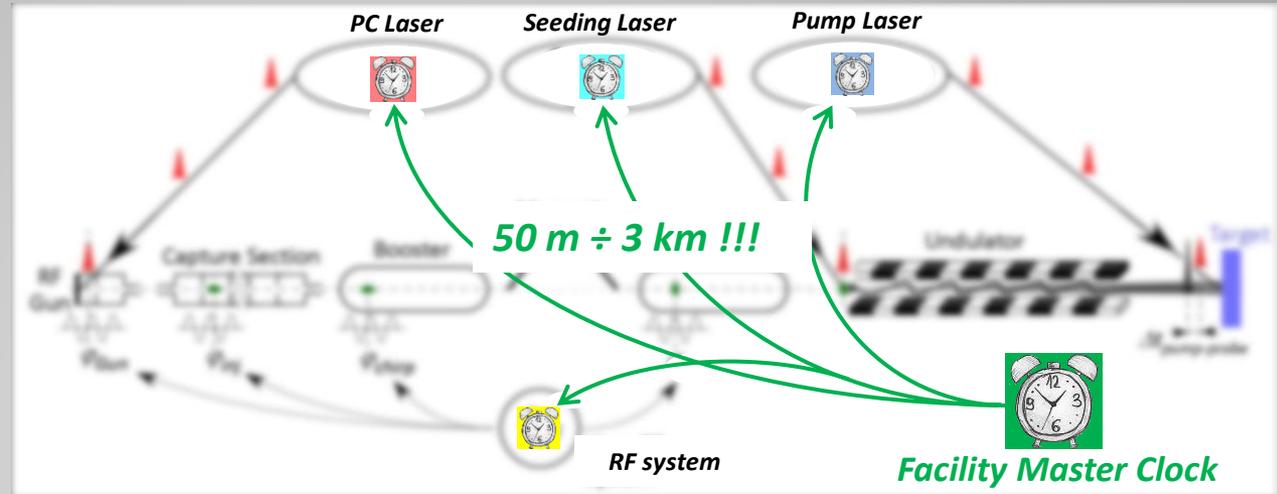


- Simplest and (relatively) low cost solution, when technically doable
- Client directly synchronized to the reference (only distribution residual noise is present)
- OMO and client lasers have to be wavelength “compatible”
- OMO has to be suitable parameters for amplification (i.e. power, spectral bandwidth, ...)

Client **jitters** can be reduced by **efficient PLLs** locking to a local copy of the reference.

Reference distribution **drifts** need to be **under control** to preserve a good facility synchronization.

Depending on the facility size and specification the reference distribution can be:

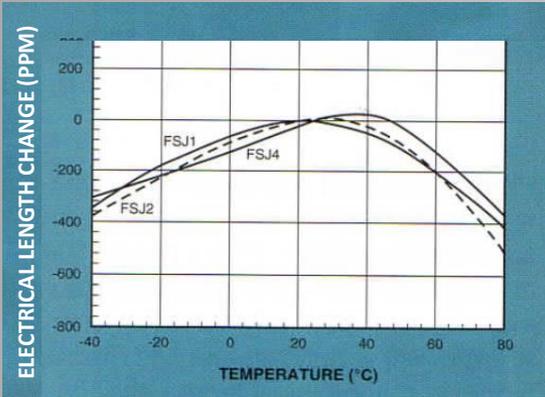


## RF based, through coaxial cables

- ✓ *Passive (mainly) / actively stabilized*
- ✓ *Cheap*
- ✓ *Large attenuation at high frequencies*
- ✓ *Sensitive to thermal variations*  
*(copper linear expansion  $\approx 1.7 \cdot 10^{-5}/^{\circ}\text{C}$ )*
- ✓ *Low-loss 3/8" coaxial cables very stable for  $\Delta T \ll 1^{\circ}\text{C}$  @  $T_0 \approx 24^{\circ}\text{C}$*

## Optical based, through fiber links

- ✓ *Pulsed (mainly), also CW AM modulated*
- ✓ *High sensitivity error detection (cross correlation, interferometry, ...)*
- ✓ *Small attenuation, large BW*
- ✓ *Expensive*
- ✓ *Active stabilization always needed (thermal sensitivity of fibers)*
- ✓ *Dispersion compensation always needed for pulsed distribution*



Around some optimal temperature  $T_{opt}$  cable physical elongation is compensated by dielectric constant variation. PPM relative delay variation is:

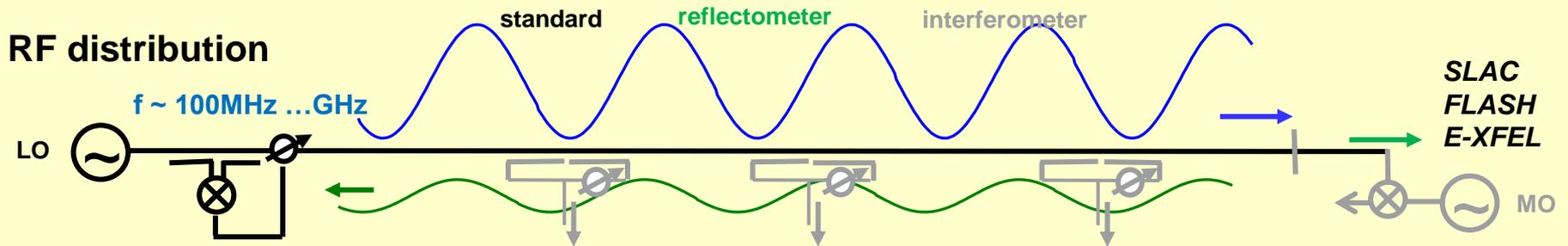
$$\left. \frac{\Delta\tau}{\tau} \right|_{PPM} \approx - \left( \frac{T - T_{opt}}{T_c} \right)^2$$

For a 3/8" cable (FSJ2):  $T_{opt} \approx 24^\circ\text{C}$ ,  $T_c \approx 2^\circ\text{C}$ . Good enough?

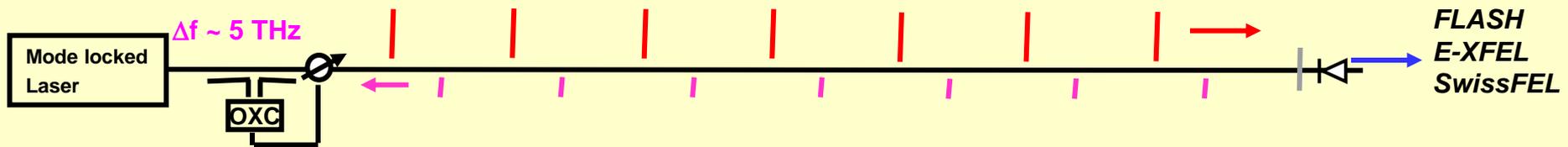
$L \approx 1 \text{ km} \rightarrow \tau \approx 5 \mu\text{s} \rightarrow \Delta\tau/\tau \approx 5 \text{ fs}/5 \mu\text{s} \approx 10^{-3} \text{ PPMs} !!!$

**LONG DISTANCES → ACTIVE LINK STABILIZATION REQUIRED !!!**

## RF distribution



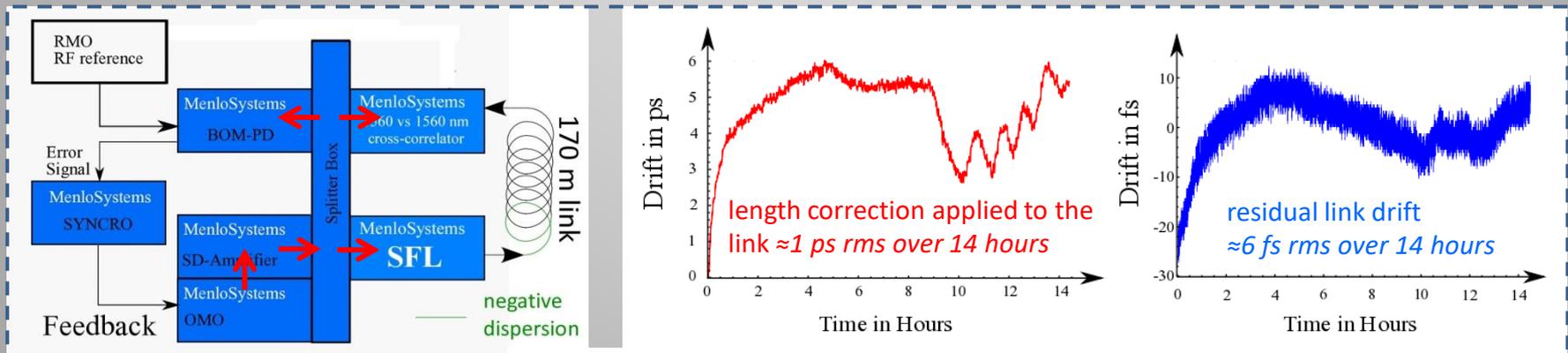
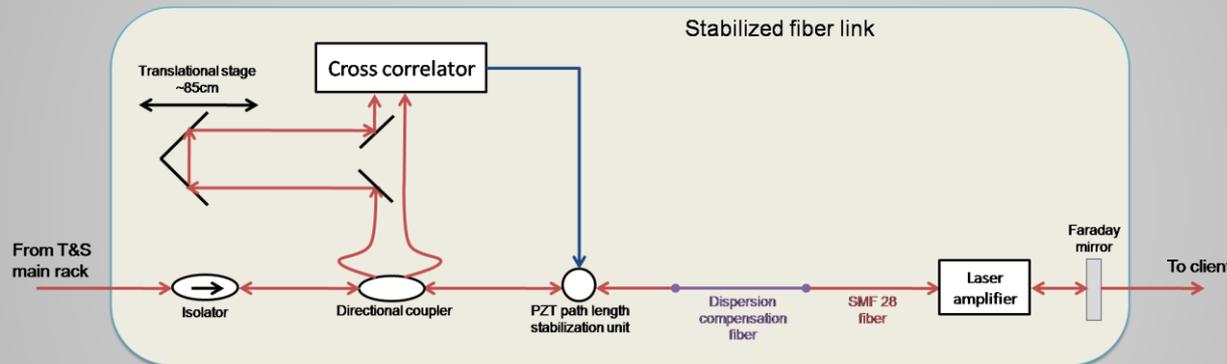
## Pulsed Optical distribution



Sketches from H. Schlarb

*Active stabilized links* are based on high resolution *round trip time measurements* and *path length correction* to stick at some stable reference value.

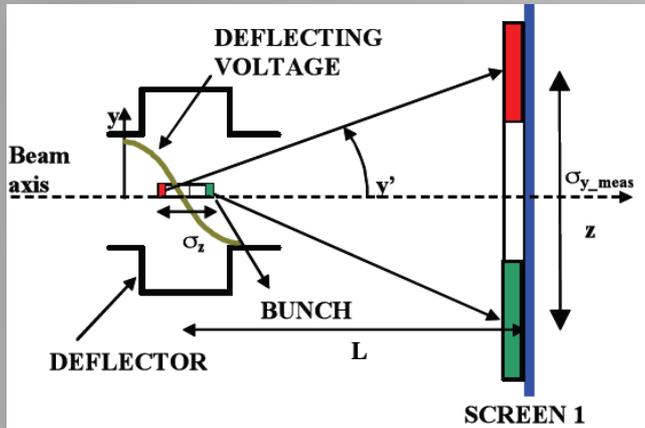
Pulsed optical distribution is especially suitable, because of low signal attenuation over long links and path length monitoring through very sensitive pulse cross-correlators. However, *dispersion compensation of the link is crucial* to keep the optical pulses very short ( $\approx 100$  fs).



Courtesy of MenloSystems GmbH

## ***Beam Synchronization***

- ***Effects of Client Synchronization Errors on Bunch Arrival Time***
- ***Bunch Arrival Monitors***

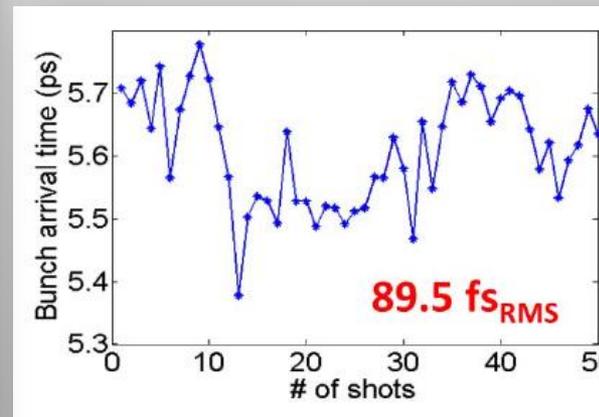
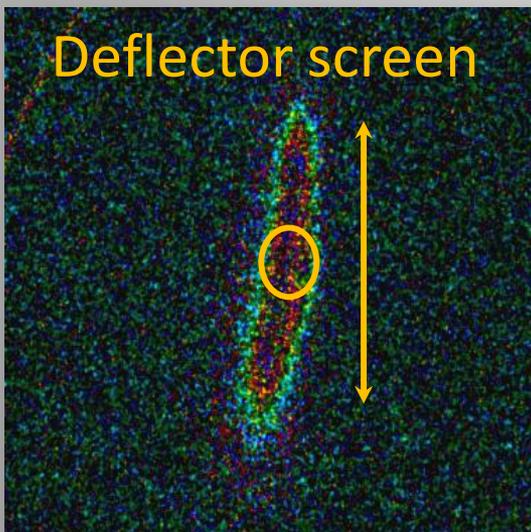


The beam is **streaked** by a **transverse RF cavity** on a **screen**. The image is captured by a camera. Longitudinal charge distribution and centroid position can be measured.

- ✓ Works typically on single bunch. Bunch trains can be eventually resolved with fast gated cameras;
- ✓ Destructive (needs a screen ...)
- ✓ Measure bunch wrt to RF (relative measurement)
- ✓ with a spectrometer → long. phase space imaging -  $(z, \epsilon) \rightarrow (y, x)$

$$\tau_{res} = \frac{E/e}{\omega_{RF} V_{\perp}} \sqrt{\frac{\epsilon_{\perp}}{\beta_{\perp}^{defl}}}$$

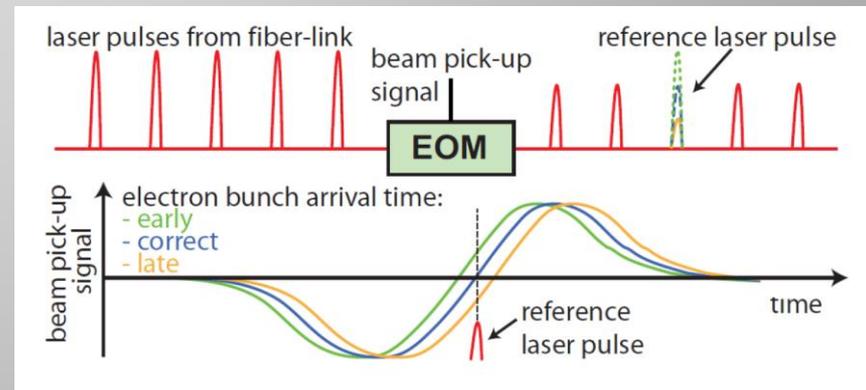
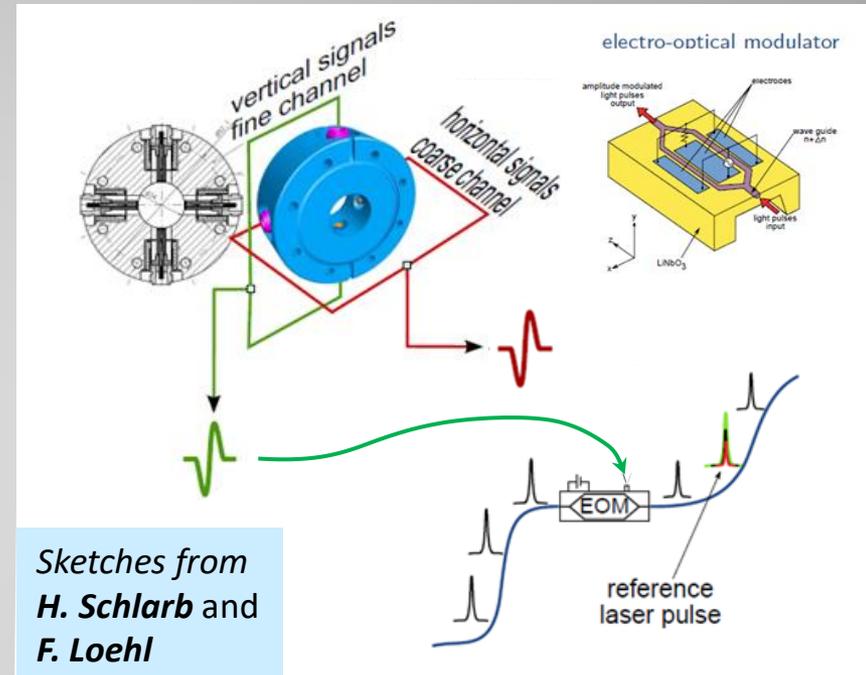
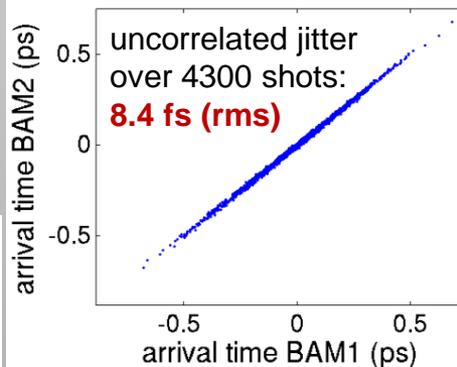
Achievable resolution down to  $\approx 10$  fs

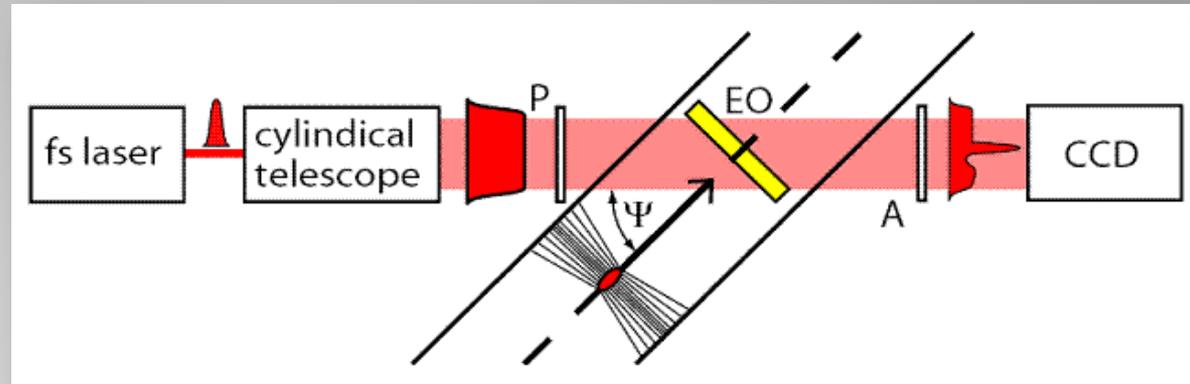
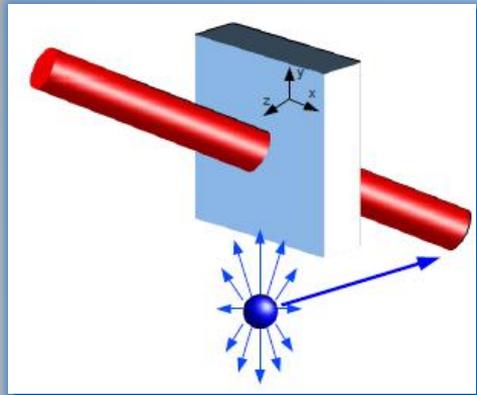


A **reference laser pulse train** (typically taken from the facility OMO) is connected to the optical input of a **Mach-Zehnder interferometric modulator (EOM)**. The short laser pulses are **amplitude-modulated** by a bipolar signal taken from a **button BPM** placed along the beam path and synchronized near to the voltage zero-crossing. **The bunch arrival time jitter and drift** is converted in **amplitude modulation** of the laser pulses and measured.

- ✓ Works very well on bunch trains;
- ✓ Non-intercepting;
- ✓ Measure bunch wrt to a laser reference (OMO);
- ✓ Demonstrated high resolution

BAM 1 – 2 placed  
60 m away along  
the beam path

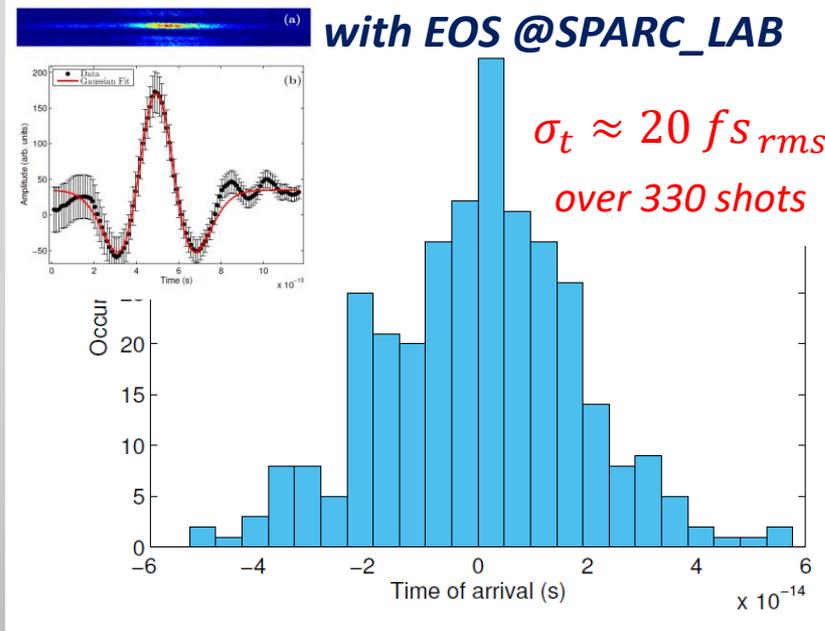




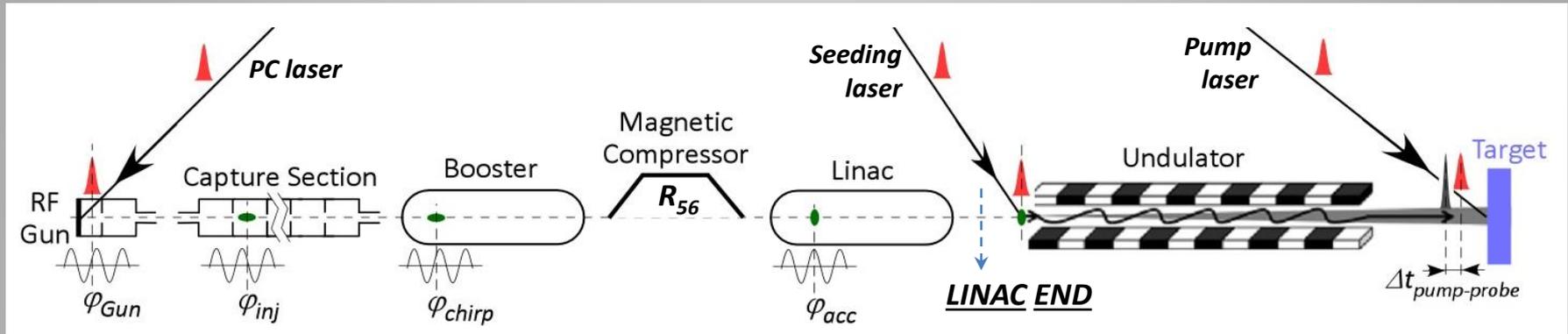
An **electro-optic crystal** is placed near the beam trajectory. In correspondence to the beam passage the crystal is illuminated with a **short reference laser pulse** transversally enlarged and **linearly polarized**. The bunch electric field induces **bi-refringence** in the crystal, so that while propagating the laser gains **elliptical polarization**. A polarized output filter delivers a signal proportional to the **polarization rotation**, i.e. to the **beam longitudinal charge distribution**.

- ✓ Single shot, non-intercepting;
- ✓ Provides charge distribution and centroid position;
- ✓ Resolution  $\approx 50$  fs for the bunch duration, higher for centroid arrival time ( $1$  pixel  $\approx 10$  fs).

## beam ATJ vs. PC laser measured with EOS @SPARC\_LAB



How beam arrival time is affected by synchronization errors of the sub-systems?



Perfect synchronization → the time (or phase)  $T_i$  of all sub-systems properly set to provide required beam characteristics at the Linac end, where the bunch centroid arrives at time  $T_b$ .

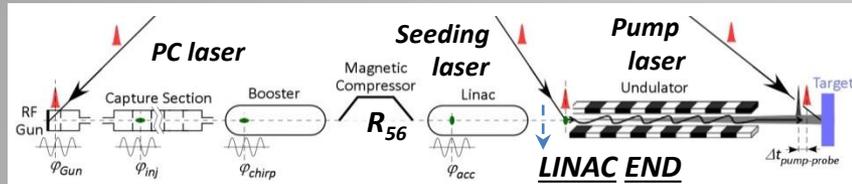
Perturbations of subsystem phasing  $\Delta t_i$  will produce a change  $\Delta t_b$  of the beam arrival time.

First-order approximation:

$$\Delta t_b = \sum_i a_i \Delta t_i = \sum_i \frac{\Delta t_i}{c_i} \quad \text{with} \quad \sum_i a_i = 1$$

Compression coefficients

Values of  $a_i$  can be computed analytically, by simulations or even measured experimentally. They very much depends on the machine working point.



How beam arrival time is affected by synchronization errors of the sub-systems?

- ✓ No compression: Beam captured by the GUN and accelerated on-crest

$$a_{PC} \approx 0.7 ; \quad a_{RF_{GUN}} \approx 0.3 ; \quad \text{others } a_i \approx 0$$

- ✓ Magnetic compression: Energy-time chirp imprinted by off-crest acceleration in the booster and exploited in magnetic chicane to compress the bunch

$$a_{RF_{boost}} \approx 1 ; \quad |a_{PC}| \ll 1 ; \quad \text{others } a_i \approx 0$$

Compression can be staged (few compressors acting at different energies). Bunch can be overcompressed (head and tail reversed,  $a_{PC} < 0$ ).

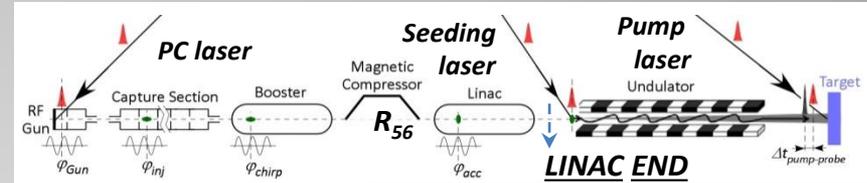
- ✓ RF compression: a non fully relativistic bunch ( $E_0 \approx \text{few MEV}$  at Gun exit) injected ahead the crest in an RF capture section slips back toward an equilibrium phase closer to the crest during acceleration, being also compressed in this process

$$a_{RF_{CS}} \approx 1 ; \quad |a_{PC}|, |a_{RF_{GUN}}| \ll 1 ; \quad \text{others } a_i \approx 0$$

The bunch gains also an Energy-time chirp. RF and magnetic compressions can be combined.

Particle distribution within the bunch and shot-to-shot centroid distribution behave similarly, but values of coefficients  $a_i$  might be different since space charge affects the intra-bunch longitudinal dynamics.

## Bunch Arrival Time Jitter



If we consider uncorrelated residual jitters of  $\Delta t_i$  (measured wrt the facility reference clock), the bunch arrival time jitter  $\sigma_{t_b}$  is given by:

$$\sigma_{t_b}^2 = \sum_i a_i^2 \sigma_{t_i}^2$$

while the jitter of the beam respect to a specific facility sub-system (such as the PC laser or the RF accelerating voltage of a certain group of cavities)  $\sigma_{t_{b-j}}$  is:

$$\sigma_{t_{b-j}}^2 = (a_j - 1)^2 \sigma_{t_j}^2 + \sum_{i \neq j} a_i^2 \sigma_{t_i}^2$$

**EXAMPLE:** PC laser jitter  $\sigma_{t_{PC}} \approx 70 \text{ fs}$ , RF jitter  $\sigma_{t_{RF}} \approx 30 \text{ fs}$

No Compression:  $a_{PC} \approx 0.65$ ,  $a_{RF_{GUN}} \approx 0.35$

$$\sigma_{t_b} \approx 47 \text{ fs}$$

$$\sigma_{t_{b-PC}} \approx 27 \text{ fs}; \sigma_{t_{b-RF}} \approx 50 \text{ fs}$$

Magnetic Compression:  $a_{PC} \approx 0.2$ ,  $a_{RF_{boost}} \approx 0.8$

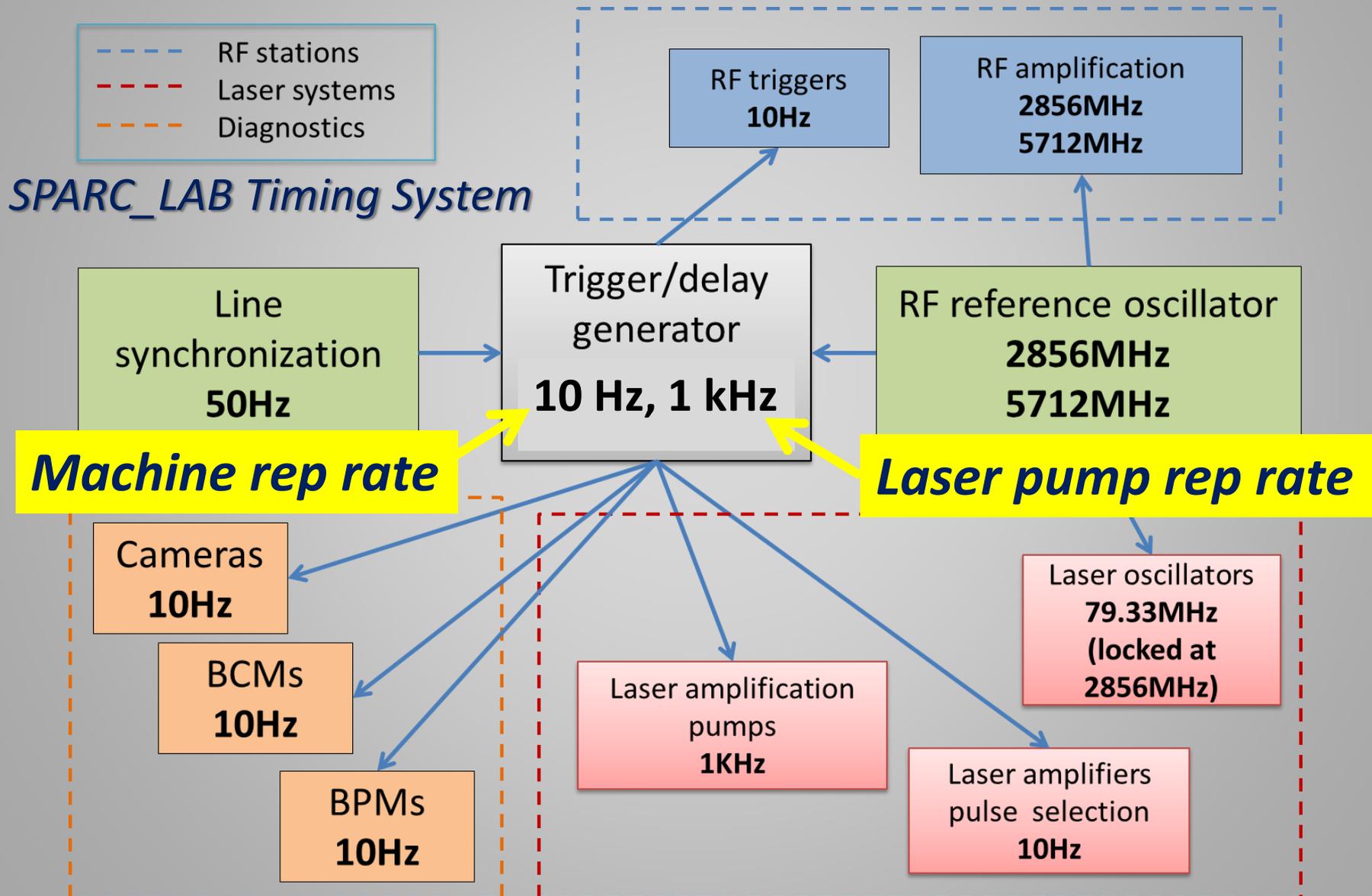
$$\sigma_{t_b} \approx 28 \text{ fs}$$

$$\sigma_{t_{b-PC}} \approx 61 \text{ fs}; \sigma_{t_{b-RF}} \approx 15 \text{ fs}$$

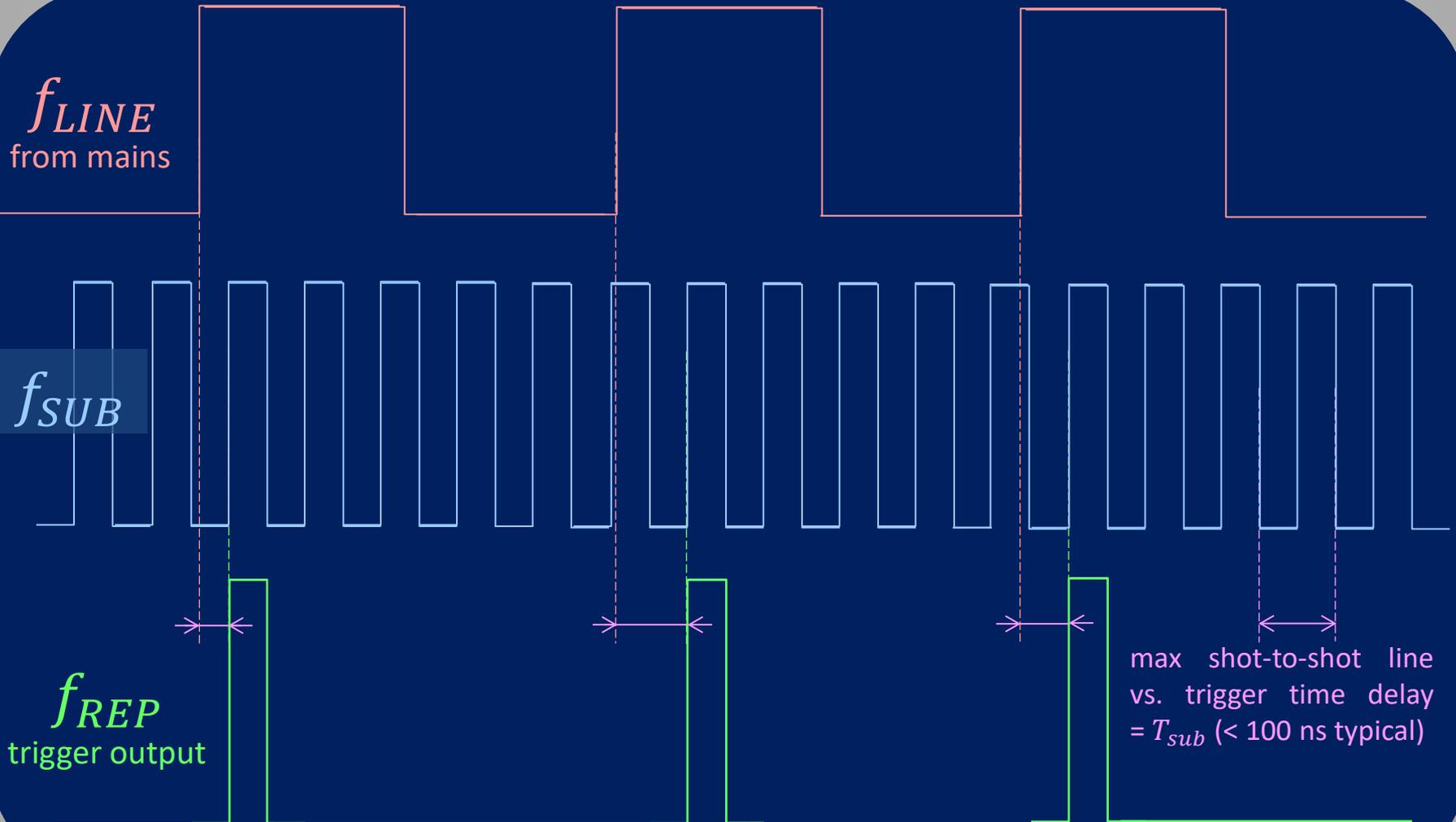
***GO TO ILC TDR  
EXAMPLE***

## ***TIMING***

- ***Generation of the main trigger signal***
- ***Analog vs. Digital distribution***
- ***An example of event sequence***



- The machine trigger generator is mainly a frequency divider
- Typically it divides one output of the RMO ( $f_{RMO}$ ) at different stages to generate all the desired sub-harmonics, down to a certain fundamental sub-multiple ( $f_{SUB}$ ). The resulting jitter is  $1\text{ps} \div 1\text{ns}$  depending of the divider stage
- It also takes the frequency of the mains (50 Hz) as input and generates a signal at the machine rep rate  $f_{REP}$  from it (either dividing or multiplying). We call it  $f_{LINE}$
- The final machine trigger is generated by changing the output logic state every first rising front of one  $f_{RMO}$  sub-harmonic ( $f_{SUB}$ ) after the  $f_{LINE}$  front (reducing magnet power supply current ripple)
- $f_{SUB}$  must preferably be an integer sub-multiple of all the system clocks (lasers rep. rate, ADC and DAC sample clocks, IF frequencies of downconverters, ...) to avoid trigger edge slippage/jumps



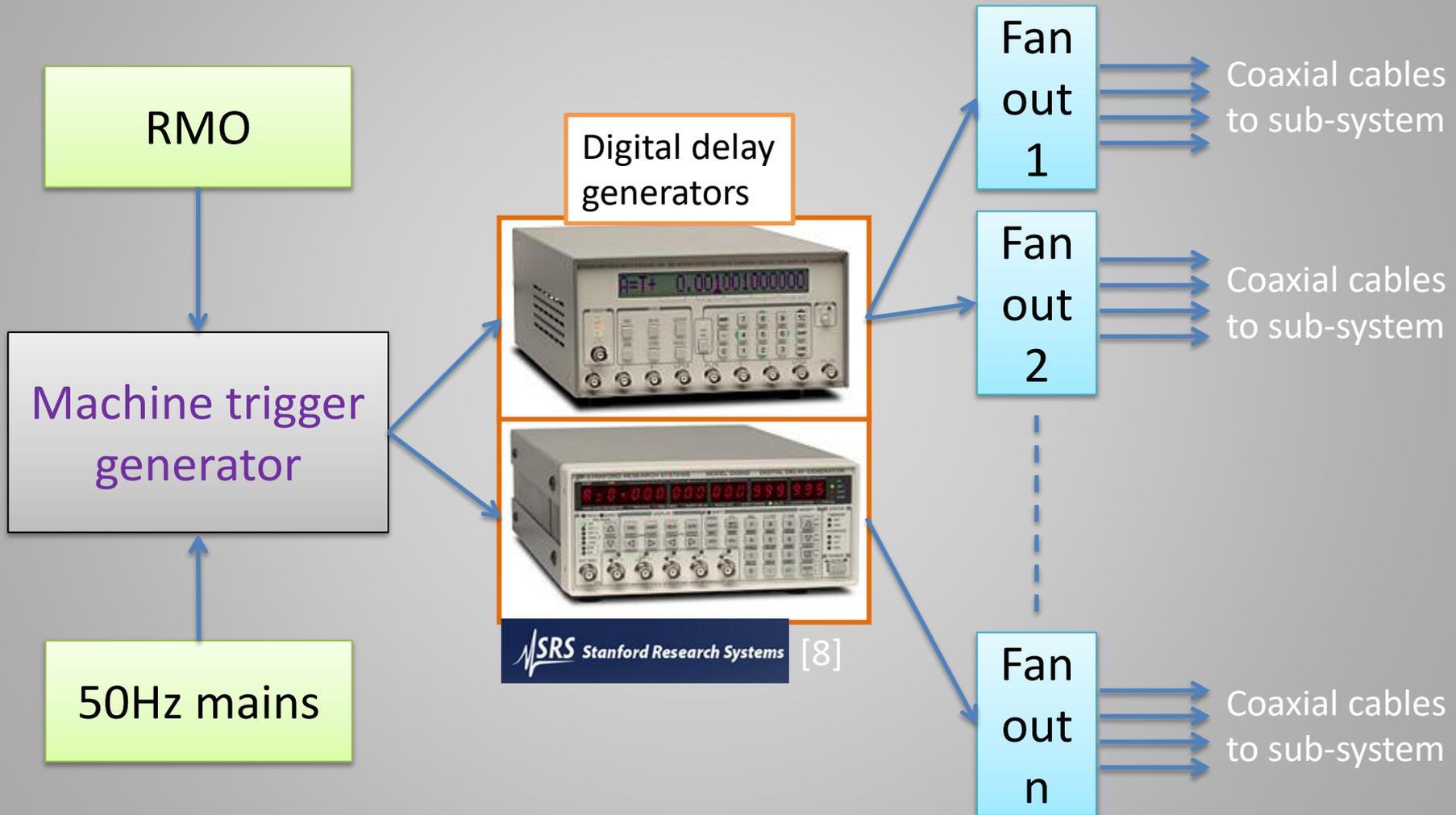
- The main trigger is then divided, delayed and distributed towards each subsystem
- Digital logic standards are commonly used (TTL, ECL, NIM, ...)
- The signal distribution can be analogic or digital

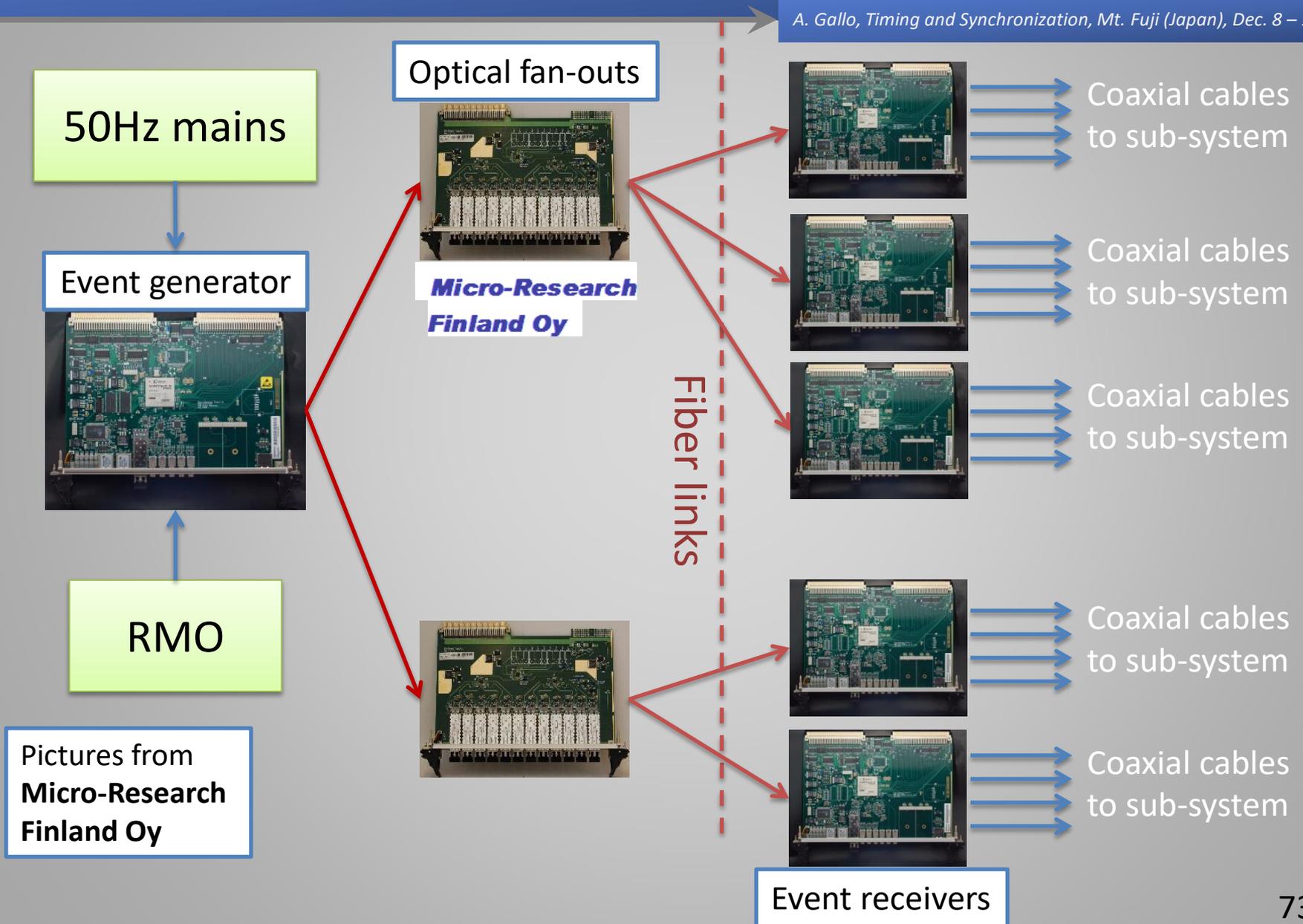
## Analog distribution

- Signal is distributed through coaxial cables ( $\approx 100$  m range)
- Commercial digital delay generators are used
- No advanced features can be implemented
- Simple design and control
- Low cost
- Limited length of cables

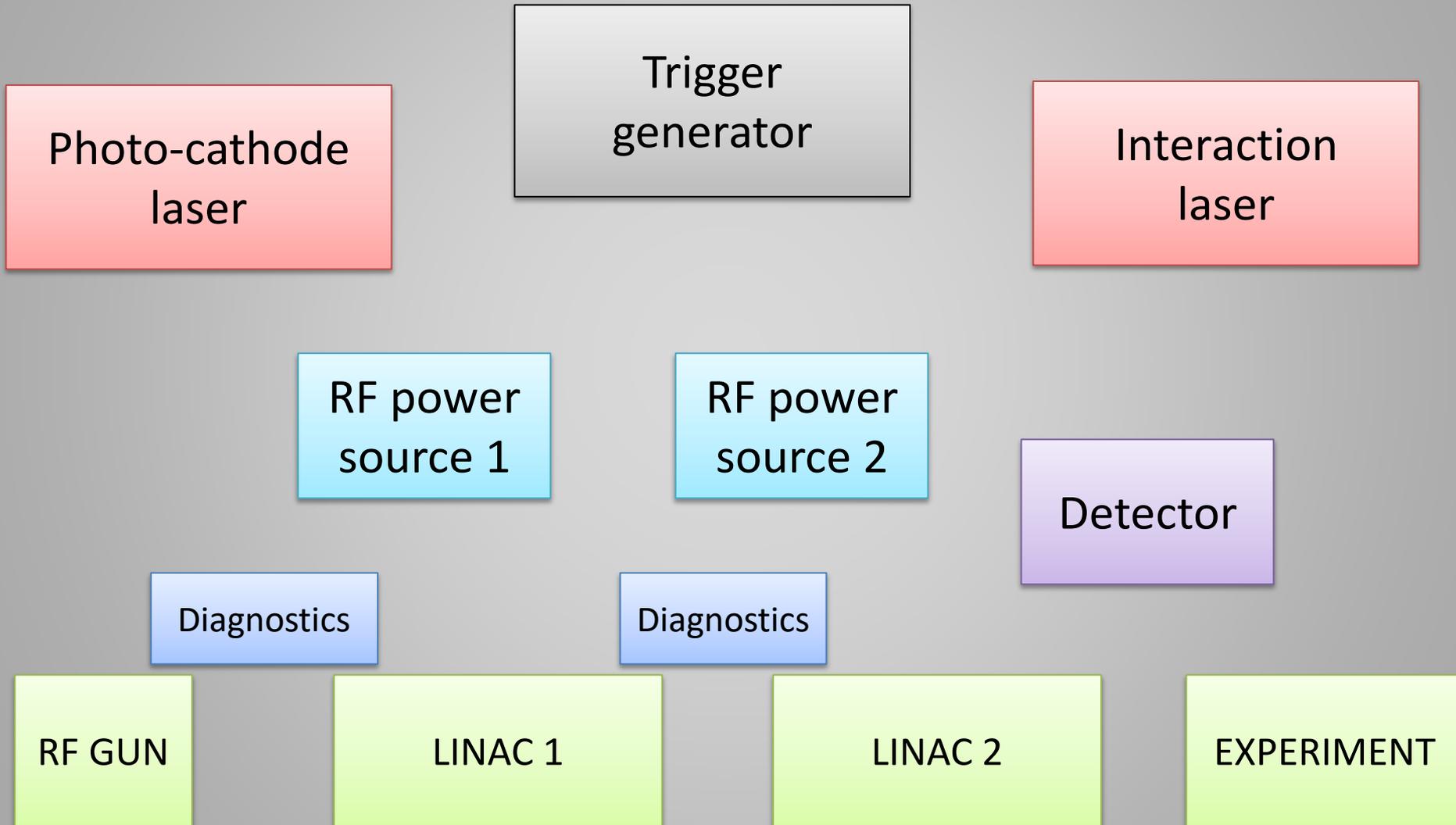
## Digital distribution

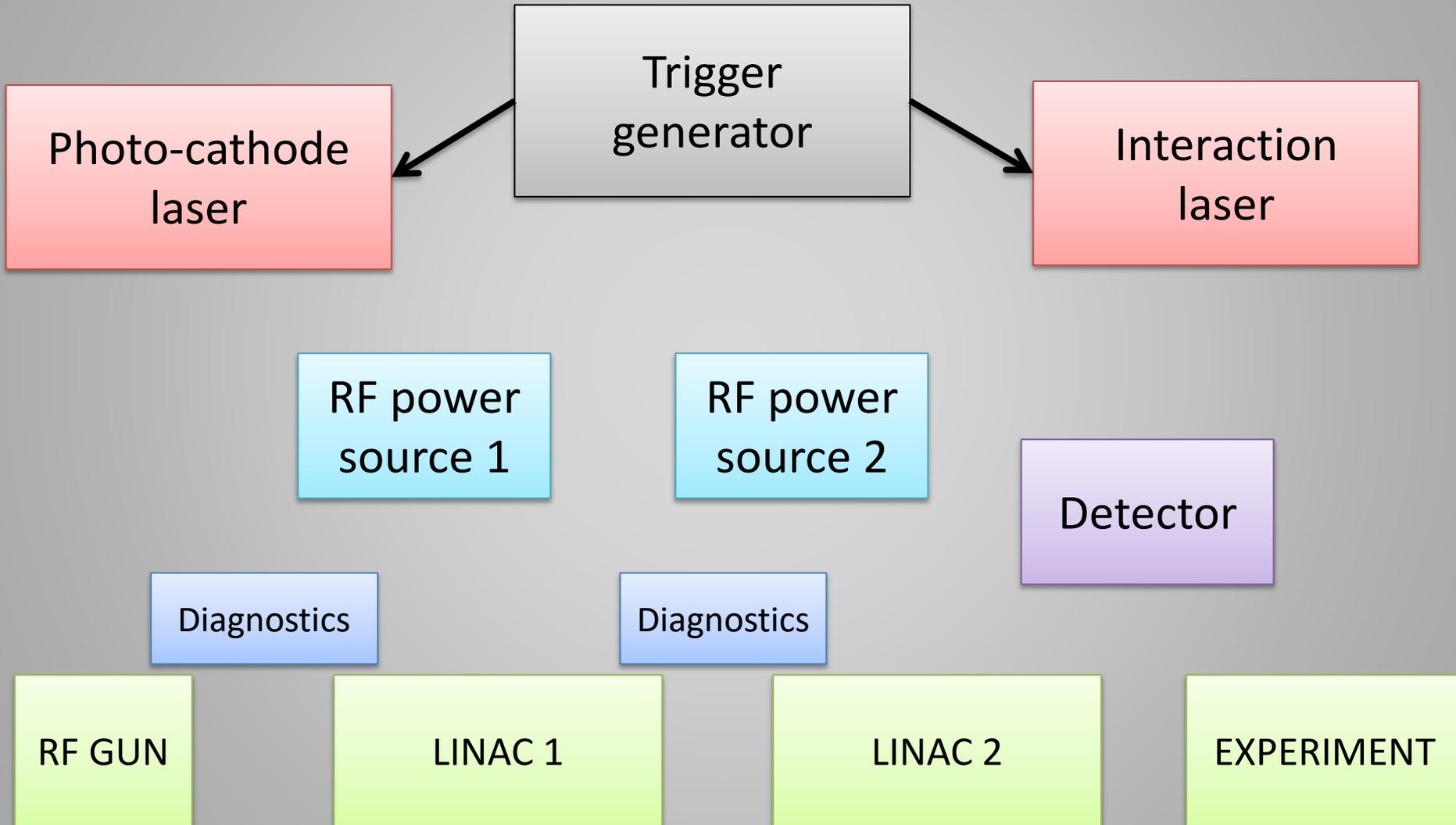
- Information packed according to a proper communication protocol
- Signal is preferably distributed through fiber links ( $\approx$  km range)
- Programmable event generator/receivers are used
- More flexible (locally delayed triggers, status word, diagnostics on system, ...)
- Higher cost, complex design
- Standard commercially available systems for accelerators





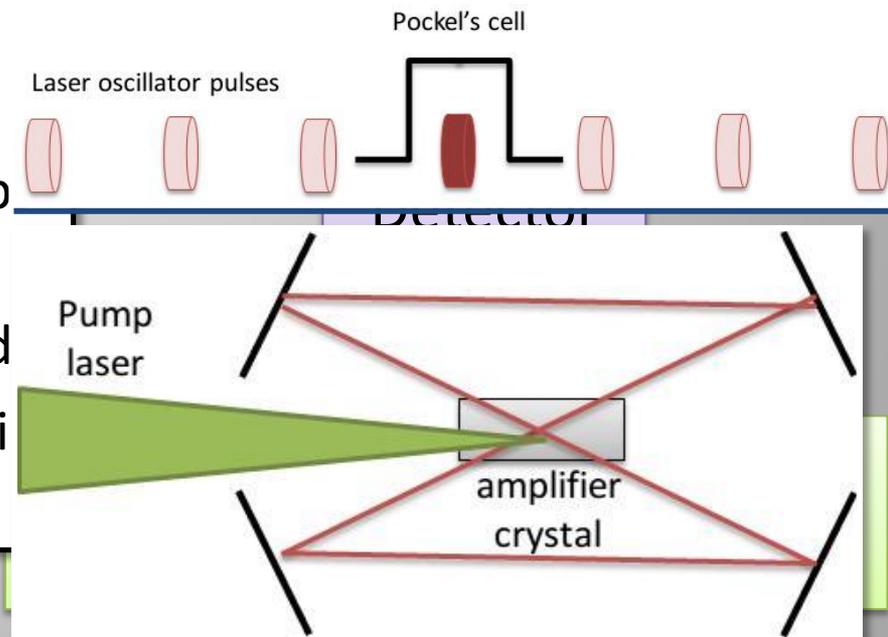
Pictures from  
**Micro-Research  
Finland Oy**

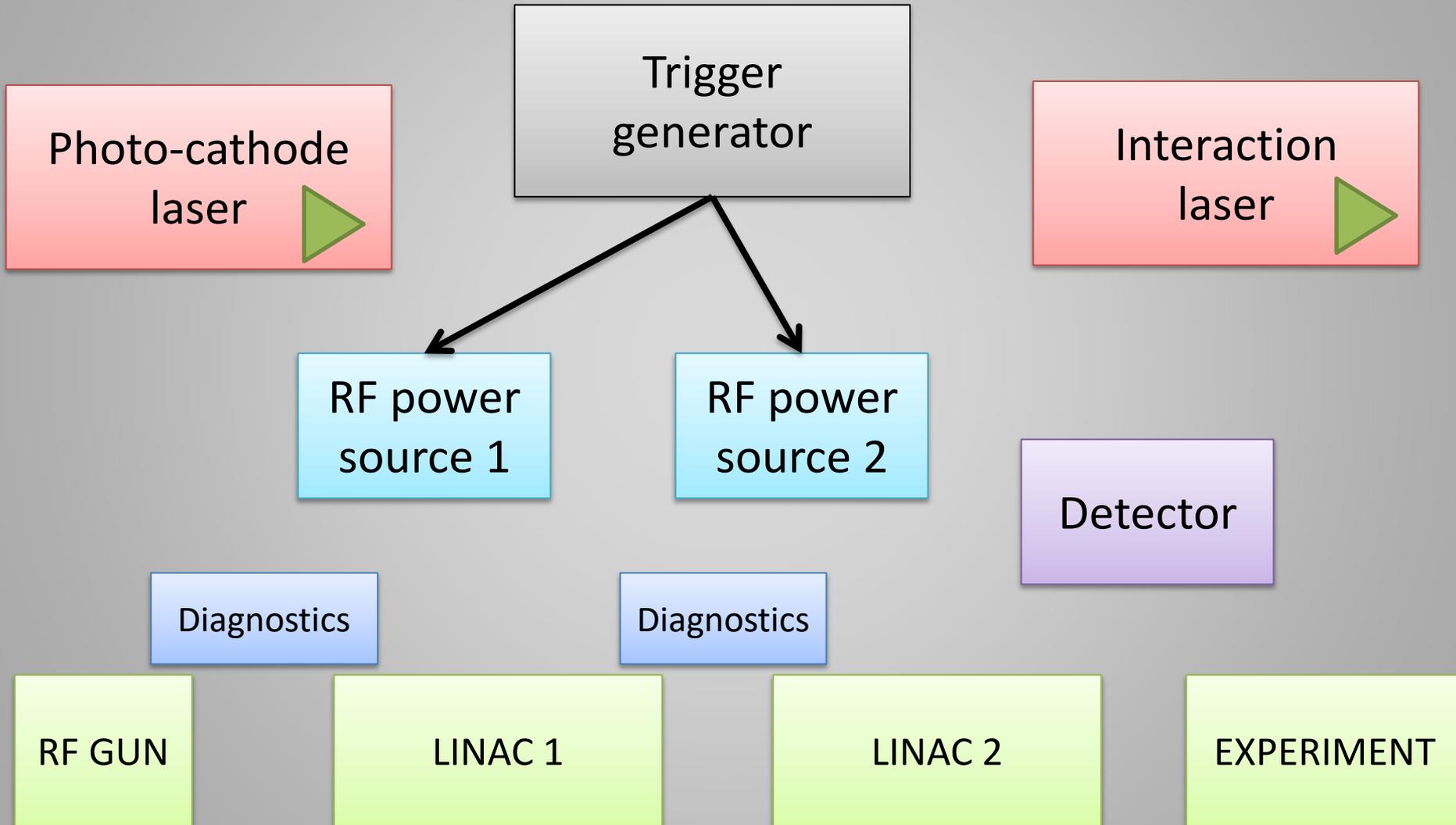


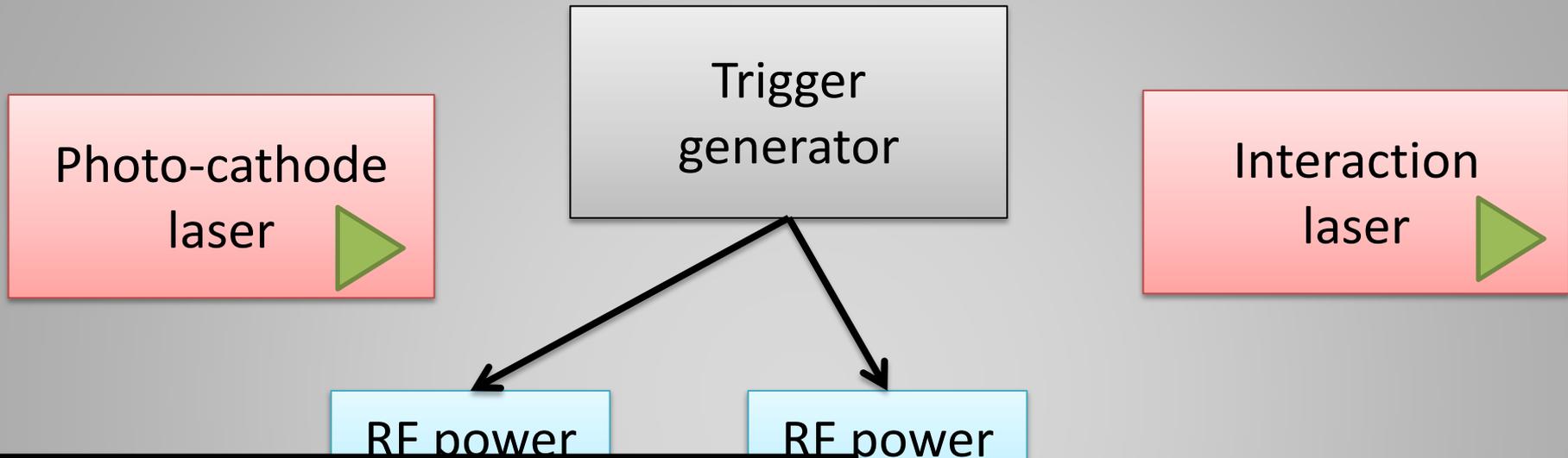




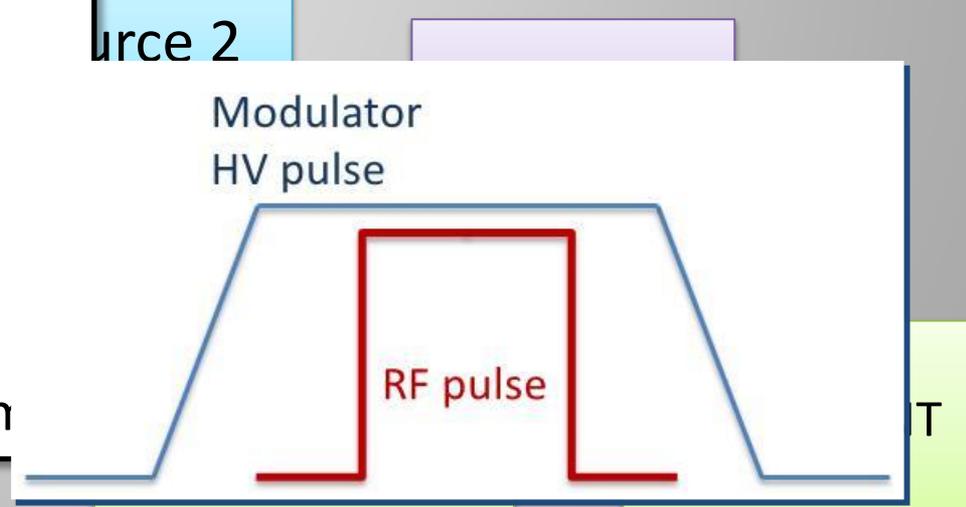
1. Trigger is sent to the laser systems
  1. Amplification chain starts
  2. Trigger signals are used for pulse pickers and optical amplifier pump
  3. Typically a multi-pass optical amplifier with a large delay is used
  4. Thus this has to be the first event in the sequence

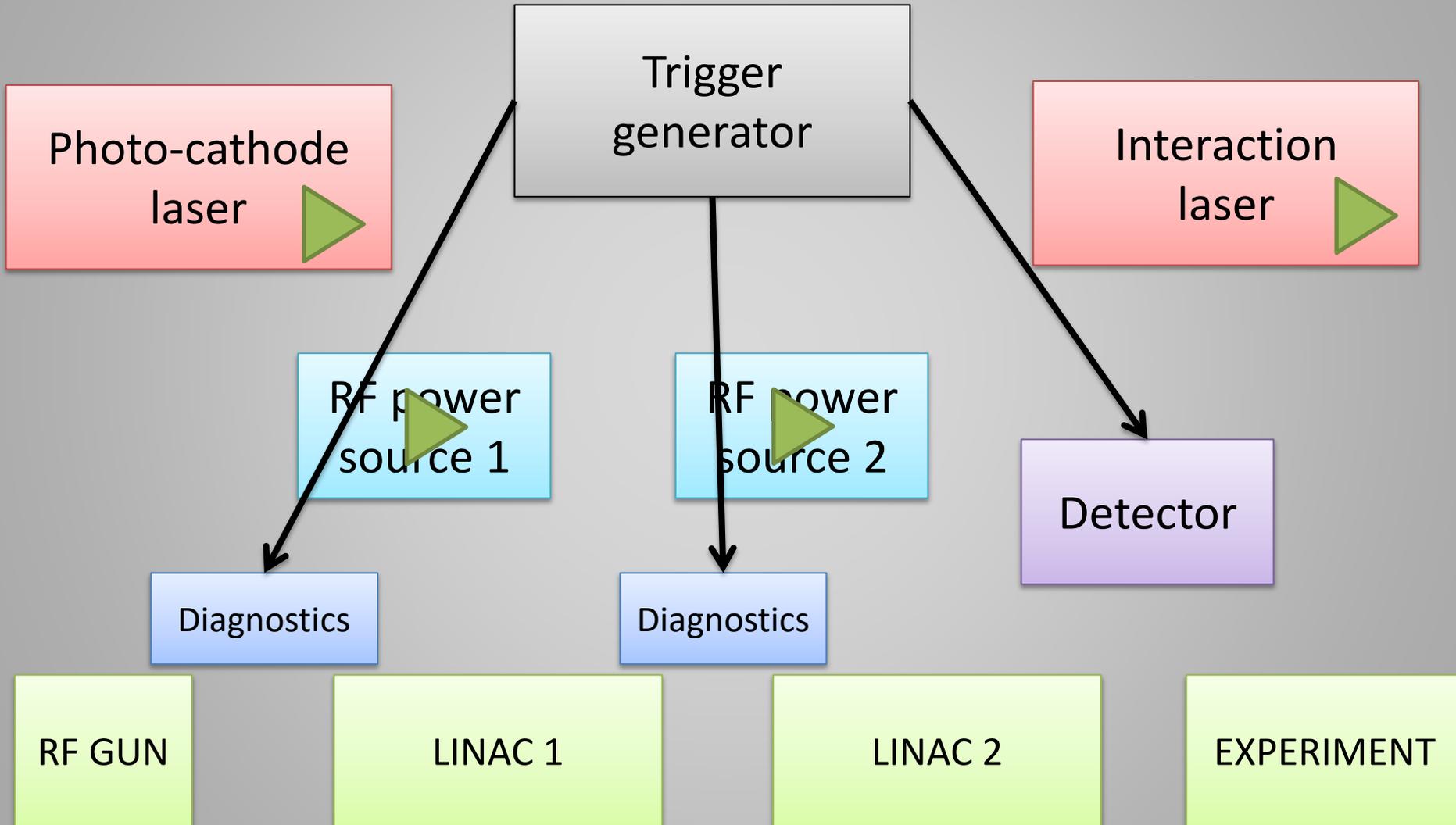


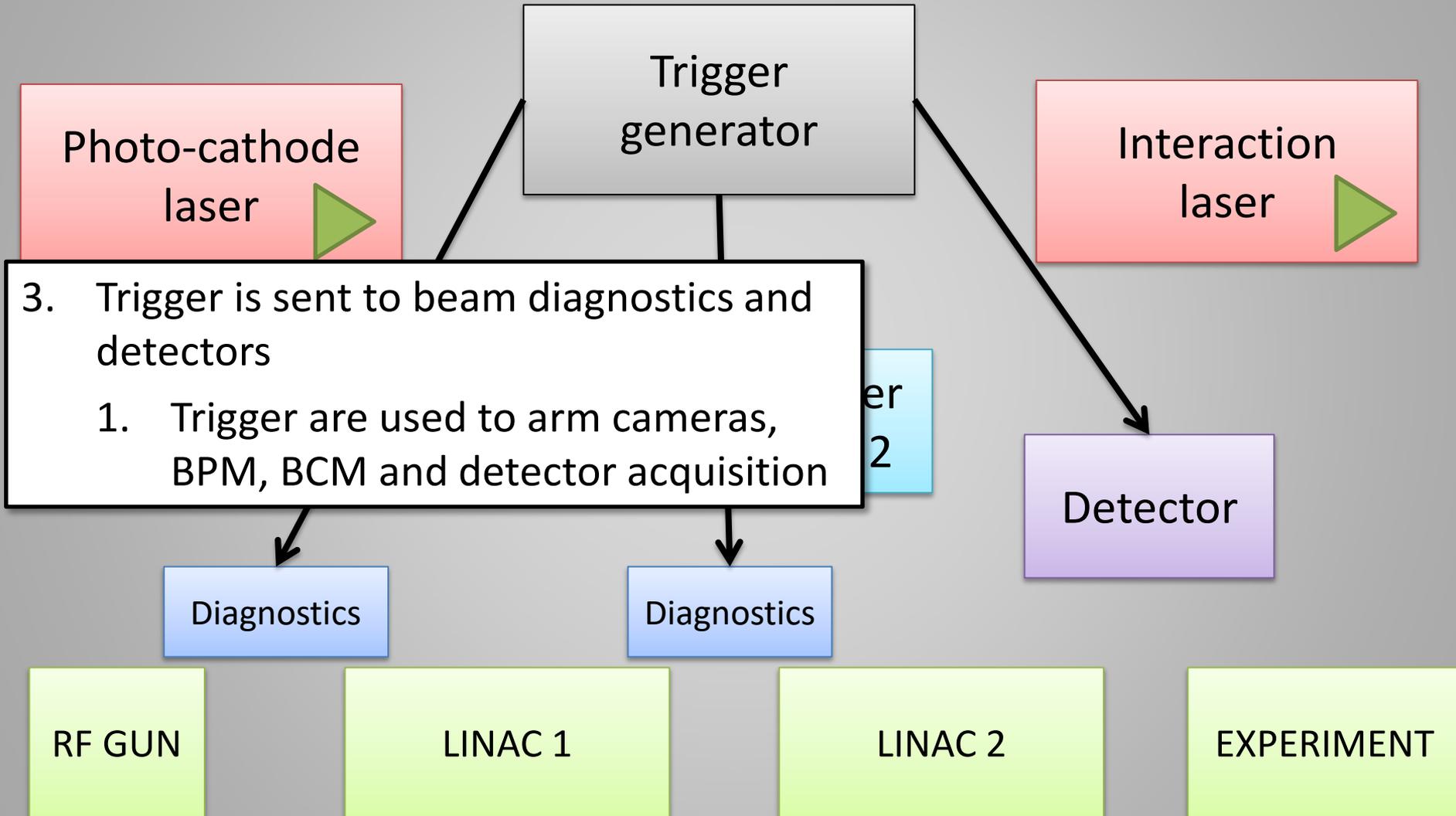




2. Trigger is sent to RF system
  1. Lasers are still running to prepare their outputs
  2. Triggers are used to start the modulator HV pulse forming and to trigger the LLRF system







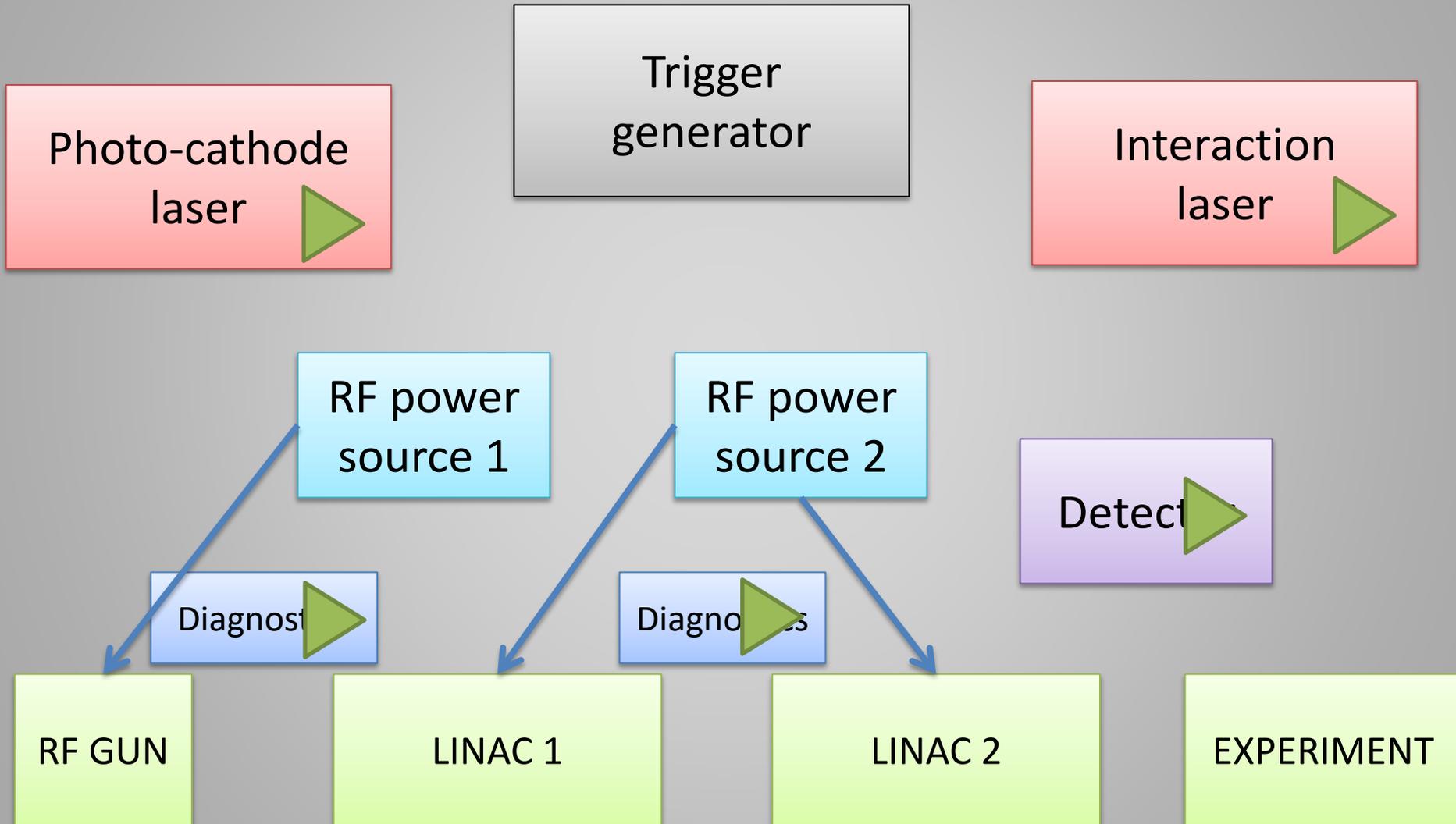
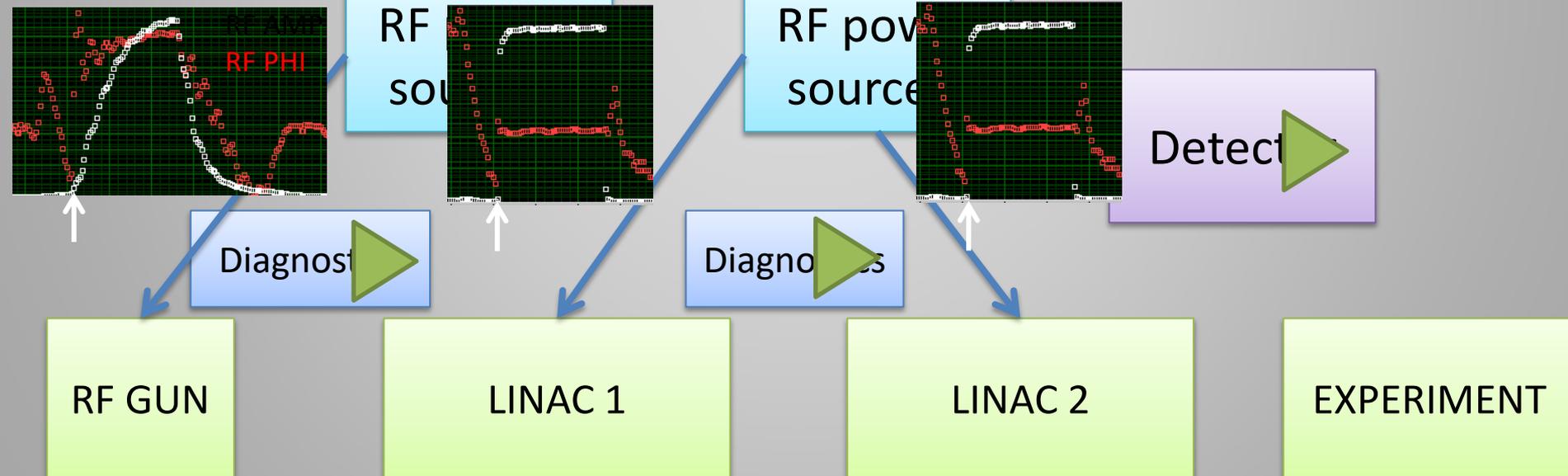


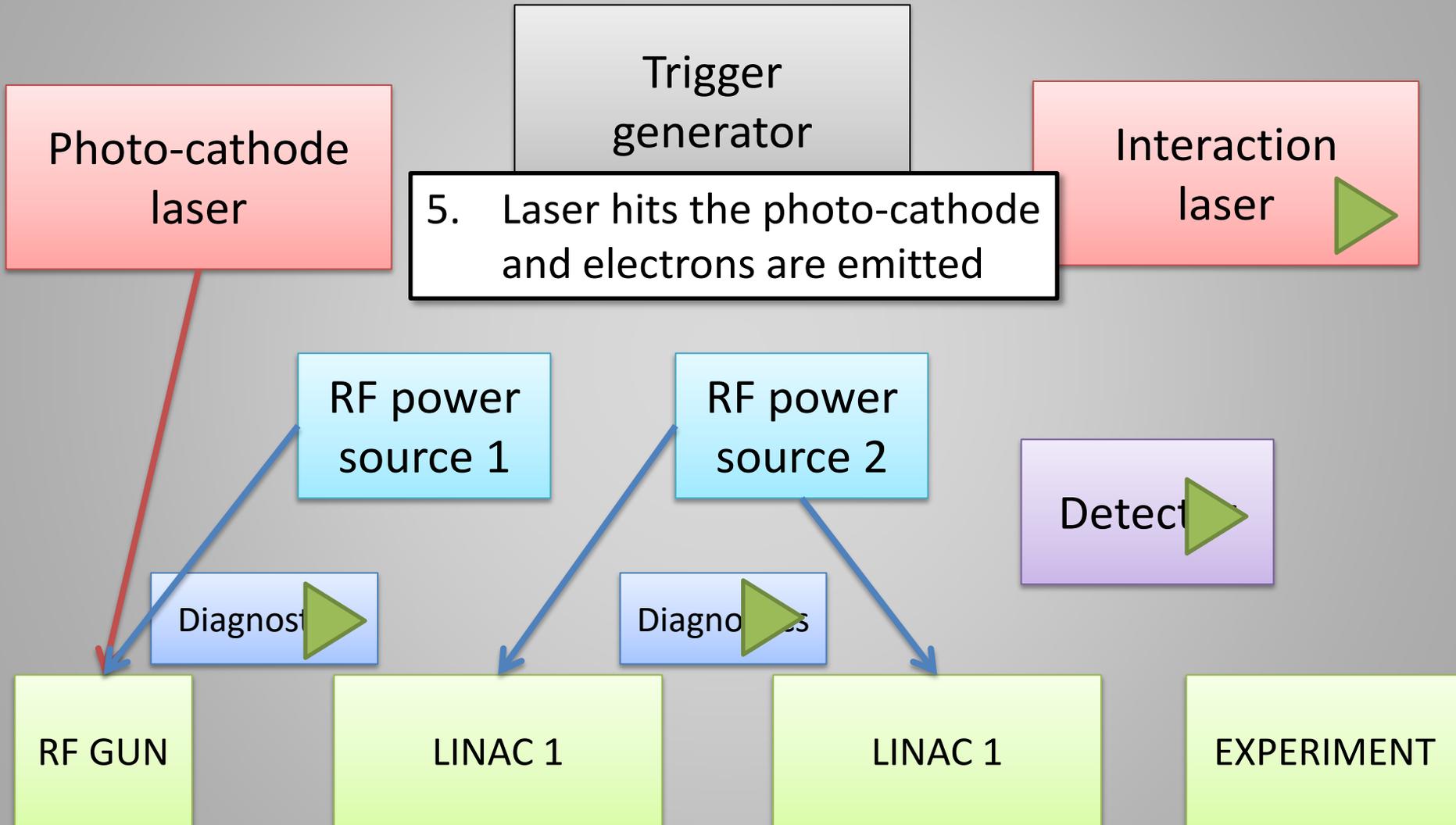
Photo-cathode  
laser

Trigger  
generator

Interaction  
laser

4. Start RF cavity feeding (filling time in  $\mu\text{s}$  scale)  
by starting the RF pulse in the power stations





- 5. Beam is accelerated
- 6. Diagnostics on beam

Trigger generator

Photo-cathode laser

Interaction laser

RF power source 1

RF power source 2

Detect

Diagnostics

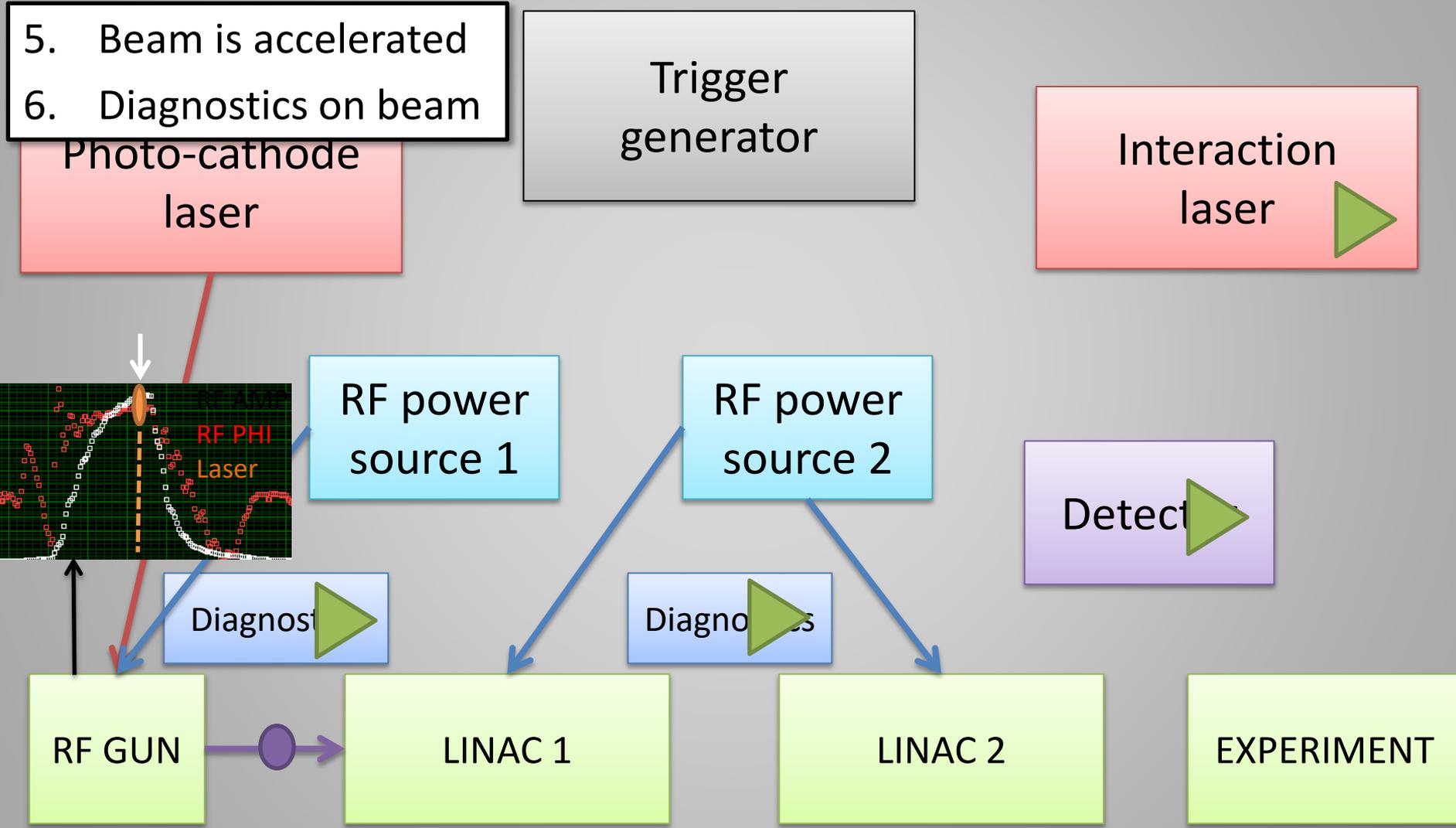
Diagnostics

RF GUN

LINAC 1

LINAC 2

EXPERIMENT



5. Laser hits the photo-cathode
6. Beam is accelerated
7. Diagnostics on beam

Trigger  
generator

Interaction  
laser

Laser

RF power  
source 1

RF power  
source 2

Detect

Diagnostics

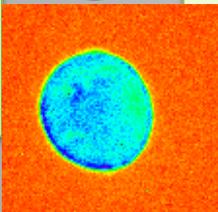
Diagnostics

RF GUN

LINAC 1

LINAC 2

EXPERIMENT

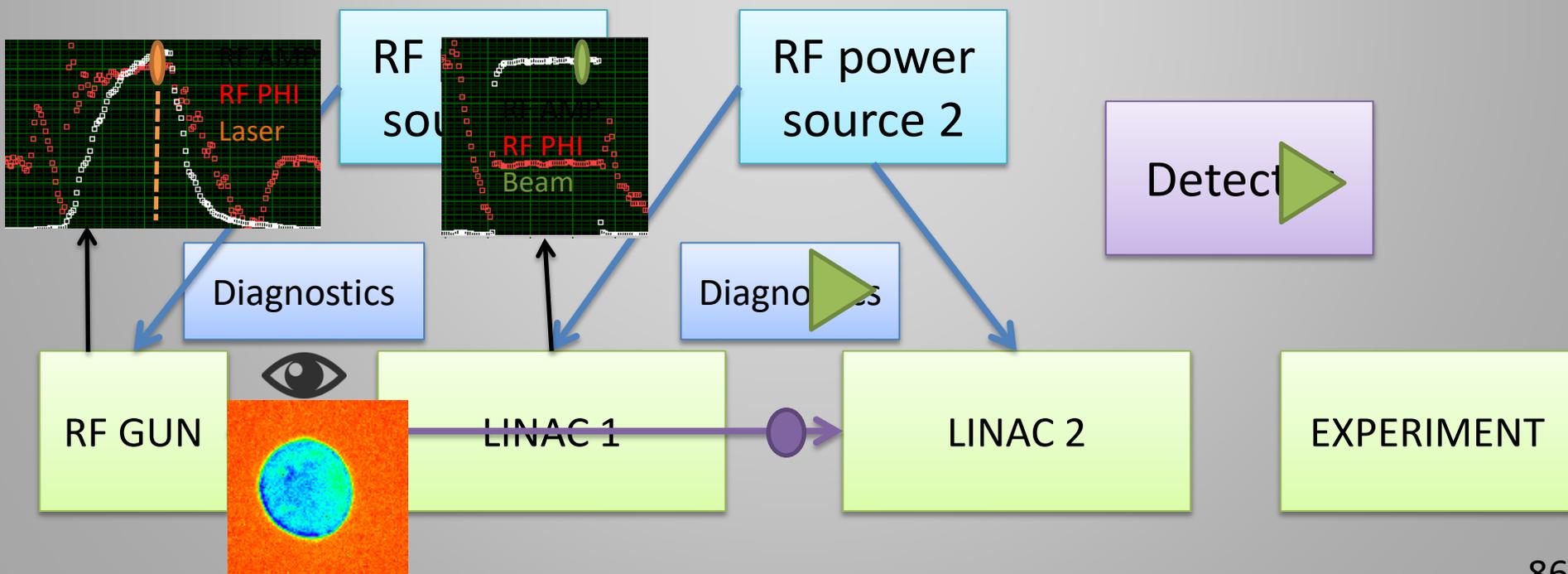


5. Laser hits the photo-cathode
6. Beam is accelerated
7. Diagnostics on beam

Trigger  
generator

Laser

Interaction  
laser



5. Laser hits the photo-cathode
6. Beam is accelerated
7. Diagnostics on beam

Trigger  
generator

Interaction  
laser

Laser

Detect

RF  
SOURCE

RF power  
source 2

Diagnostics

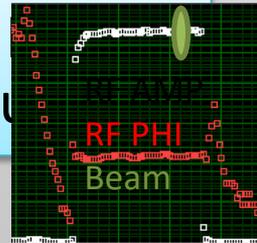
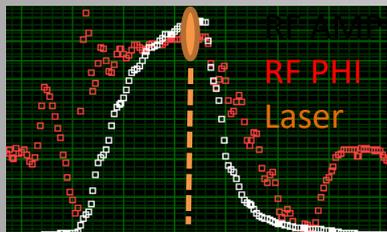
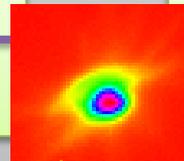
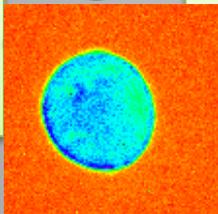
Diagnostics

RF GUN

LINAC 1

LINAC 1

EXPERIMENT



5. Laser hits the photo-cathode
6. Beam is accelerated
7. Diagnostics on beam

Trigger  
generator

Interaction  
laser

Laser

Detect

RF  
SOURCE

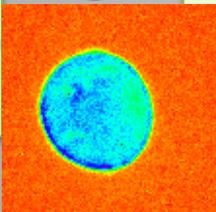
RF power  
source

Diagnostics

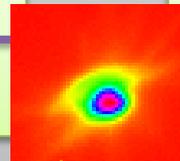
Diagnostics



RF GUN

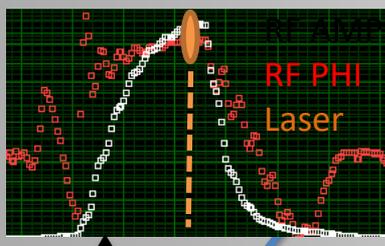
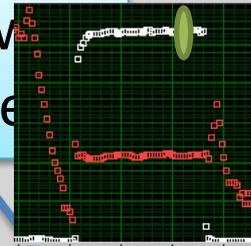
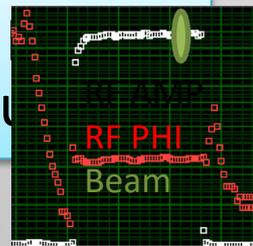


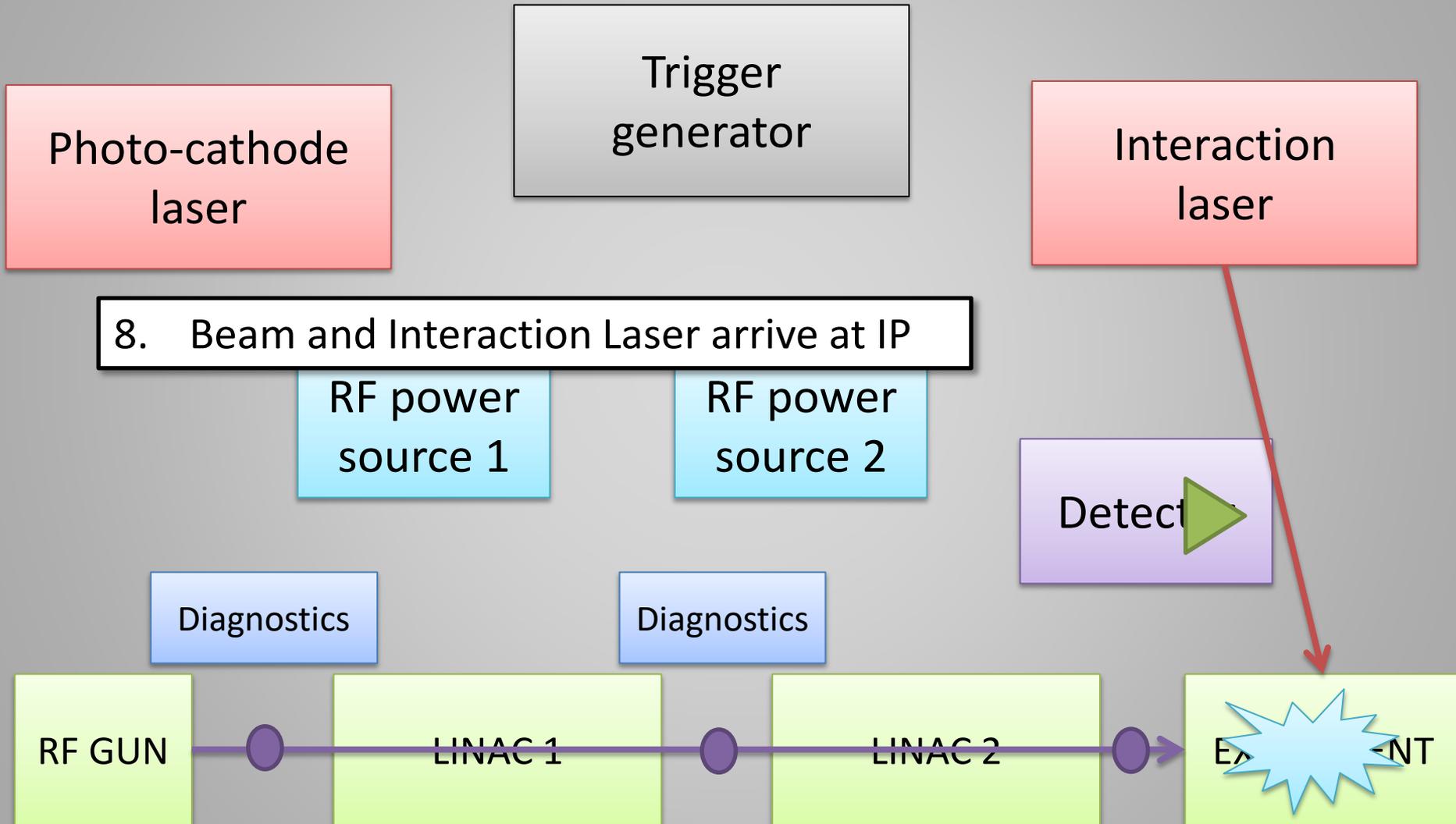
LINAC 1

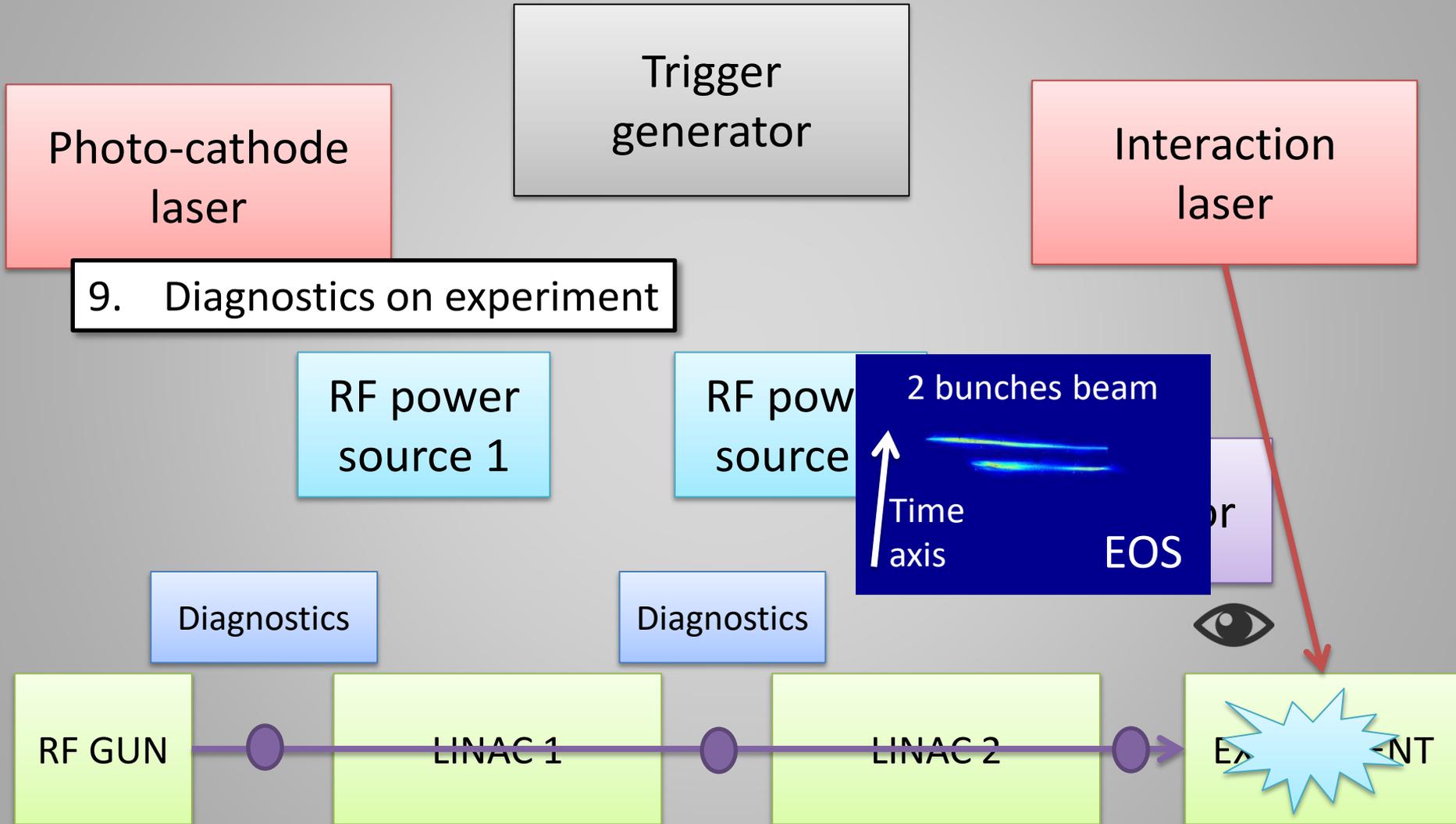


LINAC 2

EXPERIMENT







- ✓ Timing and Synchronization has growth considerably in the last ~ 15 years as a Particle Accelerators specific discipline
- ✓ It involves concepts and competences from various fields such as Electronics, RF, Laser, Optics, Control, Diagnostics, Beam dynamics, ...
- ✓ Understanding the real synchronization needs of a facility and proper specifications of the systems involved are crucial for successful and efficient operation (but also to avoid overspecification leading to extra-costs and unnecessary complexity ...)
- ✓ Synchronization diagnostics (precise arrival time monitors) is fundamental to understand beam behavior and to provide input data for beam-based feedback systems correcting synchronization residual errors
- ✓ Although stability down to the *fs* scale has been reached, many challenges still remain since requirements get tighter following the evolution of the accelerator technology. The battleground will move soon to the attosecond frontier ...

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- <http://www.onefive.com/ds/Datasheet%20Origami%20LP.pdf>
- E5052A signal source analyzer, <http://www.keysight.com/en/pd-409739-pn-E5052A/signal-source-analyzer-10-mhz-to-7-265-or-110-ghz?cc=IT&lc=ita>
- Menlo Systems GMBH: <http://www.menlosystems.com/products/?families=79>
- Andrew cables: [http://www.commscope.com/catalog/wireless/product\\_details.aspx?id=1344](http://www.commscope.com/catalog/wireless/product_details.aspx?id=1344)
- <http://www.nist.gov/>
- <http://www.thinksrs.com/index.htm>
- <http://www.mrf.fi/>
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